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Error Controls for Broadcast Communication Systems: An Integer Programming Approach to UEP Coding Scheme and A Deterministic Approach to Network Coding

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Error Controls for Broadcast Communication Systems: An Integer Programming
Approach to UEP Coding Scheme and A Deterministic Approach to Network Coding

A dissertation submitted in partial fulfillment of the requirements for the degree of
Doctor of Philosophy at George Mason University

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Dedication

I dedicate this dissertation to my parents, my wife, and my daughter.
Acknowledgments

First of all, I would like to express my heartfelt thanks to my advisor, Dr. Shih-Chun Chang who lead me to the field of coding theory and inspired me by showing his enthusiasms and ingenuity. This dissertation would not have been possible without his support, encouragement, guidance and persistent help.

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Abstract

ERROR CONTROLS FOR BROADCAST COMMUNICATION SYSTEMS: AN INTEGER PROGRAMMING APPROACH TO UEP CODING SCHEME AND A DETERMINISTIC APPROACH TO NETWORK CODING

Wook Jung, PhD
George Mason University, 2015
Dissertation Director: Dr. Shih-Chun Chang

Traditional network protocols employ error control techniques for reliable information dissemination over noisy communication channels. In this dissertation, two main topics are investigated for efficient error controls over a broadcast channel. First, unequal error protection (UEP) coding schemes for multiuser communications are investigated, and we propose integer programming approaches to UEP coding and decoding. Second, reliable packet transmissions over a single-hop broadcast network are considered, and we propose a unified solution to use a deterministic network coding for a packet retransmission scheme and a packet-level forward error correction scheme.

For multiuser communications over a broadcast channel, integer programming approaches are introduced to the construction and the decoding of a binary linear UEP code. First, optimal UEP codes are constructed from integer programming for maximum efficiency, and lower bounds of UEP codes are derived to show the efficiency. Then, performance of the UEP coding scheme for multiuser communications are analyzed on a degraded broadcast channel. Finally, a decoding method of the binary UEP code is proposed by using iterative integer programming and majority logic. By presenting numerical results, examples, and
comparisons, we demonstrate that the UEP coding scheme effectively provides efficient forward error correction for multiuser broadcast communications.

For reliable packet transmissions over a single-hop broadcast network, we propose packet-level error control schemes by using a deterministic linear network coding. We first construct a deterministic network code based on Reed-Solomon (RS) code. Then, we provide an adaptive way to apply the deterministic network code for both retransmissions and forward error corrections by puncturing the RS code. Numerical analysis and simulations are performed to show the efficiency of the error control schemes.
Chapter 1: Introduction

Error controls for communication network over a noisy channels are classified into two categories:

1. Forward error correction (FEC) scheme that corrects channel errors by using error correcting codes; or,

2. Automatic repeat request (ARQ) scheme that recovers erroneous or lost information by retransmissions based on feedback.

In this dissertation, we investigate both FEC and ARQ schemes for reliable communications over a broadcast channel.

For the forward error correction, a communication system usually employs conventional error correcting codes that have equal error protection capability. However, when multiple users communicate over a noisy channel, each user is likely to have unequal errors on the received information. An unequal error protection (UEP) coding scheme provides more efficient error controls for the communication system than the conventional coding scheme.

When information has different significance, whether it is a bit or groups of bits, unequal error protection (UEP) codes separate the information and provide different levels of error protection. The notion of a UEP code was first introduced by Masnick and Wolf in [1]. Since then, construction methodologies of UEP codes have been actively studied in many coding theory papers. A majority of the linear UEP code constructions are based on combining shorter length linear codes. In this dissertation, unlike those approaches, we propose a construction methodology of optimal UEP codes for broadcast communications based on integer programming. We also propose a decoding methodology of the UEP codes based on integer programming and majority logic.
Furthermore, consider packet transmissions over a broadcasting network that a single source has data packets to transmit to all receivers within its broadcasting range. One can consider the broadcasting source as an access point (AP) in wireless network and each receiver as a mobile station as depicted in Figure 1.1. Because of uncertainty of the broadcast channel, traditional network protocols employ error controls (either FEC scheme or ARQ scheme) for reliability of packet deliveries.

The packet retransmission scheme requires a feedback channel to receive packet error/loss information. The broadcasting source first collects acknowledgments of the transmitted packets (ACK/NACK) from its receivers through the feedback channel, then the source retransmits packets based on the acknowledgments. On the other hand, the forward error correction scheme does not require the feedback channel. Instead the forward error correction scheme adds redundancy into transmitting packets to ensure that an intended receiver can recover packets without requesting retransmissions when packet errors occur during transmission.

Since Ahlswede et al. introduced the concept of a network coding in [2], which allows to process packets at a network node, there have been some studies to apply the network coding concept into reliable packet transmissions. Our research investigates the methodologies of network coding for reliable packet transmissions and provides a unified solution based on linear network coding for both a retransmission scheme and a packet-level forward error correction scheme on a single-hop wireless broadcast network.
1.1 Contributions

The contributions of this dissertation can be categorized into two parts.

Unequal error protection coding and decoding by integer programming for broadcast channels

1. An integer programming approach is introduced to construct optimal UEP codes for multiuser communication over a broadcast channel.

   - An integer programming problem is formulated based on unequal error protection requirements of multiple users to construct an optimal binary UEP code.
   - An integer programming bound and an asymptotically achievable code rate are derived to show efficiency of the integer programming approach.
   - Performance analysis of the UEP coding scheme is presented for multiuser communications over a degraded broadcast channel.

2. A decoding algorithm is developed for the UEP codes based on iterative integer programming and majority logic.

Reliable packet transmission on single-hop broadcast networks using deterministic network coding

1. A methodology of deterministic linear network coding is investigated based on a punctured Reed-Solomon (RS) code.

2. A unified solution is provided for efficient reliable packet transmissions on a single-hop broadcast network:

   - A packet retransmission scheme (ARQ scheme) based on deterministic network coding.
   - A packet-level forward error correction scheme (FEC scheme) based on deterministic network coding.
1.2 Outline

The organization of this dissertation is as follows. First, Chapter 2 provides background and a literature review. Next, in Chapter 3, we propose an integer programming approach to construct binary UEP codes, and we provide an integer programming bound and numerical results that show the constructed UEP codes are optimal. Based on the bound, we illustrate asymptotic code rates with comparisons to throughput of the broadcast channel, and we also measure bit error performance of the UEP coding scheme on a degraded broadcast channel. Moreover, we present an iterative decoding method by using integer programming and majority logic. Then, in Chapter 4, we construct a deterministic linear network code from Reed-Solomon codes, and we present a unified solution based on the deterministic network coding for both a retransmission scheme and a packet-level forward error correction scheme on a single-hop wireless broadcast network. We also provide numerical analysis and simulation results to show the efficiency of the schemes. At the end of both Chapter 3 and Chapter 4, we discuss limitations and brief research directions. Finally, Chapter 5 presents a summary and future developments.
Chapter 2: Background and related works

2.1 Unequal error protection codes

The concept of unequal error protection (UEP) codes was first introduced by Masnick and Wolf in [1]. Consider a coded communication system depicted in Figure 2.1. Let $C$ be a binary linear code that protects a message vector $m = (m_1, m_2, \ldots, m_k)$ sent over a noisy channel,

$$C = \{c \mid c = mG, \ m \in \{0,1\}^k\}$$

where $G$ is a $k \times n$ generator matrix. Suppose that the code $C$ protects each message $m_i$ against $t_i$ channel errors for $1 \leq i \leq k$. For a conventional $t$-error correcting code, $t_i = t$ for $1 \leq i \leq k$. However, if $t_i \neq t_j$ for $1 \leq i \neq j \leq k$, the code $C$ has an unequal error protection capability, and it is called an unequal error protection code.

In [3], Dunning and Robbins introduced the notion of a separation vector which specifies the unequal error protection capability of a UEP code.

**Separation vector** For a binary linear $(n, k)$ code $C$, a separation vector $s = (s_1, s_2, \ldots, s_k)$ is defined as

$$s_i = \min \{w_H(mG) \mid m_i \neq 0\} \quad \text{for} \quad 1 \leq i \leq k. \quad (2.1)$$

where $w_H(\cdot)$ denotes the Hamming weight.

It follows from the definition that a message bit $m_i$ can be separated and protected against up to $\left\lfloor \frac{s_i - 1}{2} \right\rfloor$ channel errors for a given separation vector $s = (s_1, s_2, \ldots, s_k)$. Suppose that each message $m_i$ requires $t_i$ unequal error protection for $1 \leq i \leq k$. Then, a linear
code $C$ can satisfy the requirements if its separation vector $s = (s_1, s_2, \ldots, s_k)$ satisfies

$$s_i \geq 2t_i + 1 \quad \text{for} \quad 1 \leq i \leq k.$$

Earlier works on UEP codes [1, 3–5] have mainly focused on establishing theoretical foundations. Particularly, we are interested in bounds on lengths of UEP codes derived in [1, 5] since the bounds shall be compared to the lengths of UEP codes that we construct in Section 3. Masnick and Wolf have derived an upper bound of a UEP code in [1], and we rewrite the upper bound for a binary UEP code in the following.

**Upper bound** When a message $m_i$ is protected against $t_i$ errors for $1 \leq i \leq k$, an upper bound of a binary UEP code can be given by

$$n \leq k + r_U$$

where $r_U$ is the smallest number of check bits $r$ such that

$$2^r > \sum_{i=0}^{2t_k-1} \binom{n-1}{i} - \sum_{i=2}^{k} \binom{n-1-\Xi_i}{2t_i-2} - \sum_{i=2}^{k} \binom{n-1-\Xi_i}{2t_i-1}$$

(2.3)

when $\Xi_i$ is the number of message bits that are protected against $i$-bit or more errors (See [1, pp. 606–607] for the derivation).

On the other hand, van Gils has derived a lower bound on lengths of UEP codes for a non-increasing separation vector (i.e., $s_i \geq s_j$ for $1 \leq i \neq j \leq k$) in [5], and we rewrite the lower bound for a binary UEP code in the following.
**Lower bound** When a message $m_i$ is protected against $t_i$ errors and a non-decreasing separation vector is given as $s_i = 2t_i + 1$ for $1 \leq i \leq k$ (i.e., $t_i \geq t_j$ for $1 \leq i \neq j \leq k$), a lower bound of a binary UEP code can be given by

$$n \geq \sum_{i=1}^{k} \left\lceil \frac{s_i}{2^{t_i+1}} \right\rceil$$

(2.4)

(See [5, pp. 869–870] for the derivation).

In [1, pp. 603–604], Masnick and Wolf have also presented a binary UEP code construction method. However, it has been claimed by the authors that the optimal code construction becomes difficult for large dimensions (beyond $k = 5$). This observation motivates us to develop an integer programming approach to construct optimal UEP codes.

Since the pioneering work of Masnick and Wolf, constructions of UEP codes have been actively studied, and most construction methods of linear UEP codes are based on combining (e.g., direct sum, $|u|u + v$, concatenation, etc.) shorter length linear codes as presented in [4, 6–11]. Also there have been studies that investigate information theoretic features of UEP codes [12, 13] and studies that combines UEP coding and modulation for unequal error protection [14–19]. Furthermore, linear network coding has been applied for unequal error protection in [20–25].

### 2.2 Degraded broadcast channels

The notion of a broadcast channel was introduced by Cover in [26]. When $k$ users are simultaneously communicated through a broadcast channel, the channel can be described by a single input (denoted by $S$) and multiple outputs (denoted by $T_i$ for $1 \leq i \leq k$) as depicted in Figure 2.2.

In [27], Bergmans introduced the notion of degraded broadcast channels by decomposing a broadcast channel into multiple degraded component channels. Let $CH_i$ denote component channels and let $D_i$ be artificial channels that represent degradation for $1 \leq i \leq k$.
Figure 2.2: Broadcast channel with a channel input $S$ and channel outputs $T_i$ for $1 \leq i \leq k$.

where $CH_1 = D_1$. If a channel $CH_j$ is represented by the cascade of $CH_i$ and $D_j$, then the channel $CH_j$ is a degraded version of the channel $CH_i$ where $j = i + 1$ for $2 \leq j \leq k$ and the broadcast channel is called degraded (Figure 2.3 [27]).

By using the decomposed channel model (Figure 2.3), the error characteristics of the degraded broadcast channel can be described with $k$ cascaded binary symmetric channels (BSCs) with transition probabilities $\alpha_i \in [0, \frac{1}{2}]$ as shown in Figure 2.4 [27]. Let $p_i$ denote the bit error probability of the each component channel, then

$$p_1 = \alpha_1,$$

$$p_2 = \alpha_1 (1 - \alpha_2) + (1 - \alpha_1) \alpha_2 = p_1 (1 - \alpha_2) + (1 - p_1) \alpha_2,$$

$$p_3 = (1 - \alpha_1)(1 - \alpha_2)\alpha_3 + (1 - \alpha_1)\alpha_2 (1 - \alpha_3) + \alpha_1 (1 - \alpha_2)(1 - \alpha_3) + \alpha_1 \alpha_2 \alpha_3$$

$$= \{\alpha_1 (1 - \alpha_2) + (1 - \alpha_1) \alpha_2\} (1 - \alpha_3) + \{1 - \alpha_1 (1 - \alpha_2) - (1 - \alpha_1) \alpha_2\} \alpha_3$$

$$= p_2 (1 - \alpha_3) + (1 - p_2) \alpha_3,$$

$$\vdots \quad \vdots$$
Similarly, the bit error probability of each component channel can be written by

\[ p_i = p_{i-1}(1 - \alpha_i) + (1 - p_{i-1})\alpha_i \quad \text{for} \quad 1 \leq i \leq k \]  

(2.5)

where \( p_0 = 0 \).

Let \( \Gamma_i \) represent an information rate for each component channel \( CH_i \) for \( 1 \leq i \leq k \), then the throughput rate of the degraded broadcast channel, \( R_T \) can be given by

\[ R_T = \sum_{i=1}^{k} \Gamma_i = \Gamma_1 + \Gamma_2 + \cdots + \Gamma_k, \]  

(2.6)

and the throughput rate is upper bounded by the capacity of channel \( CH_1 \).

Since the notion of degraded broadcast channel was introduced in [27], information theoretic features (e.g., coding theorem or capacity region) of the degraded broadcast channel
have been studied in [28–34].

2.3 Linear (Integer) programming

*Linear programming* is an optimization method to find a minimum or maximum of a linear function (objective function) subject to certain linear equations or inequalities. If the variables of the objective function are restricted to be integers, then the linear programming is called an *integer programming*.

A typical linear programming problem is formulated as the following [35–37]:

Minimize or maximize

\[ f_1 x_1 + f_2 x_2 + \cdots + f_n x_n \]

subject to

\[
egin{align*}
  a_{11} x_1 + a_{12} x_2 + \cdots + a_{1n} x_n & \overset{\geq}{=} b_1 \\
  a_{21} x_1 + a_{22} x_2 + \cdots + a_{2n} x_n & \overset{\leq}{=} b_2 \\
  \vdots & \vdots \\
  a_{m1} x_1 + a_{m2} x_2 + \cdots + a_{mn} x_n & \overset{\geq}{=} b_m 
\end{align*}
\]

where

\[ x_j \geq 0 \quad \text{for} \quad 1 \leq j \leq n \]

The function \( f_1 x_1 + f_2 x_2 + \cdots + f_n x_n \) is an *objective function* to linearly optimize and the variables \( x_1, x_2, \ldots, x_n \) are called *decision variables*. If the decision variables are strictly
integers, then the optimization refers to an integer programming. If some of the decision variables are restricted to be integers, then the optimization refers to a mixed integer programming. Based on the formulated problem, a linear programming solver provides a feasible solution for the decision variables \( x_j \) for \( 1 \leq j \leq n \) that satisfy all linear constraints, and the best feasible solution is called an optimal solution.

Linear (integer) programming has been applied to coding theory for obtaining bounds on lengths of linear codes ([38, Ch. 17, p. 537]), but mostly it has been used for alternative methods to decode linear codes [39–51].

As an example, we provide the concept of an integer programming approach for maximum likelihood decoding. Consider a communication system where a codeword \( c \) of a binary linear code \( C \) is transmitted over a noisy channel as depicted in Figure 2.1. At the receiving end of the coded system, a decoder tries to recover \( \hat{m} \) from the received \( r = (r_1, r_2, \ldots, r_n) \) such that \( \hat{m} = m \). A decoding rule of a maximum likelihood decoder is to find a particular codeword \( x = (x_1, x_2, \ldots, x_n) \) that maximizes \( \Pr(x|r) \). Assuming that all codewords of \( C \) are equally likely and the channel is memoryless [52, Ch. 1], it is equivalent to minimizing \( \sum_{j=1}^{n} \gamma_j x_j \) where

\[
\gamma_j = \log \left( \frac{\Pr(r_j|x_j = 0)}{\Pr(r_j|x_j = 1)} \right). 
\]

Then, the ML decoder can determine that the transmitted codeword \( c \) is the codeword \( x \) that has the minimum sum of \( \sum_{j=1}^{n} \gamma_j x_j \). Let \( H \) be a parity check matrix of the linear code \( C \). Then an integer programming problem for the ML decoding can be formulated as

minimize

\[
\sum_{j=1}^{n} \gamma_j x_j
\]

subject to
Figure 2.5: The butterfly network: network coding on multicast

\[ \mathbf{Hx}^T = \mathbf{0} \quad \text{over} \quad \mathbb{GF}(2) \]

where

\[ x_j \in \{0, 1\} \quad \text{for} \quad 1 \leq j \leq n. \]

2.4 Network coding

The concept of network coding was first introduced by Ahlswede et al. [2]. In their work, Ahlswede et al. have showed that coding at network nodes is necessary in multicast connection for optimal utilization. Figure 2.5 shows an example of network coding in a multicast network.

With network coding, unlike the traditional store and forward packet-switching, a network node not just forwards packets but also combines packets before transmitting. This new concept in communication networks has been proposed as a promising solution in a wide range of areas such as network throughput improvement, network resource utilization, security, and so on. A simple example of benefit of network coding in terms of wireless
resource utilization is shown in Figure 2.6. Compared to the “without network coding” scenario (Figure 2.6 (a)) which requires three time slots to exchange packets, network coding allows an exchange of packets in two time slots by processing packets in an intermediate node (Figure 2.6 (b)).

In the early stage of network coding, research has focused on theoretical foundations [53–60]. Li et al [53] and Koetter and Médard [54] have provided the concept of linear network coding, and Ho et al [59] have introduced the concept of random network coding in a multicast packet network. With the random network coding, a network node transmits linearly encoded packets with randomly chosen coding coefficients from a large enough finite field.

Along with the development of the theoretical frameworks on network coding, researches to practically implement the network coding concept have been made. Chou et al. [61] provided a practical and a distributed approach to apply random network coding into traditional packet networks by injecting the encoding information (i.e., coding coefficients) in the packet header so that receivers can decode the packet. Katti et al. [62] developed another practical approach to apply network coding using XOR to encode packets at wireless nodes.
2.5 Packet retransmissions using network coding

Network coding has been adopted to provide reliable communications over lossy packet networks. Coding schemes and forward error corrections using network coding have been discussed in [63–69]. Additionally, a couple of studies have shown packet retransmission schemes using network coding on a single-hop wireless broadcast network [70, 71]. In those retransmission schemes, network coding is deployed for retransmitting packets at a broadcasting source to reduce the number of retransmissions.

Traditional retransmission scheme (ARQ) retransmits unsuccessfully delivered packets based on feedbacks (ACK/NACK) from receivers. Nguyen et al. [70] uses XOR-based network coding to retransmit packets, i.e., a broadcasting source performs XOR operation on retransmission packets based on the feedbacks from its receivers. Xiao et al. [71] uses random network coding instead of XOR based network coding, i.e., a broadcasting source encodes retransmission packets with randomly chosen coding coefficients from a large enough finite field of $\mathbb{GF}(q = 2^m)$ (e.g., $\mathbb{GF}(2^8)$) and injects its encoding information in the packet header.

We consider the following communication scenario over a single-hop wireless broadcast network to compare the number of retransmissions among a traditional ARQ, XOR based retransmission scheme, and random network coding based retransmission scheme.

- A single source broadcasts packets to all receivers within its broadcast range, and every receiver wants to receive all packets from the source.
- Each receiver sends feedback to the source whether it has successfully received packets or not.
- The broadcasting source retransmits packets based on the feedbacks.

An example of the collected feedbacks at the broadcasting source listed in Table 2.1 after transmitting 4 packets, $p_1$, $p_2$, $p_3$, and $p_4$ to receivers, $R_1$, $R_2$, $R_3$, and $R_4$. 


Table 2.1: Example of feedbacks: the symbol ‘o’ represents a successfully delivered packet and symbol ‘x’ represents a lost packet at each receiver.

<table>
<thead>
<tr>
<th>receiver</th>
<th>p1</th>
<th>p2</th>
<th>p3</th>
<th>p4</th>
</tr>
</thead>
<tbody>
<tr>
<td>R₁</td>
<td>o</td>
<td>o</td>
<td>x</td>
<td>x</td>
</tr>
<tr>
<td>R₂</td>
<td>x</td>
<td>x</td>
<td>o</td>
<td>o</td>
</tr>
<tr>
<td>R₃</td>
<td>o</td>
<td>x</td>
<td>o</td>
<td>x</td>
</tr>
<tr>
<td>R₄</td>
<td>o</td>
<td>x</td>
<td>x</td>
<td>o</td>
</tr>
</tbody>
</table>

**Traditional ARQ scheme** Since none of the 4 packets is received successfully at all 4 receivers simultaneously, the broadcasting source has to retransmit all 4 packets to receivers. Let \( q₁, q₂, q₃, \) and \( q₄ \) be the retransmission packets, then

\[
qᵢ = pᵢ \quad \text{for} \quad 1 ≤ i ≤ 4.
\]

**XOR-based retransmission scheme** If XOR operation is allowed for retransmission, the number of retransmissions can be reduced to 3 encoded packets. Let \( q₁, q₂, \) and \( q₃ \) be the retransmission packets, then

\[
q₁ = p₁ ⊕ p₃, \quad q₂ = p₂, \quad \text{and} \quad q₃ = p₄.
\]

At the receiving end, every receiver can recover its lost packets using XOR operation (See Figure 2.7). For example, since the receiver \( R₂ \) has already successfully received \( p₃ \) from the previous transmission, the lost packets, \( p₁ \) and \( p₂ \) can be recovered from

\[
p₁ = q₁ ⊕ p₃ = (p₁ ⊕ p₃) ⊕ p₃,
\]

\[
p₂ = q₂.
\]

**Retransmission scheme based on random network coding** Suppose that a broadcasting source can linearly encode packets with coding coefficients. Since the packet loss pattern in Table 2.1 shows that every receiver wants to receive two out of four
packets, two linearly combined retransmission packets, $q_1$ and $q_2$ will be enough for all receivers to recover their lost packets:

$$q_1 = \alpha_1 p_1 + \alpha_2 p_2 + \alpha_3 p_3 + \alpha_4 p_4$$

$$q_2 = \beta_1 p_1 + \beta_2 p_2 + \beta_3 p_3 + \beta_4 p_4$$

where $\alpha_1, \alpha_2, \alpha_3, \alpha_4$ and $\beta_1, \beta_2, \beta_3, \beta_4$ are coding coefficients over a certain finite field. If the source linearly combines packets with proper coding coefficients and if all receivers know what coding coefficients are used to combine the retransmitted packets,
linear operation at $R_1$: \[
\begin{pmatrix}
\alpha_3 & \alpha_4 \\
\beta_3 & \beta_4
\end{pmatrix}
\begin{pmatrix}
p_3 \\
p_4
\end{pmatrix}
= \begin{pmatrix}
q_1 \\
q_2
\end{pmatrix}
+ \begin{pmatrix}
\alpha_1 & \alpha_2 \\
\beta_1 & \beta_2
\end{pmatrix}
\begin{pmatrix}
p_1 \\
p_2
\end{pmatrix}
\]

linear operation at $R_2$: \[
\begin{pmatrix}
\alpha_1 & \alpha_2 \\
\beta_1 & \beta_2
\end{pmatrix}
\begin{pmatrix}
p_1 \\
p_2
\end{pmatrix}
= \begin{pmatrix}
q_1 \\
q_2
\end{pmatrix}
+ \begin{pmatrix}
\alpha_3 & \alpha_4 \\
\beta_3 & \beta_4
\end{pmatrix}
\begin{pmatrix}
p_3 \\
p_4
\end{pmatrix}
\]

linear operation at $R_3$: \[
\begin{pmatrix}
\alpha_2 & \alpha_3 \\
\beta_2 & \beta_3
\end{pmatrix}
\begin{pmatrix}
p_2 \\
p_3
\end{pmatrix}
= \begin{pmatrix}
q_1 \\
q_2
\end{pmatrix}
+ \begin{pmatrix}
\alpha_1 & \alpha_4 \\
\beta_1 & \beta_4
\end{pmatrix}
\begin{pmatrix}
p_1 \\
p_4
\end{pmatrix}
\]

linear operation at $R_4$: \[
\begin{pmatrix}
\alpha_2 & \alpha_3 \\
\beta_2 & \beta_3
\end{pmatrix}
\begin{pmatrix}
p_2 \\
p_3
\end{pmatrix}
= \begin{pmatrix}
q_1 \\
q_2
\end{pmatrix}
+ \begin{pmatrix}
\alpha_1 & \alpha_4 \\
\beta_1 & \beta_4
\end{pmatrix}
\begin{pmatrix}
p_1 \\
p_4
\end{pmatrix}
\]

Figure 2.8: Retransmissions with random network coding
receivers can recover their lost packets by solving linear equations (See Figure 2.8).

For example, since $R_3$ already successfully received $p_1$ and $p_3$ from the previous packet transmissions, the receiver $R_3$ can recover $p_2$ and $p_4$ by solving the following linear equations:

$$
\begin{pmatrix}
  \alpha_2 & \alpha_4 \\
  \beta_2 & \beta_4
\end{pmatrix}
\begin{pmatrix}
  p_2 \\
  p_4
\end{pmatrix}
= 
\begin{pmatrix}
  q_1 \\
  q_2
\end{pmatrix}
+ 
\begin{pmatrix}
  \alpha_1 & \alpha_3 \\
  \beta_1 & \beta_3
\end{pmatrix}
\begin{pmatrix}
  p_1 \\
  p_3
\end{pmatrix},
$$

hence,

$$
\begin{pmatrix}
  p_2 \\
  p_4
\end{pmatrix}
= 
\begin{pmatrix}
  \alpha_2 & \alpha_4 \\
  \beta_2 & \beta_4
\end{pmatrix}^{-1}
\begin{pmatrix}
  q_1 \\
  q_2
\end{pmatrix}
+ 
\begin{pmatrix}
  \alpha_1 & \alpha_3 \\
  \beta_1 & \beta_3
\end{pmatrix}
\begin{pmatrix}
  p_1 \\
  p_3
\end{pmatrix}.
$$
Chapter 3: UEP coding schemes for broadcast channels

A multiuser communication system over a broadcast channel is depicted in Figure 3.1. Due to the inequality of errors that the broadcast channel introduces, each user requires a different level of error protection denoted by

\[ t = (t_1, t_2, \ldots, t_k) \quad \text{for} \quad 1 \leq i \leq k. \]  

(3.1)

For a message vector \( \mathbf{m} = (\mathbf{m}_1, \mathbf{m}_2, \ldots, \mathbf{m}_k) \) whose element \( \mathbf{m}_i \) represents a \( l \)-bit message of each user,

\[ \mathbf{m}_i = (m_1^{(i)}, m_2^{(i)}, \ldots, m_l^{(i)}) \quad \text{for} \quad 1 \leq i \leq k, \]

a binary UEP code \( C \) with a generator matrix \( \mathbf{G} \) can be represented as

\[ C = \left\{ \mathbf{mG} \mid \mathbf{m} = (\mathbf{m}_1, \mathbf{m}_2, \ldots, \mathbf{m}_k), \mathbf{m}_i \in \{0,1\}^l \quad \text{for} \quad 1 \leq i \leq k \right\}. \]

As defined in [3], the unequal error protection capability of the code can be specified by its separation vector denoted by \( \hat{s} = (\hat{s}_1, \hat{s}_2, \ldots, \hat{s}_k) \) where

\[ \hat{s}_i = \min \{ w_H (\mathbf{mG}) \mid \mathbf{m}_i \neq \mathbf{0} \} \quad \text{for} \quad 1 \leq i \leq k. \]  

(3.2)

where \( w_H(\cdot) \) denotes the Hamming weight. If the separation vector satisfies

\[ \hat{s}_i \geq 2t_i + 1 \quad \text{for} \quad 1 \leq i \leq k, \]  

(3.3)

then the UEP code can correct up to \( t_i \) errors and recover the \( l \)-bit message \( \hat{\mathbf{m}}_i = \mathbf{m}_i \) for each user.
Suppose that the unequal error protection requirement from each user is given as a separation vector $s = (s_1, s_2, \ldots, s_k)$ such that

$$s_i = 2t_i + 1 \quad \text{for } 1 \leq i \leq k.$$  \hfill (3.4)

Then, by using integer programming, our objective is to construct a binary UEP code whose separation vector $\hat{s}$ satisfies

$$\hat{s}_i \geq s_i \quad \text{for } 1 \leq i \leq k,$$  \hfill (3.5)

i.e.,

$$\min \{ w_H (mG) \mid m_i \neq 0 \} \geq s_i \quad \text{for } 1 \leq i \leq k.$$  \hfill (3.6)

In addition, we develop a decoding algorithm by using integer programming such that each receiver $R_i$ recovers the message $m_i$ when the broadcast channel introduces less than or equal to $t_i$ errors.
3.1 Integer programming approach to UEP coding scheme for single-bit messages

In this section, we limit our scope to the case of single-bit message for each user, i.e., \( m_i = m_i \) where \( m_i \in \{0, 1\} \) for \( 1 \leq i \leq k \).

3.1.1 UEP code constructions using integer programming

First of all, a separation vector which specifies the unequal error protection requirement of each user is defined as the following:

**Definition 3.1** (Non-decreasing separation vector). A separation vector \( s = (s_1, s_2, \ldots, s_k) \) is defined for unequal error protection as in non-decreasing order, i.e.,

\[
  s_i \leq s_j \quad \text{for} \quad 1 \leq i < j \leq k. \tag{3.7}
\]

Let \( A_b \) be a \( k \times (2^k - 1) \) matrix consisting of all nonzero binary \( k \)-tuples as columns in increasing order,

\[
  A_b = \begin{bmatrix}
    a_{1,1} & a_{1,2} & \cdots & a_{1,2^k-1} \\
    a_{2,1} & a_{2,2} & \cdots & a_{2,2^k-1} \\
    \vdots & \vdots & \ddots & \vdots \\
    a_{k,1} & a_{k,2} & \cdots & a_{k,2^k-1}
  \end{bmatrix} = \begin{bmatrix}
    a_1 \\
    a_2 \\
    \vdots \\
    a_k
  \end{bmatrix} \tag{3.8}
\]

\[
  = \begin{bmatrix}
    0 & 0 & 0 & \cdots & 0 & 1 & \cdots & 1 & 1 \\
    0 & 0 & 0 & \cdots & 1 & 0 & \cdots & 1 & 1 \\
    \vdots & \vdots & \vdots & \ddots & \vdots & \vdots & \ddots & \vdots & \vdots \\
    0 & 1 & 1 & \cdots & 1 & 0 & \cdots & 1 & 1 \\
    1 & 0 & 1 & \cdots & 1 & 0 & \cdots & 0 & 1
  \end{bmatrix} \tag{3.9}
\]
where \( \mathbf{a}_i = (a_{i,1}, a_{i,2}, \ldots, a_{i,2^k-1}) \) is a row vector, and let \( \mathbf{G} \) be a generator matrix of UEP code written as

\[
\mathbf{G} = \begin{pmatrix}
\mathbf{g}_1 \\
\mathbf{g}_2 \\
\vdots \\
\mathbf{g}_k
\end{pmatrix},
\]

(3.10)

then, for \( 1 \leq i \leq k \), each row vector \( \mathbf{g}_i \) can be represented as

\[
\mathbf{g}_i = \left( a_{i,1}, \ldots, a_{i,1}, a_{i,2}, \ldots, a_{i,2}, \ldots, a_{i,2k-1}, \ldots, a_{i,2k-1} \right)_{x_1 \text{ times}}_{x_2 \text{ times}}_{x_{2k-1} \text{ times}}
\]

(3.11)

where \( x_j \geq 0 \) for \( 1 \leq j \leq 2^k - 1 \), and

\[
n = \sum_{j=1}^{2^k-1} x_j
\]

(3.12)

represents the code length.

For a given separation vector \( \mathbf{s} = (s_1, s_2, \ldots, s_k) \), it follows from (3.2) and (3.7) that

\[
w_H(\mathbf{g}_1) \geq s_1,
\]

(3.13a)

\[
w_H\left( \mathbf{g}_i + \sum_{j=1}^{i-1} \omega_j \mathbf{g}_j \right) \geq s_i \quad \text{for} \quad 2 \leq i \leq k
\]

(3.13b)
where $\omega_j \in \{0, 1\}$. Then, from (3.11),

$$w_H(g_1) = \sum_{j=1}^{2^k-1} a_{1,j} x_j = a_1 x^T,$$

(3.14a)

$$w_H(g_i + \sum_{j=1}^{i-1} \omega_j g_j) = \left( a_i + \sum_{j=1}^{i-1} \omega_j a_j \right) x^T \text{ for } 2 \leq i \leq k.$$  

(3.14b)

where $x = (x_1, x_2, \ldots, x_{2^k-1})$.

Therefore, from (3.13) and (3.14), we can have the following inequalities

$$A_i x^T \geq b_i^T \text{ for } 1 \leq i \leq k$$

(3.15)

where $A_i$ is a $2^{i-1} \times (2^k - 1)$ matrix that contains all $2^{i-1}$ rows of

$$a_1 \text{ for } i = 1$$

(3.16a)

$$a_i + \sum_{j=1}^{i-1} \omega_j a_j \text{ for } 2 \leq i \leq k,$$

(3.16b)

and $b_i = (s_i, s_i, \ldots, s_i)$ is a row vector of length $2^{i-1}$.

Based on (3.15), we formulate an integer programming problem for UEP code construction with the separation vector $s = (s_1, s_2, \ldots, s_k)$ whose elements are given as $s_i = 2t_i + 1$ for $1 \leq i \leq k$. 

23
Minimize
\[ n = x_1 + x_2 + \cdots + x_{2^k-1} \]
subject to
\[ Ax^\top \geq b^\top \]
where
\[
A = \begin{pmatrix}
A_1 \\
A_2 \\
\vdots \\
A_k
\end{pmatrix}, \quad b^\top = \begin{pmatrix}
b_1^\top \\
b_2^\top \\
\vdots \\
b_k^\top
\end{pmatrix}
\]
A feasible solution or the best feasible solution (i.e., optimal solution) to the integer programming problem shall provide the vector \( x = (x_1, x_2, \ldots, x_{2^k-1}) \) whose sum is the objective value \( n \). Let an index set \( J_s \) be
\[
J_s = \{ j \mid x_j \neq 0, \quad 1 \leq j \leq 2^k - 1 \},
\]
\[
= \{ j_1, j_2, \ldots, j_\tau \} \quad \text{where} \quad 1 \leq j_1 < j_2 < \ldots < j_\tau \leq 2^k - 1, \quad (3.17)
\]
and let \( q_j \) be \( j \)-th column of the matrix \( A_b \), i.e.,
\[
A_b = (q_{1}, q_2, \ldots, q_{2^k-1}). \quad (3.18)
\]
Then, a generator matrix of UEP code can be constructed from the integer programming solution as
\[
G = (q_{j_1}, \ldots, q_{j_1}, q_{j_2}, \ldots, q_{j_2}, \ldots, q_{j_\tau}, \ldots, q_{j_\tau})_{x_{j_1} \times \text{times}} (3.19)
\]
Example 3.1 \((k = 3)\). For \(s = (3, 5, 7)\), it follows from (3.8),

\[
\mathbf{A}_n = \begin{pmatrix}
0 & 0 & 0 & 1 & 1 & 1 & 1 \\
0 & 1 & 1 & 0 & 0 & 1 & 1 \\
1 & 0 & 1 & 0 & 1 & 0 & 1
\end{pmatrix}
= \begin{pmatrix}
a_1 \\
a_2 \\
a_3
\end{pmatrix},
\]

then the generator matrix can be represented as

\[
\mathbf{G} = \begin{pmatrix}
0 & \cdots & 0 & \cdots & 0 & \cdots & 0 \\
0 & \cdots & 0 & \cdots & 1 & \cdots & 1 \\
1 & \cdots & 1 & \cdots & 0 & \cdots & 0
\end{pmatrix}
= \begin{pmatrix}
g_1 \\
g_2 \\
g_3
\end{pmatrix}.
\]

\(\leftarrow x_1 \rightarrow \leftarrow x_2 \rightarrow \cdots \rightarrow x_7 \rightarrow\)

From (3.16),

\[
\mathbf{A}_1 = \begin{pmatrix}
0 & 0 & 0 & 1 & 1 & 1 & 1
\end{pmatrix}
= \mathbf{a}_1,
\]

\[
\mathbf{A}_2 = \begin{pmatrix}
0 & 1 & 1 & 0 & 1 & 1 \\
0 & 1 & 1 & 1 & 0 & 0 \\
1 & 1 & 1 & 0 & 0 & 0
\end{pmatrix}
= \begin{pmatrix}
a_2 \\
a_2 + a_1
\end{pmatrix},
\]

\[
\mathbf{A}_3 = \begin{pmatrix}
1 & 0 & 1 & 0 & 1 & 1 & 1 \\
1 & 0 & 1 & 1 & 0 & 1 & 0 \\
1 & 1 & 0 & 0 & 1 & 1 & 0 \\
1 & 1 & 0 & 1 & 0 & 0 & 1
\end{pmatrix}
= \begin{pmatrix}
a_3 \\
a_3 + a_1 \\
a_3 + a_2 \\
a_3 + a_1 + a_2
\end{pmatrix}.
\]

Therefore, the UEP code construction is to find \(\mathbf{x}\) that minimizes the sum \(x_1 + x_2 + \cdots + x_7\)
satisfying

\[ x_4 + x_5 + x_6 + x_7 \geq 3, \]
\[ x_2 + x_3 + x_6 + x_7 \geq 5, \]
\[ x_2 + x_3 + x_4 + x_5 \geq 5, \]
\[ x_1 + x_3 + x_5 + x_7 \geq 7, \]
\[ x_1 + x_3 + x_4 + x_6 \geq 7, \]
\[ x_1 + x_2 + x_5 + x_6 \geq 7, \]
\[ x_1 + x_2 + x_4 + x_7 \geq 7. \]

The optimal solution obtained from the integer programming is

\[ n = \sum_{j=1}^{7} x_j = 11 \]

where

\[
\begin{array}{ccccccccc}
  x_1 & x_2 & x_3 & x_4 & x_5 & x_6 & x_7 \\
  3 & 2 & 2 & 1 & 1 & 1 & 1 \\
\end{array}
\]

From (3.19), the corresponding generator matrix is

\[ G = \begin{pmatrix}
  0 & 0 & 0 & 0 & 0 & 0 & 1 & 1 & 1 \\
  0 & 0 & 0 & 1 & 1 & 1 & 0 & 0 & 1 \\
  1 & 1 & 1 & 0 & 0 & 1 & 1 & 0 & 1 \\
\end{pmatrix}. \]
Since \( \hat{s} = (4, 6, 7) \) and
\[
\hat{s}_i \geq s_i \quad \text{for} \quad 1 \leq i \leq k,
\]
the UEP code generated from \( \mathbf{G} \) satisfies the unequal error protection requirement.

### 3.1.2 Bounds, results, and comparisons

#### Integer programming bounds

We begin by introducing a lower bound on the length of UEP codes in the following theorem.

**Theorem 3.1** (Integer programming bound). For a given non-decreasing separation vector 
\( s = (s_1, s_2, \ldots, s_k) \), an integer programming bound is given by

\[
n \geq \sum_{i=1}^{k} \left\lceil \frac{s_i}{2^{k-i}} \right\rceil.
\]

**Proof.** For the integer programming approach to construct UEP code, we formulate \( 2^k - 1 \) inequalities in matrix form as

\[
\mathbf{A} x^\top \geq \mathbf{b}^\top.
\]

Since the rows of \( \mathbf{A} \) consist of \( 2^k - 1 \) linear combinations of \( \mathbf{a}_i \) for \( 1 \leq i \leq k \), each column of \( \mathbf{A} \) has exactly \( 2^{k-1} \) ones [52, p.97]. Therefore, the sum of \( 2^k - 1 \) inequalities can be given as

\[
2^{k-1} (x_1 + x_2 + \cdots + x_{2^k-1}) \geq \sum_{i=1}^{k} 2^{i-1}s_i,
\]

hence,

\[
2^{k-1} n \geq \sum_{i=1}^{k} 2^{i-1}s_i.
\]

To preserve the integer property of the length \( n \), we add ceiling functions into (3.22); as a
result,

\[ n \geq \sum_{i=1}^{k} \left\lfloor \frac{2^i - 1}{2^{k-1}} s_i \right\rfloor. \]  \hspace{1cm} (3.23)

Therefore,

\[ n \geq \sum_{i=1}^{k} \left\lfloor \frac{s_i}{2^{k-1}} \right\rfloor. \]

We observe that the integer programming bound in (3.20) is consistent with the lower bound derived in [5, Corollary 14]. As introduced in (2.4), van Gils has derived a lower bound of a UEP code for a non-increasing separation vector \( s' = (s'_1, s'_2, \ldots, s'_k) \) as

\[ n_{s'} \geq \sum_{i=1}^{k} \left\lfloor \frac{s'_i}{2^{i-1}} \right\rfloor. \]  \hspace{1cm} (3.24)

Since the separation vector \( s = (s_1, s_2, \ldots, s_k) \) is in non-decreasing order, we set \( s'_i = s_{k-i+1} \). Then, we transform the bound of (3.24) into

\[ n_{s'} \geq \sum_{i=1}^{k} \left\lfloor \frac{s'_i}{2^{i-1}} \right\rfloor = \sum_{i=1}^{k} \left\lfloor \frac{s_{k-i+1}}{2^{i-1}} \right\rfloor = \sum_{i=1}^{k} \left\lfloor \frac{s_i}{2^{k-i}} \right\rfloor. \]

In the following, we also include an upper bound on the length of UEP codes derived by Masnick and Wolf in [1]. As we have reviewed in (2.2), the length of a UEP code with a
given error protection requirement \( t = (t_1, t_2, \ldots, t_k) \) can be upper bounded by

\[
n \leq k + r_U
\]  

(3.25)

where \( r_U \) is the smallest number of check bits \( r \) such that

\[
2^r > \sum_{i=0}^{2^k-1} \binom{n-1}{i} - \sum_{i=2}^{k} \binom{n-1 - T_i}{2t_i - 2} - \sum_{i=2}^{k} \binom{n-1 - T_i}{2t_i - 1}.
\]  

(3.26)

**Integer programming results**

Numerical results of integer programming by using IBM ILOG CPLEX v12.5.1\(^1\) [72] for a given \( s = (3, 5, \ldots, 2k + 1) \) are presented in Table 3.1. From \( k = 2 \) to \( 8 \), lengths are exactly the same as the lower bound, therefore the corresponding UEP codes are optimal. These optimal results are listed in Table 3.2. For \( 9 \leq k \leq 15 \), instead of finding optimal solutions, we limit our search for sub-optimal solutions due to time constraint. The results and the corresponding lower and upper bounds are plotted in Figure 3.2.

In Table 3.2, for each \( k \) that has the optimal solution, we show nonzero variables \( x_j \) that construct the generator matrix\(^2\) of the UEP code. We note that there are many combinations of \( x_j \) for \( 1 \leq j \leq 2^k - 1 \) that are summed to the optimal value of \( n \) (e.g., there are 3 solutions to \( n = 7 \) when \( k = 2 \), 7 solutions to \( n = 11 \) when \( k = 3 \), 2063 solutions to \( n = 16 \) when \( k = 4 \), and so on).

**Comparisons**

In Table 3.3, we compare the length of UEP codes to the length of time sharing repetition codes and the length of shortened BCH codes [73]. First of all, the length of time sharing repetition codes that provides the error protection requirement \( t = (t_1, t_2, \ldots, t_k) \) can be

\(^1\)The IBM ILOG CPLEX v12.5.1 were run on ARGO, a research computing cluster provided by the Office of Research Computing at George Mason University, VA. (URL: http://orc.gmu.edu)

\(^2\)The corresponding generator matrices are provide in Appendix A
Table 3.1: Numerical results from integer programming and the corresponding upper and lower bounds for $s = (3, 5, \ldots, 2k + 1)$

<table>
<thead>
<tr>
<th>$k$</th>
<th>Lower bounds ((3.20))</th>
<th>Integer programming results, $n$</th>
<th>Upper bounds ((3.25))</th>
</tr>
</thead>
<tbody>
<tr>
<td>2</td>
<td>7</td>
<td>7</td>
<td>7</td>
</tr>
<tr>
<td>3</td>
<td>11</td>
<td>11</td>
<td>12</td>
</tr>
<tr>
<td>4</td>
<td>16</td>
<td>16</td>
<td>19</td>
</tr>
<tr>
<td>5</td>
<td>20</td>
<td>20</td>
<td>25</td>
</tr>
<tr>
<td>6</td>
<td>25</td>
<td>25</td>
<td>32</td>
</tr>
<tr>
<td>7</td>
<td>30</td>
<td>30</td>
<td>39</td>
</tr>
<tr>
<td>8</td>
<td>35</td>
<td>35</td>
<td>46</td>
</tr>
<tr>
<td>9</td>
<td>39</td>
<td>$40^a$</td>
<td>53</td>
</tr>
<tr>
<td>10</td>
<td>44</td>
<td>$45$</td>
<td>60</td>
</tr>
<tr>
<td>11</td>
<td>49</td>
<td>$52$</td>
<td>67</td>
</tr>
<tr>
<td>12</td>
<td>55</td>
<td>$58$</td>
<td>74</td>
</tr>
<tr>
<td>13</td>
<td>59</td>
<td>$64$</td>
<td>81</td>
</tr>
<tr>
<td>14</td>
<td>64</td>
<td>$70$</td>
<td>88</td>
</tr>
<tr>
<td>15</td>
<td>69</td>
<td>$76$</td>
<td>95</td>
</tr>
</tbody>
</table>

$^a$ Underline indicates sub-optimal length

obtained by

$$n_{TS} = \sum_{i=1}^{k} n_i \quad (3.27)$$

where $n_i$ denotes the length of component code that provide $t_i$ error correction for $1 \leq i \leq k$.

Since the lengths of the component codes can be given by

$$n_i = 2t_i + 1 \quad \text{for} \quad 1 \leq i \leq k, \quad (3.28)$$
Table 3.2: Optimal code construction from integer programming for a separation vector \( s = (3, 5, \ldots, 2k + 1) \)

<table>
<thead>
<tr>
<th>( k )</th>
<th>( n )</th>
<th>( x_j ) for ( j \in J_s )</th>
</tr>
</thead>
</table>
| 2 | 7 | \( x_1 x_2 x_3 \)  
\( 4 \ 2 \ 1 \) |
| 3 | 11 | \( x_1 x_2 x_3 x_4 x_5 x_6 x_7 \)  
\( 3 \ 2 \ 2 \ 1 \ 1 \ 1 \ 1 \) |
| 4 | 16 | \( x_1 x_2 x_3 x_4 x_5 x_6 x_7 x_8 x_9 x_{10} x_{11} x_{12} x_{13} x_{14} x_{15} \)  
\( 2 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \) |
| 5 | 20 | \( x_{11} x_{12} x_{13} x_{14} x_{15} x_{16} x_{17} x_{18} x_{19} \)  
\( 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \) |
| 6 | 25 | \( x_{1} x_{2} x_{3} x_{4} x_{5} x_{6} x_{7} x_{8} x_{9} x_{10} x_{11} x_{12} x_{13} x_{14} x_{15} x_{16} x_{17} x_{18} x_{19} x_{20} x_{21} x_{22} x_{23} x_{24} x_{25} x_{26} x_{27} x_{28} x_{29} x_{30} x_{31} \)  
\( 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \) |
| 7 | 30 | \( x_{16} x_{17} x_{18} x_{19} x_{20} x_{21} x_{22} x_{23} x_{24} x_{25} x_{26} x_{27} x_{28} x_{29} x_{30} x_{31} x_{32} x_{33} x_{34} x_{35} x_{36} x_{37} x_{38} x_{39} x_{40} x_{41} x_{42} x_{43} x_{44} x_{45} x_{46} x_{47} x_{48} x_{49} x_{50} x_{51} x_{52} x_{53} x_{54} x_{55} x_{56} x_{57} x_{58} x_{59} x_{60} x_{61} x_{62} x_{63} x_{64} x_{65} x_{66} x_{67} x_{68} x_{69} x_{70} x_{71} x_{72} x_{73} x_{74} x_{75} x_{76} x_{77} x_{78} x_{79} x_{80} x_{81} x_{82} x_{83} x_{84} x_{85} x_{86} x_{87} x_{88} x_{89} x_{90} x_{91} x_{92} x_{93} x_{94} x_{95} x_{96} x_{97} x_{98} x_{99} x_{100} x_{101} x_{102} x_{103} x_{104} x_{105} x_{106} x_{107} x_{108} x_{109} x_{110} x_{111} x_{112} x_{113} x_{114} x_{115} x_{116} x_{117} x_{118} x_{119} x_{120} x_{121} x_{122} x_{123} x_{124} x_{125} x_{126} x_{127} x_{128} x_{129} x_{130} x_{131} x_{132} x_{133} x_{134} x_{135} x_{136} x_{137} x_{138} x_{139} x_{140} x_{141} x_{142} x_{143} x_{144} x_{145} x_{146} x_{147} x_{148} x_{149} x_{150} x_{151} x_{152} x_{153} x_{154} x_{155} x_{156} x_{157} x_{158} x_{159} x_{160} x_{161} x_{162} x_{163} x_{164} x_{165} x_{166} x_{167} x_{168} x_{169} x_{170} x_{171} x_{172} x_{173} x_{174} x_{175} x_{176} x_{177} x_{178} x_{179} x_{180} x_{181} x_{182} x_{183} x_{184} \)  
\( 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \) |

The length of time sharing repetition codes with a given separation vector \( s = (3, 5, \ldots, 2k + 1) \) is

\[
n_{TS} = \sum_{i=1}^{k} (2t_i + 1) = k(k + 2) \quad (3.29)
\]
Secondly, since BCH codes are equal error protection codes, a minimum length of shortened BCH code that provides $t = (t_1, t_2, \ldots, t_k)$ is equivalent to a minimum length of shortened BCH code that provides at least $t = \max t_i = t_k$ error corrections. Therefore, for a given separation vector $s = (3, 5, \ldots, 2k + 1)$, a minimum length of shortened BCH code can be obtained by the following procedures.

1. Let $(n_B, k_B, t_B)$ be parameters for $t_B$-error-correcting binary BCH codes, then we find a minimum length BCH code whose dimension $k_B$ is at least $k$ and error correction capability $t_B$ is at least $t_k = \left\lfloor \frac{s_k}{2} \right\rfloor = k$.

2. Then, a minimum length of shortened BCH code with $k$ error correction capability can be given as

$$n_{SB} = n_B - (k_B - k).$$  \hfill (3.30)
Table 3.3: Codelength comparisons among UEP codes, Time sharing repetition codes, and shortened BCH codes for \( s = (3k, 5, \ldots, 2k + 1) \)

<table>
<thead>
<tr>
<th>( k )</th>
<th>( n )</th>
<th>( n_{TS} )</th>
<th>( (n_{SB}, k \geq k) )</th>
</tr>
</thead>
<tbody>
<tr>
<td>2</td>
<td>7</td>
<td>8</td>
<td>((10, 2, 2))</td>
</tr>
<tr>
<td>3</td>
<td>11</td>
<td>15</td>
<td>((13, 3, 3))</td>
</tr>
<tr>
<td>4</td>
<td>16</td>
<td>24</td>
<td>((24, 4, 5))</td>
</tr>
<tr>
<td>5</td>
<td>20</td>
<td>35</td>
<td>((25, 5, 5))</td>
</tr>
<tr>
<td>6</td>
<td>25</td>
<td>48</td>
<td>((31, 6, 7))</td>
</tr>
<tr>
<td>7</td>
<td>30</td>
<td>63</td>
<td>((46, 7, 7))</td>
</tr>
<tr>
<td>8</td>
<td>35</td>
<td>80</td>
<td>((53, 8, 10))</td>
</tr>
<tr>
<td>9</td>
<td>40*</td>
<td>99</td>
<td>((54, 9, 10))</td>
</tr>
<tr>
<td>10</td>
<td>45</td>
<td>120</td>
<td>((55, 10, 10))</td>
</tr>
<tr>
<td>11</td>
<td>52</td>
<td>143</td>
<td>((58, 11, 11))</td>
</tr>
<tr>
<td>12</td>
<td>58</td>
<td>168</td>
<td>((89, 12, 13))</td>
</tr>
<tr>
<td>13</td>
<td>64</td>
<td>195</td>
<td>((90, 13, 13))</td>
</tr>
<tr>
<td>14</td>
<td>70</td>
<td>224</td>
<td>((98, 14, 14))</td>
</tr>
<tr>
<td>15</td>
<td>76</td>
<td>255</td>
<td>((106, 15, 15))</td>
</tr>
</tbody>
</table>

*Underline indicates sub-optimal length

3.1.3 Performance analysis

Asymptotic code rates

Based on the integer programming bounds, we compute asymptotically achievable code rates in the following theorem.

**Theorem 3.2.** Let \( R \) be the rate of UEP code whose separation vector is given as \( s = (3k, 5, \ldots, 2k + 1) \). Then

\[
R \approx 0.2 \quad \text{when} \quad k \gg 1.
\]

(3.31)

**Proof.** Let \( n \) be the length of the optimal UEP code whose separation vector is \( s = (3k, 5, \ldots, 2k + 1) \).
(3, 5, . . . , 2k + 1), then, from (3.20),

\[ n = \sum_{i=1}^{k} \left\lfloor \frac{2i+1}{2^{k-i}} \right\rfloor = \sum_{j=0}^{k-1} \left\lfloor \frac{2(k-j)+1}{2^j} \right\rfloor. \quad (3.32) \]

Let

\[ \eta_j = \left\lfloor \frac{(2k-2j+1)}{2^j} \right\rfloor, \]

and

\[ k = a_x 2^x + a_{x-1} 2^{x-1} + \cdots + a_0 \]

where \( x = \lfloor \log_2 k \rfloor \), then

\[ \eta_j = \begin{cases} 
2k + 1, & j = 0 \\
k, & j = 1 \\
a_x 2^{x-j+1} + \cdots + a_{j-1} 2^0 + \delta_j, & 2 \leq j \leq x + 1 \\
1, & x + 2 \leq j \leq k - 1 
\end{cases} \quad (3.33) \]

where \( \delta_j \in \{0, 1\} \) [74, p.47,51]. By letting \( \Delta_j \triangleq \eta_j - \delta_j \) for \( 2 \leq j \leq x + 1 \), we can have

\[ \sum_{j=2}^{x+1} \Delta_j = a_x (2^{x-1} + \cdots + 1) + a_{x-1} (2^{x-2} + \cdots + 1) + \cdots + a_2 (2 + 1) + a_1 \]

\[ = a_x (2^x - 1) + a_{x-1} (2^{x-1} - 1) + \cdots + a_0 (1 - 1) \]

\[ = k - \sum_{w=0}^{x} a_w \quad (3.34) \]
From (3.33) and (3.34),

\[
\sum_{j=0}^{1} \eta_j = 3k + 1, \quad (3.35a)
\]

\[
\sum_{j=2}^{x+1} \eta_j = k - \sum_{w=0}^{x} a_w + \sum_{j=2}^{x+1} \delta_j, \quad (3.35b)
\]

and

\[
\sum_{j=x+2}^{k-1} \eta_j = k - \lfloor \log_2 k \rfloor - 2. \quad (3.35c)
\]

Therefore,

\[
n = \sum_{j=0}^{k-1} \eta_j \approx 5k \quad \text{when} \quad k \gg 1. \quad (3.36)
\]

Consequently, the code rate \( R_U \) is converged to

\[
R_U = \frac{k}{n} \approx \frac{k}{5k} = 0.2 \quad \text{when} \quad k \gg 1.
\]

Simulation results based on \( R = \frac{k}{n} \) of the UEP codes are illustrated in Figure 3.3 for \( s = (3, 5, \ldots, 2k + 1) \) and \( 2 \leq k \leq 2^{15} \), which shows asymptotic convergence to 0.2 as proven in Theorem 3.2.

**Throughput of the degraded broadcast channels**

Recall from Section 2.2, the proposed broadcast channel model depicted in Figure 3.1 can be considered as a degraded broadcast channel that has \( k \) component channels [27]. From \( k \) cascaded binary symmetric channels (BSCs) with parameters \( \alpha_i \in [0, \frac{1}{2}] \) as shown in
Figure 3.3: Rates of optimal UEP codes for $2 \leq k \leq 2^{15}$ when a separation vector is given as $s = (3, 5, \ldots, 2k + 1)$.

Figure 2.4, the bit error probability of each component channel can be given by

$$p_i = p_{i-1}(1 - \alpha_i) + (1 - p_{i-1})\alpha_i \quad \text{for} \quad 1 \leq i \leq k$$  \hfill (3.37)

where $p_0 = 0$ [27]. For simplicity, let $\alpha_i = p$ for $1 \leq i \leq k$, then

$p_1 = p$,

$p_2 = (1 - p_1)p + p_1(1 - p) = p(1 + \Phi)$,

$p_3 = (1 - p_2)p + p_2(1 - p) = p(1 + \Phi + \Phi^2)$,

\[ \vdots \]

$p_i = (1 - p_{i-1})p + p_{i-1}(1 - p) = p(1 + \Phi + \Phi^2 + \cdots + \Phi^{i-1})$
where $\Phi = (1 - 2p)$. Therefore, (3.37) can be written as in a closed form,

$$p_i = \frac{1 - \Phi^i}{2} \quad \text{for} \quad 1 \leq i \leq k. \quad (3.38)$$

Let $n$ satisfy the bound (3.20) for a given separation vector $s = (3, 5, \ldots, 2k + 1)$, then $m_i$ can be successfully delivered to receiver $i$ when the corresponding component channel introduces less than or equal to $i$ errors. Therefore, the average rate of successful transmission of a bit to receiver $R_i$, denoting by $\theta_i$, can be given as

$$\theta_i = \sum_{j=0}^{i} \binom{n}{j} (1 - p_i)^{n-j} p_i^j, \quad 1 \leq i \leq k, \quad (3.39)$$

consequently,

$$\Gamma_i = \frac{\theta_i}{n}, \quad 1 \leq i \leq k \quad (3.40)$$

where $\Gamma_i$ denote the effective transmission rate of each component channel.

From (2.6), throughput of the degraded broadcast channel can be given by

$$R_T = \sum_{i=1}^{k} \Gamma_i \leq \frac{k}{n}. \quad (3.41)$$

Numerical results of the throughput $R_T$ for $2 \leq k \leq 2^8$ and the corresponding code rate, $\frac{k}{n}$, for a given $s = (3, 5, \ldots, 2k + 1)$, are illustrated in Figure 3.4.

**Bit-error performance of the degraded broadcast channels**

For the degrade broadcast channel model with cascaded BSCs, a message bit $m_i$ cannot be recovered at a receiver $i$ if the channel introduces more than $\lceil \frac{i}{2} \rceil$ errors when the proposed UEP coding scheme is used for multiuser communications. Therefore we can obtain a
probability of bit error for a receiver $i$ as

$$P_b(i) = \Pr(\hat{m}_i \neq m_i) = \sum_{j=i+1}^{n} \binom{n}{j} (1 - p_i)^{n-j} p_i^j, \quad 1 \leq i \leq k$$  \hspace{1cm} (3.42)
Figure 3.5: Bit error performance with a binary UEP code where $n = 25$ and $k = 6$ for a given $s = (3, 5, \ldots, 13)$.

where $p_i$ is a bit error probability of the component channel as derived in (3.38). In Fig. 3.5(a), assuming an AWGN channel with BPSK signaling (i.e., $p = Q\left(\sqrt{\frac{2kE_b}{nN_0}}\right)$), we illustrate the bit error performances of the 6-user communication system over the degraded broadcast channel with a binary UEP code whose length is $n = 25$ for a given
For comparison, we investigate the bit error performance when the optimal UEP codes are applied for a conventional multilevel error protection. Consider a communication scenario that a $k$-bit message vector $\mathbf{m} = (m_1, m_2, \ldots, m_k)$ is transmitted to a single receiver where the message bit $m_i$ for $1 \leq i \leq k$ has levels of error protection requirement. Suppose that a separation vector $\mathbf{s} = (3, 5, \ldots, 2k + 1)$ specifies the multilevel error protection, i.e., a message bit $m_i$ is protected against $i$-bit channel errors. Then, a probability of bit error for each message bit can be written as

$$P_b(i) = \Pr(\hat{m}_i \neq m_i) = \sum_{j=i+1}^{n} \binom{n}{j} (1-p)^{n-j}p^j, \quad 1 \leq i \leq k.$$  \hspace{1cm} (3.43)

where $p$ denotes a transition probability of a single BSC (i.e., $p = Q\left(\sqrt{\frac{2kE_b}{nN_0}}\right)$ by assuming an AWGN channel with BPSK signaling). In Fig. 3.5(b), we illustrate the bit error performances of the 6-level error protection with binary UEP codes whose length is $n = 25$ for a given $\mathbf{s} = (3, 5, \ldots, 13)$.

3.1.4 Decoding of UEP codes using integer programming

Decoding by majority logic

Let a generator matrix of UEP code be represented with its column vectors $\mathbf{f}_j$ for $1 \leq j \leq n$,

$$\mathbf{G} = \begin{pmatrix}
g_{1,1} & g_{1,2} & \cdots & g_{1,n} 
g_{2,1} & g_{2,2} & \cdots & g_{2,n} 
\vdots & \vdots & \ddots & \vdots 
g_{k,1} & g_{k,2} & \cdots & g_{k,n}
\end{pmatrix},$$

$$= (\mathbf{f}_1, \mathbf{f}_2, \ldots, \mathbf{f}_n), \hspace{1cm} (3.44)$$
and let a received vector at receiver $R_i$ for $1 \leq i \leq k$ be written as $r_i = (r_1, r_2, \ldots, r_n)$. Then each received bit $r_j$ can be represented by

$$r_j = mf_j + e_j, \quad (3.45)$$

$$= \sum_{i=1}^{k} m_i g_{i,j} + e_j \quad \text{for} \quad 1 \leq j \leq n$$

where $m = (m_1, m_2, \ldots, m_k)$ is a message vector, $g_{i,j}$ is an element at the $i$-th row and the $j$-th column of the generator matrix $G$, and $e_j$ is a channel error.

Let $J_h$ be a subset of $J$ where $J = \{1, 2, \ldots, n\}$ for a given $h$, and $\hat{r}_h$ be a modified received bit where

$$\hat{r}_h = \sum_{j \in J_h} r_j \quad (3.46)$$

under modulo-2 additions. If the subset $J_h$ satisfies

$$\sum_{j \in J_h} f_j = i_i \quad (3.47)$$

where $i_i$ denotes the $i$-th column of $k \times k$ identity matrix,

$$\hat{r}_h = \sum_{j \in J_h} (mf_j + e_j),$$

$$= m_i + \sum_{j \in J_h} e_j. \quad (3.48)$$

Consider the generator matrix $G$ from Example 3.1 and the index subsets $J_1 = \{8\}$, $J_2 = \{5, 10\}$, and $J_3 = \{7, 11\}$. Then, the corresponding modified received bits are written
as

\[ \hat{r}_1 = \sum_{j \in J_1} r_j = r_8 = m_1 + e_8, \]

\[ \hat{r}_2 = \sum_{j \in J_2} r_j = r_5 + r_{10} = (m_2 + e_5) + (m_1 + m_2 + e_{10}) \]

\[ = m_1 + (e_5 + e_{10}), \]

\[ \hat{r}_3 = \sum_{j \in J_3} r_j = r_7 + r_{11} \]

\[ = (m_2 + m_3 + e_7) + (m_1 + m_3 + m_2 + e_{11}) \]

\[ = m_1 + (e_7 + e_{11}). \]

Suppose that the channel has introduced no error or single-bit error (i.e., \( \sum_{j \in v} e_j \leq 1 \)). Then, it is easy to see that the message bit \( m_1 \) can be determined at the receiver \( R_1 \) by majority logic since at most one of \( \hat{r}_1, \hat{r}_2, \) and \( \hat{r}_3 \) has an error component. Based on this observation, we develop the following theorem.

**Theorem 3.3.** Suppose that, at receiver \( R_i \) for \( 1 \leq i \leq k \), the number of errors are less than or equal to \( t_i = \lfloor \frac{s_i}{2} \rfloor \). Then the receiver \( R_i \) can recover the message \( m_i \) if there exist disjoint subsets \( J_1, J_2, \ldots, J_{s_i} \) of \( J \) where each subset satisfies

\[ \sum_{j \in J_h} f_j = i_i \quad \text{for} \quad 1 \leq h \leq s_i. \]

**Proof.** From (3.48), each subset modifies the corresponding received bits as

\[ \hat{r}_h = \sum_{j \in J_h} r_j = m_i + \sum_{j \in J_h} e_j \quad \text{for} \quad 1 \leq h \leq s_i. \]
If the subsets $J_1, J_2, \ldots, J_s$ are disjoint, i.e.,

$$J_h \cap J_{h'} = \emptyset \quad \text{for} \quad 1 \leq h \neq h' \leq s,$$

(3.50)

where $\bigcup_{h=1}^{s_i} J_h \subseteq \mathcal{J}$, then less than or equal to $\left\lfloor \frac{s_i}{2} \right\rfloor$ of $\hat{r}_h$ has nonzero error components since $\sum_{\forall j} e_j \leq \left\lfloor \frac{s_i}{2} \right\rfloor$. Therefore, the message $m_i$ can be determined at the receiver $R_i$ by using majority logic on $(\hat{r}_1, \hat{r}_2, \ldots, \hat{r}_{s_i})$, i.e.,

$$m_i = \begin{cases} 
0 & \text{if } \sum_{h=1}^{s_i} \hat{r}_h \leq \left\lfloor \frac{s_i}{2} \right\rfloor \\
1 & \text{otherwise}
\end{cases}$$

(3.51)

Based on Theorem 3.3, we formulate an integer programming problem such that it finds a subset of $\mathcal{J}$ that satisfies (3.47). Then, we iterate the integer programming until all disjoint subsets, $J_1, J_2, \ldots, J_s$ are found.

**Iterative integer programming**

Consider a subset $J_h$ of an index set $\mathcal{J} = \{1, 2, \ldots, n\}$ that satisfies the following constraint over $\text{GF}(2)$ for a given $i$,

$$\sum_{j \in J_h} g_{i,j} = 1$$

(3.52a)

$$\sum_{j \in J_h} g_{i',j} = 0 \quad \text{for} \quad 1 \leq i' \neq i \leq k.$$  

(3.52b)
Then, from (3.45) and (3.46),

\[
\hat{r}_h = \sum_{j \in J_h} r_j = \sum_{j \in J_h} (mf_j + e_j)
\]

\[
= m_i \sum_{j \in J_h} g_{i,j} + \sum_{1 \leq i' \neq i \leq k} m_{i'} \sum_{j \in J_h} g_{i',j} + \sum_{j \in J_h} e_j
\]

\[
= m_i + \sum_{j \in J_h} e_j.
\]

Therefore, the subset \( J_h \) which satisfies (3.47) can be obtained from the constraints (3.52) under modulo-2 addition.

Let us define a vector \( y = \{y_1, y_2, \ldots, y_n\} \) that consists of binary variables \( y_j \) where

\[
y_j = \begin{cases} 
0 & \text{if } j \notin J_h \\
1 & \text{if } j \in J_h
\end{cases} \quad \text{for } 1 \leq j \leq n. \tag{3.53}
\]

Then, the constraints (3.52) to find the subset \( J_h \) can be rewritten under modulo-2 addition as

\[
\sum_{j \in G_i} y_j = 1, \tag{3.54a}
\]

\[
\sum_{j \in G_{i'}} y_j = 0, \quad \text{for } 1 \leq i' \neq i \leq k \tag{3.54b}
\]

where \( G_i \) denotes an index set for the \( i \)-th row of \( G \) that has nonzero component, i.e.,

\[
G_i = \{j \mid g_{i,j} \neq 0, \, 1 \leq j \leq n\} \quad \text{for } 1 \leq i \leq k. \tag{3.55}
\]

Furthermore, since the objective of iterative integer programming is to find \( s_i \) numbers
of disjoint subsets $J_1, J_2, \ldots, J_s$ of $J$, and since

$$|J_1| + |J_2| + \cdots + |J_s| \leq |J| = n$$  \hspace{1cm} (3.56)

where $|\cdot|$ denotes the cardinality of a set, minimizing the number of elements in a subset is desired to maximize the possibility that there exist $s_i$ numbers of disjoint subsets.

Therefore, for receiver $R_i$, finding a subset $J_h$ becomes to an integer programming problem that minimizes the sum of $y_1 + y_2 + \cdots + y_n$ satisfying the constraints in (3.54):

**Finding an index subset at receiver $R_i$**

Minimize

$$y_1 + y_2 + \cdots + y_n$$

subject to

$$Gy^\top - 2z^\top = i_i$$

where

$$y = (y_1, y_2, \ldots, y_n),$$

$$y_1, y_2, \ldots, y_n \in \{0, 1\},$$

$$z = (z_1, z_2, \ldots, z_k),$$

$$z_1, z_2, \ldots, z_k \in \{0, 1, 2, 3, \ldots\}.$$  

In the formulated integer programming problem, artificial variables $z_u$ for $1 \leq u \leq k$ are introduced to convert the modulo-2 additions in (3.54) into the linear constraints (i.e., real additions), and they are bounded by

$$\sum_{j \in G_u} y_j - 1 \leq 2z_u \leq \sum_{j \in G_u} y_j \quad \text{for} \quad 1 \leq u \leq k.$$  \hspace{1cm} (3.57)
The following table shows an example of the conversion with an artificial variable $z$ that is bounded by

$$y_1 + y_2 + y_3 - 1 \leq 2z \leq y_1 + y_2 + y_3$$

where $z \in \{0, 1, 2, \ldots \}$.

<table>
<thead>
<tr>
<th>$y_1$</th>
<th>$y_2$</th>
<th>$y_3$</th>
<th>$\Theta_y$</th>
<th>$\sum_y$</th>
<th>$z$</th>
<th>$\sum_y - 2z$</th>
</tr>
</thead>
<tbody>
<tr>
<td>0</td>
<td>0</td>
<td>0</td>
<td>0</td>
<td>0</td>
<td>0</td>
<td>0</td>
</tr>
<tr>
<td>0</td>
<td>0</td>
<td>1</td>
<td>1</td>
<td>1</td>
<td>0</td>
<td>1</td>
</tr>
<tr>
<td>0</td>
<td>1</td>
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<td>1</td>
</tr>
<tr>
<td>0</td>
<td>1</td>
<td>1</td>
<td>0</td>
<td>2</td>
<td>1</td>
<td>0</td>
</tr>
<tr>
<td>1</td>
<td>0</td>
<td>0</td>
<td>1</td>
<td>1</td>
<td>0</td>
<td>1</td>
</tr>
<tr>
<td>1</td>
<td>0</td>
<td>1</td>
<td>0</td>
<td>2</td>
<td>1</td>
<td>0</td>
</tr>
<tr>
<td>1</td>
<td>1</td>
<td>0</td>
<td>0</td>
<td>2</td>
<td>1</td>
<td>0</td>
</tr>
<tr>
<td>1</td>
<td>1</td>
<td>1</td>
<td>1</td>
<td>3</td>
<td>1</td>
<td>1</td>
</tr>
</tbody>
</table>

Decoding algorithm

**Example 3.2** ($k = 3$). From $G$ in Example 3.1 and (3.55),

$$\mathcal{G}_1 = \{8, 9, 10, 11\},$$

$$\mathcal{G}_2 = \{4, 5, 6, 7, 10, 11\},$$

$$\mathcal{G}_3 = \{1, 2, 3, 6, 7, 9, 11\}.$$
Therefore, the integer programming problem at $R_1$ becomes to minimize the sum $y_1 + y_2 + \cdots + y_{11}$ satisfying

$$y_8 + y_9 + y_{10} + y_{11} - 2z_1 = 1,$$
$$y_4 + y_5 + y_6 + y_7 + y_{10} + y_{11} - 2z_2 = 0,$$
$$y_1 + y_2 + y_3 + y_6 + y_7 + y_9 + y_{11} - 2z_3 = 0.$$

The optimal solution of the integer programming problem finds the smallest subset that satisfy (3.47);

$$\begin{array}{cccccccccccc}
y_1 & y_2 & y_3 & y_4 & y_5 & y_6 & y_7 & y_8 & y_9 & y_{10} & y_{11} \\
0 & 0 & 0 & 0 & 0 & 0 & 1 & 0 & 0 & 0 & 0
\end{array} \rightarrow J_1 = \{8\},$$

then $R_1$ sets $y_8 = 0$ and repeats the integer programming to obtain disjoint subset $J_2$;

$$\begin{array}{cccccccccccc}
y_1 & y_2 & y_3 & y_4 & y_5 & y_6 & y_7 & y_8 & y_9 & y_{10} & y_{11} \\
0 & 0 & 0 & 0 & 1 & 0 & 0 & 0 & 0 & 1 & 0
\end{array} \rightarrow J_2 = \{5, 10\}.$$

Since $R_1$ needs $s_i = 3$ disjoint subsets to decode $m_1$, $R_1$ sets $y_5 = y_8 = y_{10} = 0$ and repeats the integer programming to obtain the last disjoint subset $J_3$;

$$\begin{array}{cccccccccccc}
y_1 & y_2 & y_3 & y_4 & y_5 & y_6 & y_7 & y_8 & y_9 & y_{10} & y_{11} \\
0 & 0 & 0 & 0 & 0 & 1 & 0 & 0 & 0 & 1 & 0
\end{array} \rightarrow J_3 = \{7, 11\}.$$

Using the disjoint subsets $J_1$, $J_2$, and $J_3$, $R_1$ can determine $m_1$ by majority logic. We note here that the iterative integer programming to find the $s_i$ numbers of disjoint subsets does not depend on the received information (i.e., it only depends on the structure of a generator matrix). Therefore, only the majority logic decoding is applied upon receiving
information with the predetermined index subsets, which reduces the complexity of the decoding.

The detailed descriptions of the decoding algorithm is shown in Algorithm 1, and diagrams of the iterative integer programming and the majority logic decoding are illustrated in Fig. 3.6. Additionally, complete decoding procedures are listed in Table 3.4 for all receivers $R_1$, $R_2$, and $R_3$ with a message vector $m = (1, 1, 1)$ and the corresponding codewords $c = (1, 1, 1, 1, 0, 0, 1, 0, 0, 1)$. Let $e_1$, $e_2$, and $e_3$ denote error vectors at receiver $R_1$, $R_2$, and $R_3$, respectively. Then, the error vectors and received vectors are given as

\[
e_1 = (0, 0, 0, 0, 0, 0, 0, 0, 1, 0) \rightarrow r_1 = (1, 1, 1, 1, 0, 0, 1, 0, 1, 1),
\]

\[
e_2 = (0, 0, 0, 0, 0, 0, 0, 1, 1, 0) \rightarrow r_2 = (1, 1, 1, 1, 0, 1, 1, 1, 1, 1),
\]

\[
e_3 = (0, 0, 0, 0, 1, 0, 1, 1, 1, 0) \rightarrow r_3 = (1, 1, 1, 1, 1, 0, 1, 1, 1, 1).
\]

Algorithm 1 UEP decoding algorithm at receiver $R_i$

```
1: procedure ITERATIVE INTEGER PROGRAMMING
2:     $h \leftarrow 0$
3:     repeat $\triangleright$ Finding $s_i$ numbers of subsets
4:         $h \leftarrow h + 1$
5:         $J_h \leftarrow$ integer programming solution
6:         $y_j \leftarrow 0$ for $j \in \bigcup_{1 \leq w \leq h} J_w$
7:     until $h = s_i$
8: end procedure
9: Upon receiving $r_i = (r_1, r_2, \ldots, r_n)$
10: procedure MAJORITY LOGIC DECODING
11:     $h \leftarrow 0$
12:     repeat $\triangleright$ Modifying received bits
13:         $h \leftarrow h + 1$
14:         $\hat{r}_h \leftarrow \sum_{j \in J_h} r_j$
15:     until $h = s_i$
16:     if $\sum_{h=1}^{s_i} \hat{r}_h \leq \left\lfloor \frac{s_i}{2} \right\rfloor$ then $\triangleright$ Majority logic
17:         $\hat{m}_i \leftarrow 0$
18:     else
19:         $\hat{m}_i \leftarrow 1$
20:     end if
21: end procedure
```
Table 3.4: UEP decoding example using integer programming and majority logic

\[ \mathbf{r}_1 = (1, 1, 1, 1, 0, 0, 1, 0, 1, 1) \text{ at } R_1 \]

<table>
<thead>
<tr>
<th>( h )</th>
<th>( \mathcal{J}_h )</th>
<th>( \hat{r}_h )</th>
</tr>
</thead>
<tbody>
<tr>
<td>1</td>
<td>{8}</td>
<td>( \hat{r}_1 = r_8 = 1 )</td>
</tr>
<tr>
<td>2</td>
<td>{5, 10}</td>
<td>( \hat{r}<em>2 = r_5 + r</em>{10} = 0 )</td>
</tr>
<tr>
<td>3</td>
<td>{7, 11}</td>
<td>( \hat{r}<em>3 = r_7 + r</em>{11} = 1 ) → ( m_1 = 1 )</td>
</tr>
</tbody>
</table>

\[ \mathbf{r}_2 = (1, 1, 1, 1, 0, 0, 1, 1, 1, 1) \text{ at } R_2 \]

<table>
<thead>
<tr>
<th>( h )</th>
<th>( \mathcal{J}_h )</th>
<th>( \hat{r}_h )</th>
</tr>
</thead>
<tbody>
<tr>
<td>1</td>
<td>{4}</td>
<td>( \hat{r}_1 = r_4 = 1 )</td>
</tr>
<tr>
<td>2</td>
<td>{5}</td>
<td>( \hat{r}_2 = r_5 = 1 )</td>
</tr>
<tr>
<td>3</td>
<td>{8, 10}</td>
<td>( \hat{r}<em>3 = r_8 + r</em>{10} = 0 )</td>
</tr>
<tr>
<td>4</td>
<td>{1, 6}</td>
<td>( \hat{r}_4 = r_1 + r_6 = 1 )</td>
</tr>
<tr>
<td>5</td>
<td>{9, 11}</td>
<td>( \hat{r}<em>5 = r_9 + r</em>{11} = 0 ) → ( m_2 = 1 )</td>
</tr>
</tbody>
</table>

\[ \mathbf{r}_3 = (1, 1, 1, 1, 0, 1, 1, 1, 1, 1) \text{ at } R_3 \]

<table>
<thead>
<tr>
<th>( h )</th>
<th>( \mathcal{J}_h )</th>
<th>( \hat{r}_h )</th>
</tr>
</thead>
<tbody>
<tr>
<td>1</td>
<td>{1}</td>
<td>( \hat{r}_1 = r_1 = 1 )</td>
</tr>
<tr>
<td>2</td>
<td>{2}</td>
<td>( \hat{r}_2 = r_2 = 1 )</td>
</tr>
<tr>
<td>3</td>
<td>{3}</td>
<td>( \hat{r}_3 = r_3 = 1 )</td>
</tr>
<tr>
<td>4</td>
<td>{8, 9}</td>
<td>( \hat{r}_4 = r_8 + r_9 = 0 )</td>
</tr>
<tr>
<td>5</td>
<td>{4, 6}</td>
<td>( \hat{r}_5 = r_4 + r_6 = 1 )</td>
</tr>
<tr>
<td>6</td>
<td>{10, 11}</td>
<td>( \hat{r}<em>6 = r</em>{10} + r_{11} = 0 )</td>
</tr>
<tr>
<td>7</td>
<td>{5, 7}</td>
<td>( \hat{r}_7 = r_5 + r_7 = 0 ) → ( m_3 = 1 )</td>
</tr>
</tbody>
</table>

The optimal UEP codes listed in Table 3.2 can be successfully decoded by using the integer programming decoding. However, not every optimal code constructed from the integer programming approach is decodable by the proposed decoding algorithm since it may not have the disjoint subsets. For example, there are 2,063 solutions for \( k = 4 \) that have optimal value \( n = 11 \), but 1,719 solutions (i.e., 1,719 generator matrices for UEP codes) have the disjoint subsets. Therefore, we investigate the decodability of the proposed decoding algorithm in Section 3.3.2.
3.2 Integer programming approach to UEP coding scheme for multi-bit messages

In this section, we extend the integer programming approach for the case of single-bit messages introduced in Section 3.1 to \( l \)-bit message case.
3.2.1 UEP code constructions using integer programming

Recall that a message vector $\mathbf{m} = (\mathbf{m}_1, \mathbf{m}_2, \ldots, \mathbf{m}_k)$ consist of $l$-bit messages for $k$ users denoted by

$$
\mathbf{m}_i = (m_1^{(i)}, m_2^{(i)}, \ldots, m_l^{(i)}) \quad \text{for} \quad 1 \leq i \leq k
$$

(3.58)

where $m_u^{(i)} \in \{0, 1\}$ for $1 \leq u \leq l$.

Furthermore, for a given non-decreasing separation vector $\mathbf{s} = (s_1, s_2, \ldots, s_k)$ where $s_i = 2t_i + 1$ for $1 \leq i \leq k$, it follows from (3.3) that a UEP code can correct up to $t_i = \left\lfloor \frac{s_i}{2} \right\rfloor$ channel errors for the message $\mathbf{m}_i$ if

$$
w_H(\mathbf{mG}) \geq s_i, \quad \mathbf{m}_i \neq 0 \quad \text{for} \quad 1 \leq i \leq k.
$$

(3.59)

Let

$$
m'_{(i-1)l+u} = m_u^{(i)} \quad \text{for} \quad 1 \leq i \leq k \quad \text{and} \quad 1 \leq u \leq l,
$$

(3.60)

and

$$
k' = kl.
$$

(3.61)

Then, we can rewrite the message vector $\mathbf{m}$ as

$$
\mathbf{m} = (\mathbf{m}_1 | \mathbf{m}_2 | \ldots | \mathbf{m}_k)
$$

$$
= (m_1^{(1)}, m_2^{(1)}, \ldots, m_l^{(1)} | m_1^{(2)}, m_2^{(2)}, \ldots, m_l^{(2)} | \ldots | m_1^{(k)}, m_2^{(k)}, \ldots, m_l^{(k)})
$$

$$
= (m_1', m_2', \ldots, m_l' | m'_{l+1}, m'_{l+2}, \ldots, m'_{2l} | \ldots | m'_{k'-l+1}, m'_{k'-l+2}, \ldots, m'_{k'})
$$

(3.62)

Also, let us define the modified separation vector of length $k'$ as $\bar{s} = (\bar{s}_1, \bar{s}_2, \ldots, \bar{s}_{k'})$ where each element is written by

$$
\bar{s}_{i'} = s_i \quad \text{for} \quad (i - 1)l + 1 \leq i' \leq il \quad \text{and} \quad 1 \leq i \leq k,
$$

(3.63)

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i.e.,

\[ \ddot{s} = (s_1, s_1, \ldots, s_1, s_2, s_2, \ldots, s_2, \ldots, s_k, s_k, \ldots, s_k \text{, } t \text{ times}, s_2, s_2, \ldots, s_2, \ldots, s_k, s_k, \ldots, s_k \text{, } t \text{ times}) . \]  \hspace{1cm} (3.64)

Then, the constraints (3.59) is equivalent to

\[ w_H(mG) \geq \ddot{s}_{i'}, \quad m'_{i'} = 1 \quad \text{for} \quad 1 \leq i' \leq k' , \]  \hspace{1cm} (3.65)

consequently, using the integer programming approach introduced in Section 3.1.1, we can construct a UEP code that satisfies (3.65).

Let \( A_b \) be the \( k' \times (2^k' - 1) \) matrix as defined in (3.8), i.e.,

\[ A_b = \begin{pmatrix}
0 & 0 & 0 & \ldots & 0 & 1 & \ldots & 1 & 1 \\
0 & 0 & 0 & \ldots & 1 & 0 & \ldots & 1 & 1 \\
\vdots & \vdots & \vdots & \ddots & \vdots & \vdots & \ddots & \vdots & \vdots \\
0 & 1 & 1 & \ldots & 1 & 0 & \ldots & 1 & 1 \\
1 & 0 & 1 & \ldots & 1 & 0 & \ldots & 0 & 1
\end{pmatrix} = \begin{pmatrix}
a_1 \\
a_2 \\
\vdots \\
a_{k'-1} \\
a_{k'}
\end{pmatrix} \]  \hspace{1cm} (3.66)

then, from (3.15), we have the following inequalities for integer programming problem:

\[ A_{i'} x^T \geq b_{i'}^T \quad \text{for} \quad 1 \leq i' \leq k' \]  \hspace{1cm} (3.67)

where

\[ A_{i'} = \begin{cases}
a_1 & \text{if } i' = 1 \\
a_{i'} + \sum_{u=1}^{i'-1} \omega_u a_u, & \text{if } 2 \leq i' \leq k' \end{cases} \]  \hspace{1cm} (3.68a)

where \( \omega_u \in \{0,1\} \),
\( x = (x_1, x_2, \ldots, x_{2^k - 1}) \), \hspace{1cm} (3.68b)

and

\[ b_i' = (s_{i}', s_{i}'', \ldots, s_{i}^{2^k - 1}). \]  \hspace{1cm} (3.68c)

Therefore, based on (3.67), we formulate an integer programming problem for UEP code construction with a given separation vector \( s = (s_1, s_2, \ldots, s_k) \) whose elements are given as \( s_i = 2t_i + 1 \) for \( 1 \leq i \leq k \).

\begin{center}
\textbf{UEP code construction}
\end{center}

Minimize

\[ n = x_1 + x_2 + \cdots + x_{2^k - 1} \]

subject to

\[ Ax^\top \geq b^\top \]

where

\[
A = \begin{pmatrix}
A_1 \\
A_2 \\
\vdots \\
A_{k'}
\end{pmatrix}, \quad b^\top = \begin{pmatrix}
b_1^\top \\
b_2^\top \\
\vdots \\
b_{k'}^\top
\end{pmatrix}
\]
Example 3.3 \((k = 2 \& l = 2)\). For a given \(s = (3, 5)\), it follows from (3.66),

\[
A_b = \begin{pmatrix}
000000011111111 \\
001111100001111 \\
011001100110011 \\
101010101010101
\end{pmatrix} = \begin{pmatrix}
a_1 \\
a_2 \\
a_3 \\
a_4
\end{pmatrix},
\]

and, from (3.68a),

\[
A_1 = \begin{pmatrix}
000000011111111
\end{pmatrix} = (a_1),
\]

\[
A_2 = \begin{pmatrix}
000111100001111 \\
00111111110000
\end{pmatrix} = \begin{pmatrix}
a_2 \\
00111111110000
\end{pmatrix} = \begin{pmatrix}
a_2 + a_1
\end{pmatrix},
\]

\[
A_3 = \begin{pmatrix}
011001100110011 \\
011001111001100 \\
011110000111100 \\
011110011000011
\end{pmatrix} = \begin{pmatrix}
a_3 \\
a_3 + a_1 \\
a_3 + a_2 \\
a_3 + a_1 + a_2
\end{pmatrix},
\]

\[
A_4 = \begin{pmatrix}
101010101010101 \\
101010101010101 \\
101100101101010 \\
101101010100101 \\
110011001100110 \\
110011001100110 \\
110100110110011 \\
110100110110011
\end{pmatrix} = \begin{pmatrix}
a_4 \\
a_4 + a_1 \\
a_4 + a_2 \\
a_4 + a_1 + a_2 \\
a_4 + a_3 \\
a_4 + a_1 + a_3 \\
a_4 + a_2 + a_3 \\
a_4 + a_1 + a_2 + a_3
\end{pmatrix}.
\]
Therefore, the UEP code construction becomes to find $x$ that minimizes the sum $x_1 + x_2 + \cdots + x_{15}$ satisfying

\[
\begin{align*}
  x_8 + x_9 + x_{10} + x_{11} + x_{12} + x_{13} + x_{14} + x_{15} & \geq 3 \\
  x_4 + x_5 + x_6 + x_7 + x_{12} + x_{13} + x_{14} + x_{15} & \geq 3 \\
  x_4 + x_5 + x_6 + x_7 + x_8 + x_9 + x_{10} + x_{11} & \geq 3 \\
  x_2 + x_3 + x_6 + x_7 + x_{10} + x_{11} + x_{14} + x_{15} & \geq 5 \\
  x_2 + x_3 + x_6 + x_7 + x_8 + x_9 + x_{12} + x_{13} & \geq 5 \\
  x_2 + x_3 + x_4 + x_5 + x_{10} + x_{11} + x_{12} + x_{13} & \geq 5 \\
  x_2 + x_3 + x_4 + x_5 + x_8 + x_9 + x_{14} + x_{15} & \geq 5 \\
  x_1 + x_3 + x_5 + x_7 + x_9 + x_{11} + x_{13} + x_{15} & \geq 5 \\
  x_1 + x_3 + x_5 + x_7 + x_8 + x_{10} + x_{12} + x_{14} & \geq 5 \\
  x_1 + x_3 + x_4 + x_6 + x_9 + x_{11} + x_{12} + x_{14} & \geq 5 \\
  x_1 + x_3 + x_4 + x_6 + x_8 + x_{10} + x_{13} + x_{15} & \geq 5 \\
  x_1 + x_2 + x_5 + x_6 + x_9 + x_{10} + x_{13} + x_{14} & \geq 5 \\
  x_1 + x_2 + x_5 + x_6 + x_8 + x_{11} + x_{12} + x_{15} & \geq 5 \\
  x_1 + x_2 + x_4 + x_7 + x_9 + x_{10} + x_{12} + x_{15} & \geq 5 \\
  x_1 + x_2 + x_4 + x_7 + x_8 + x_{11} + x_{13} + x_{14} & \geq 5.
\end{align*}
\]
The optimal value obtained by solving the integer programming problem is

\[ n = \sum_{j=1}^{15} x_j = 10, \]

where

\[ x_1 x_2 x_3 x_4 x_5 x_7 x_8 x_9 x_{10} x_{11} \]

\[ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1. \]

Therefore, the corresponding generator matrix is

\[
G = \begin{pmatrix}
0 & 0 & 0 & 0 & 0 & 0 & 1 & 1 & 1 & 1 \\
0 & 0 & 1 & 1 & 0 & 0 & 0 & 0 & 0 & 0 \\
0 & 1 & 1 & 0 & 0 & 1 & 0 & 0 & 1 & 1 \\
1 & 0 & 1 & 0 & 1 & 1 & 0 & 1 & 0 & 1
\end{pmatrix}.
\]

### 3.2.2 Bounds, results, and comparisons

A lower bound on the length of the UEP code for the case of \( l \)-bit messages are given in the following corollary.

**Corollary 3.1** (Integer programming bound for \( l \)-bit messages). For a given non-decreasing separation vector \( s = (s_1, s_2, \ldots, s_k) \), an integer programming bound is given by

\[ n \geq \sum_{i=1}^{k} \sum_{j=il-l+1}^{il} \left\lceil \frac{s_i}{2^{kl-j}} \right\rceil. \]  

(3.69)

**Proof.** For the given separation vector \( s = (s_1, s_2, \ldots, s_k) \), we formulate \( 2^{kl} - 1 \) inequalities.
Table 3.5: Optimal results of integer programming: $l$-bit message

<table>
<thead>
<tr>
<th>$l$</th>
<th>$k$</th>
<th>IP bound</th>
<th>IP result</th>
<th>nonzero $x_j$ for $1 \leq j \leq 2^k l - 1$</th>
</tr>
</thead>
<tbody>
<tr>
<td>2</td>
<td>2</td>
<td>10</td>
<td>10</td>
<td>$x_1 x_2 x_3 x_4 x_5 x_7 x_8 x_9 x_{10} x_{11}$</td>
</tr>
<tr>
<td></td>
<td></td>
<td></td>
<td></td>
<td>1 1 1 1 1 1 1 1 1 1</td>
</tr>
<tr>
<td>2</td>
<td>3</td>
<td>16</td>
<td>16</td>
<td>$x_1 x_2 x_3 x_4 x_5 x_6 x_8 x_9 x_{10} x_{11} x_{16} x_{17} x_{19} x_{32} x_{35} x_{47} x_{61}$</td>
</tr>
<tr>
<td></td>
<td></td>
<td></td>
<td></td>
<td>1 1 1 1 1 1 1 1 1 1 1 1 1</td>
</tr>
<tr>
<td>3</td>
<td>2</td>
<td>13</td>
<td>13</td>
<td>$x_1 x_2 x_3 x_4 x_5 x_6 x_7 x_8 x_{16} x_{32} x_{44} x_{54} x_{61}$</td>
</tr>
<tr>
<td></td>
<td></td>
<td></td>
<td></td>
<td>1 1 1 1 1 1 1 1 1 1 1 1 1</td>
</tr>
<tr>
<td>4</td>
<td>2</td>
<td>15</td>
<td>15</td>
<td>$x_1 x_2 x_4 x_7 x_8 x_{11} x_{13} x_{14} x_{16} x_{32} x_{64} x_{127} x_{128} x_{179} x_{213}$</td>
</tr>
<tr>
<td></td>
<td></td>
<td></td>
<td></td>
<td>1 1 1 1 1 1 1 1 1 1 1 1 1 1 1</td>
</tr>
</tbody>
</table>

for constraints of the integer programming problem as

$$A x^T \geq b^T.$$ 

Similar to the proof of Theorem 3.20, each column of $A$ has $2^{kl-1}$ ones, and the sum of the inequalities can be written as

$$2^{kl-1} (x_1 + x_2 + \cdots + x_{2^l-1})$$

$$\geq (2^l - 1)s_1 + 2^l(2^l - 1)s_2 + \cdots + 2^{(k-1)l}(2^l - 1)s_k. \quad (3.70)$$

Consequently,

$$n \ 2^{kl-1} \geq \sum_{i=1}^{l} 2^{i-1}s_1 + \sum_{i=l+1}^{2l} 2^{i-1}s_2 + \cdots + \sum_{i=(k-1)l+1}^{kl} 2^{i-1}s_k. \quad (3.71)$$
Table 3.6: Code length comparisons for \( s = (3, 5, \ldots, 2k + 1) \)

<table>
<thead>
<tr>
<th>( l )</th>
<th>( k )</th>
<th>UEP code ( n )</th>
<th>Shortened BCH(^a) ( n_{SB} )</th>
<th>Time sharing ( n_{TS} )</th>
<th>( n_{TS} ) component codes(^b)</th>
</tr>
</thead>
<tbody>
<tr>
<td>2</td>
<td>2</td>
<td>10</td>
<td>(12, 4, 2)</td>
<td>15</td>
<td>(5, 2, 1) ( (10, 2, 2) )</td>
</tr>
<tr>
<td>2</td>
<td>3</td>
<td>16</td>
<td>(21, 6, 3)</td>
<td>27</td>
<td>(5, 2, 1) ( (10, 2, 2) ) ( (12, 2, 3) )</td>
</tr>
<tr>
<td>3</td>
<td>2</td>
<td>13</td>
<td>(14, 6, 2)</td>
<td>17</td>
<td>(6, 3, 1) ( (11, 3, 2) )</td>
</tr>
<tr>
<td>4</td>
<td>2</td>
<td>15</td>
<td>(18, 8, 2)</td>
<td>19</td>
<td>(7, 4, 1) ( (12, 4, 2) )</td>
</tr>
</tbody>
</table>

\(^{a}\) Shortened BCH codes with parameters: \( (n_{SB}, kl, t \geq k) \)

\(^{b}\) Shortened BCH codes with parameters: \( (ni, l, t \geq i) \)

By applying ceiling functions,

\[
n \geq \sum_{i=1}^{l} \left\lceil \frac{2^{i-1}s_1}{2^{kl-1}} \right\rceil + \sum_{i=l+1}^{2l} \left\lceil \frac{2^{i-1}s_2}{2^{kl-1}} \right\rceil + \cdots + \sum_{i=(k-1)l+1}^{kl} \left\lceil \frac{2^{i-1}s_k}{2^{kl-1}} \right\rceil. \quad (3.72)
\]

Therefore,

\[
n \geq \sum_{i=1}^{k} \sum_{j=il-1}^{il} \left\lceil \frac{s_i}{2^{kl-j}} \right\rceil.
\]

In Table 3.5, we show results of integer programming for the \( l \)-bit messages with \( s = (3, 5, \ldots, 2k + 1) \). For the listed \( l \) and \( k \), the optimal UEP codes are constructed by integer programming such that their lengths satisfy the integer programming bounds derived in (3.69). Generator matrices for the optimal UEP codes are constructed in Appendix A.
In addition, we compare the length of UEP codes to the length of $t$-error-correcting shortened BCH codes and the length of time sharing shortened BCH codes in Table 3.6. Similar to (3.30), for a separation vector given as $s = (3, 5, \ldots, 2k + 1)$, a minimum length of shortened BCH code that provides at least $t = \left\lfloor \frac{s_k}{2} \right\rfloor = k$ error corrections can be obtained by

$$n_{SB} = n_B - (k_B - kl) \quad (3.73)$$

where $n_B$ is a minimum length of binary BCH code whose dimension, $k_B$ is at least $kl$ and whose error correction capability is at least $t = k$. Also, a length of time sharing shortened BCH codes can be written as the sum of the length of components codes,

$$n_{TS} = \sum_{i=1}^{k} n_i \quad (3.74)$$

where $n_i$ is a minimum length of shortened BCH code whose dimension is $l$ and whose error correction capability is at least $t = \left\lfloor \frac{s_i}{2} \right\rfloor = i$.

### 3.2.3 Asymptotic code rates and throughput of broadcast channels

In the following theorem, an asymptotically achievable code rate of the optimal UEP code is derived for the case of $l$-bit messages.

**Theorem 3.4.** Let $R(l)$ be a rate of the optimal UEP code for the $l$-bit messages when the non-decreasing separation vector is given as $s = (3, 5, \ldots, 2k + 1)$. Then,

$$R(l) \approx \frac{l}{l + 4} \quad \text{when} \quad k \gg 1. \quad (3.75)$$

**Proof.** From (3.69), a length of the optimal UEP code for a given $s = (3, 5, \ldots, 2k + 1)$ can
be written as

\[ n = \sum_{i=1}^{k} \sum_{j=il-l+1}^{il} \left\lceil \frac{s_i}{2^{kl-j}} \right\rceil. \]

Since \( s_i = 2i + 1 \) for \( 1 \leq i \leq k \),

\[ n = \sum_{i=1}^{k} \sum_{j=il-l+1}^{il} \left\lceil \frac{2i + 1}{2^{kl-j}} \right\rceil. \quad (3.76) \]

Then, from (3.63),

\[ n = k \sum_{u=1}^{kl} \left\lceil \frac{2\left\lceil \frac{u}{2^{kl}} \right\rceil + 1}{2^{kl-u}} \right\rceil, \quad (3.77a) \]

\[ = \sum_{v=0}^{kl-1} \left\lceil \frac{2k + 1 - 2\left\lceil \frac{v}{2^x} \right\rceil}{2^v} \right\rceil. \quad (3.77b) \]

Let

\[ \eta_v = \left\lceil \frac{2k + 1 - 2\left\lceil \frac{v}{2^x} \right\rceil}{2^v} \right\rceil, \]

and

\[ k = a_x 2^x + a_{x-1} 2^{x-1} + \cdots + a_0 \]

where \( x = \lfloor \log_2 k \rfloor \), then

\[ \eta_v = \begin{cases} 
2k + 1 & , \quad v = 0 \\
1 & , \quad v = 1 \\
2k + 1 + a_{x-1} 2^{x-1} + \cdots + a_v 2^{x-v+1} + \delta_v, & 2 \leq v \leq x + 1 \\
1 & , \quad x + 2 \leq v \leq kl - 1 
\end{cases} \quad (3.78) \]
where $\delta_v \in \{0,1\}$.

Let $\Delta_v = \eta_v - \delta_v$ for $2 \leq v \leq x + 1$, then

$$
\Delta_v = a_x 2^{x-v+1} + a_{x-1} 2^{x-v} + \cdots + a_{v-1} 2^0
$$

(3.79)

and

$$
\sum_{v=2}^{x+1} \Delta_v = a_x (2^{x-1} + \cdots + 1) + a_{x-1} (2^{x-2} + \cdots + 1) + \cdots + a_2 (2 + 1) + a_1
$$

$$
= a_x (2^x - 1) + a_{x-1} (2^{x-1} - 1) + \cdots + a_0 (1 - 1)
$$

$$
= k - \sum_{w=0}^x a_w.
$$

(3.80)

From (3.78) and (3.80),

$$
\sum_{v=0}^{1} \eta_v = 3k + 2,
$$

(3.81a)

$$
\sum_{v=2}^{x+1} \eta_v = k - \sum_{w=0}^x a_w + \sum_{v=2}^{x+1} \delta_v,
$$

(3.81b)

and

$$
\sum_{v=x+2}^{k-1} \eta_v = kl - \lfloor \log_2 k \rfloor - 2.
$$

(3.81c)

Therefore,

$$
n = \sum_{v=0}^{k-1} \eta_v \approx (l + 4)k \quad \text{when} \quad k \gg 1,
$$

(3.82)
consequently, the code rate is converged to

\[ R(l) = \frac{kl}{n} \approx \frac{l}{l+4} \quad \text{when} \quad k \gg 1. \]

Simulation results for the rates of the UEP codes obtained by computing \( R(l) = \frac{kl}{n} \) are illustrated in Fig. 3.7 for \( 2 \leq k \leq 2^{12} \), which shows asymptotic convergence \( \frac{l}{l+4} \) for \( l = 2, 3, \) and 4 as proven in Theorem 3.4.

As explained in Section 2.2, the broadcast channel model can be viewed as \( k \) degraded component channels. Consequently, the model can be described by \( k \) cascaded BSCs with transition probabilities, \( \alpha_i \) for \( 1 \leq i \leq k \) as illustrated in Figure 2.4.

Let \( n \) satisfy the bound in (3.69) for a given separation vector \( s = (3, 5, \ldots, 2k + 1) \). It follows from (3.37) and (3.39), since the \( l \)-bit message \( \mathbf{m}_i \) is successfully delivered to the receiver \( R_i \) when the corresponding component channel introduces less than or equal to \( i \) errors, the effective transmission rate of the \( l \)-bit message \( \mathbf{m}_i \) to the receiver \( R_i \) through the
Figure 3.8: Throughput of the degraded broadcast channel for $2 \leq k \leq 2^7$
component channel can be given by

\[ \Gamma_i = \frac{1}{n} \sum_{j=0}^{i} \binom{n}{j} (1 - p_i)^{n-j} p_i^j, \quad 1 \leq i \leq k \] (3.83)

where \( p_i \) is a bit error probability of the component channel as derived in (3.38). Consequently, the throughput of the degraded broadcast channel can be given by

\[ R_T = \sum_{i=1}^{k} \Gamma_i \leq \frac{k}{n}. \] (3.84)

We illustrate the throughput of the degraded broadcast channel for the case of \( l = 2, 3, \) and 4 in Figure 3.8 when \( \alpha_i = p = \frac{1}{2n} \) for \( 1 \leq i \leq k \).

3.2.4 Decoding of UEP codes using integer programming

In this section, we extend the decoding algorithm introduced in Section 3.1.4 to decode \( l \)-bit messages, \( \mathbf{m}_i \) at each receiver \( R_i \) for \( 1 \leq i \leq k \). Since a message vector is given as \( \mathbf{m} = (\mathbf{m}_1, \mathbf{m}_2, \ldots, \mathbf{m}_k) \) where \( \mathbf{m}_i = (m_1^{(i)}, m_2^{(i)}, \ldots, m_l^{(i)}) \) for \( 1 \leq i \leq k \), each element of the received vector \( \mathbf{r}_i \) can be written as

\[ r_j = \sum_{i=1}^{k} \sum_{u=1}^{l} m_u^{(i)} g_{l(i-1)+u,j} + e_j \quad \text{for} \quad 1 \leq j \leq n \] (3.85)

where \( g_{k,j} \) represents the \( i \)-th row and the \( j \)-th column element of \( \mathbf{G} \) and \( e_j \) is a channel error. In the following, we explain the decoding method with an example of \( k = 2 \) and \( l = 2 \) to recover \( \mathbf{m}_1 = (m_1^{(1)}, m_2^{(1)}) \) at receiver \( R_1 \).
Example 3.4 \((k = 2 & l = 2)\). From Example 3.3, the corresponding generator matrix is

\[
G = \begin{pmatrix}
0 & 0 & 0 & 0 & 0 & 0 & 1 & 1 & 1 & 1 \\
0 & 0 & 1 & 1 & 0 & 0 & 0 & 0 & 0 & 0 \\
0 & 1 & 1 & 0 & 0 & 1 & 0 & 0 & 1 & 1 \\
1 & 0 & 1 & 0 & 1 & 1 & 0 & 1 & 0 & 1
\end{pmatrix}.
\]

Iterative integer programming Receiver \(R_1\) first finds subsets \(J_1^1, J_2^1, J_3^1\) using iterative integer programming to decode \(m_1^{(1)}\). From the generator matrix, we have

\[
G_1 = \{7, 8, 9, 10\},
\]

\[
G_2 = \{4, 5, 6\},
\]

\[
G_3 = \{2, 3, 6, 9, 10\},
\]

\[
G_4 = \{1, 3, 5, 6, 8, 10\}.
\]

Therefore, the integer programming problem that finds a subset \(J_h^1\) for \(1 \leq h \leq s_i\) becomes to minimize the sum \(y_1 + y_2 + \cdots + y_{10}\) satisfying

\[
y_7 + y_8 + y_9 + y_{10} - 2z_1 = 1,
\]

\[
y_4 + y_5 + y_6 - 2z_2 = 0,
\]

\[
y_2 + y_3 + y_6 + y_9 + y_{10} - 2z_3 = 0,
\]

\[
y_1 + y_3 + y_5 + y_6 + y_8 + y_{10} - 2z_4 = 0.
\]
The subsets obtained from integer programming are $J_1^1 = \{7\}$, $J_2^1 = \{2, 9\}$, and $J_3^1 = \{1, 8\}$. Since the subsets for decoding $m_1^{(1)}$ has been found, $R_1$ sets $g_{1,j} = 0$ for $j \in G_1$, and $R_1$ finds subsets $J_1^2, J_2^2, J_3^2$ to decode $m_2^{(1)}$. Since we have

$$G_1 = \{\} = \emptyset,$$

$$G_2 = \{4, 5, 6\},$$

$$G_3 = \{2, 3, 6, 9, 10\},$$

$$G_4 = \{1, 3, 5, 6, 8, 10\},$$

the integer programming problem that finds a subset $J_h^2$ for $1 \leq h \leq s_i$ becomes to minimize the sum $y_1 + y_2 + \cdots + y_{10}$ satisfying

$$y_4 + y_5 + y_6 - 2z_2 = 1,$$

$$y_2 + y_3 + y_6 + y_9 + y_{10} - 2z_3 = 0,$$

$$y_1 + y_3 + y_5 + y_6 + y_8 + y_{10} - 2z_4 = 0.$$

The subsets obtained from integer programming are $J_1^2 = \{4\}$, $J_2^2 = \{6, 10\}$, and $J_3^2 = \{1, 5\}$. 
Majority logic decoding  Upon receiving $\mathbf{r}_i = (r_1, r_2, \ldots, r_n)$, $R_1$ recovers $\mathbf{m}_1 = (m_1^{(1)}, m_2^{(1)})$ using majority logic based on the subsets found from iterative integer programming. Since the subsets for $m_1^{(1)}$ are $J_1^1 = \{7\}$, $J_2^1 = \{2, 9\}$, and $J_3^1 = \{1, 8\}$,

$$\hat{r}_1 = r_7 = m_1^{(1)} + e_7,$$

$$\hat{r}_2 = r_2 + r_9 = \left( m_1^{(2)} + e_2 \right) + \left( m_1^{(1)} + m_2^{(2)} + e_9 \right) = m_1^{(1)} + (e_2 + e_9),$$

$$\hat{r}_3 = r_1 + r_8 = \left( m_2^{(2)} + e_1 \right) + \left( m_1^{(1)} + m_2^{(2)} + e_8 \right) = m_1^{(1)} + (e_1 + e_8).$$

Consequently, $m_1^{(1)}$ can be determined by majority logic if $\sum_{j} e_j \leq t_i$.

To cancel out $m_1^{(1)}$ in the received vector, $R_1$ updates $\mathbf{r}_i = (r_1, r_2, \ldots, r_n)$ by

$$r_j = r_j + m_1^{(1)} \quad \text{for} \quad j \in \mathcal{G}_1,$$

i.e.,

$$r_7 = r_7 + m_1^{(1)} = m_1^{(2)} + m_1^{(1)} + e_7,$$

$$r_8 = r_8 + m_1^{(1)} = m_1^{(2)} + m_2^{(1)} + m_2^{(2)} + e_8,$$

$$r_9 = r_9 + m_1^{(1)} = m_2^{(2)} + m_1^{(1)} + m_1^{(2)} + e_9,$$

$$r_{10} = r_{10} + m_1^{(1)} = m_2^{(2)} + m_1^{(1)} + m_2^{(2)} + m_2^{(1)} + e_{10}.$$

Then, $R_1$ use the subsets $J_1^2 = \{4\}$, $J_2^2 = \{6, 10\}$, and $J_3^2 = \{1, 5\}$ to obtain the following
modified received bits:

\[
\hat{r}_1 = r_4 = m_2^{(1)} + e_4,
\]

\[
\hat{r}_2 = r_6 + r_{10} = \left( m_2^{(1)} + m_1^{(2)} + m_2^{(2)} + e_6 \right) + \left( m_1^{(2)} + m_2^{(2)} + e_{10} \right) = m_2^{(1)} + (e_6 + e_{10}),
\]

\[
\hat{r}_3 = r_1 + r_5 = \left( m_2^{(2)} + e_1 \right) + \left( m_2^{(1)} + m_2^{(2)} + e_5 \right) = m_2^{(1)} + (e_1 + e_5).
\]

Consequently, \( R_1 \) recovers \( m_2^{(1)} \) by majority logic if \( \sum_{j} e_j \leq t_i \). Complete decoding procedures are listed in Table 3.7 for receivers \( R_1 \) and \( R_2 \) with a message vector \( m = (1, 1, 1, 1) \) and the corresponding codewords \( c = (1, 1, 0, 1, 0, 0, 0, 1) \).

In general, \( R_i \) first finds subsets \( \mathcal{J}_1^u, \mathcal{J}_2^u, \ldots, \mathcal{J}_{s_i}^u \) using iterative integer programming for \( 1 \leq u \leq l \). Then, upon receiving the received bit \( r_i \), the receiver \( R_i \) applies majority logic on the modified received bits,

\[
\hat{r}_h = \sum_{j \in \mathcal{J}_h^u} r_j = m_u^{(i)} + \sum_{j \in \mathcal{J}_h^u} e_j \quad \text{for} \quad 1 \leq h \leq s_i \quad (3.86)
\]

to determine \( m_u^{(i)} \), and \( R_i \) repeats procedures for \( 1 \leq u \leq l \). The detailed descriptions of the decoding algorithm is shown in Algorithm 2, and diagrams of the iterative integer programming and the majority logic decoding are illustrated in Fig. 3.9.
Algorithm 2 Decoding algorithm at \( R_i \) for \( l \)-bit message

1: **procedure** \textsc{Iterative Integer Programming} \\
2: \[ u \leftarrow 0 \] \\
3: \textbf{repeat} \hspace{1cm} \triangleright \text{Finding subsets for } m_{u}^{(i)} \\
4: \hspace{1cm} u \leftarrow u + 1 \\
5: \hspace{1cm} v \leftarrow l(i - 1) + u \\
6: \hspace{1cm} \text{Formulate an integer programming problem} \\
7: \hspace{1cm} \begin{align*}
\min & \quad y_1 + y_2 + \cdots + y_n \\
\text{s.t.} & \quad G y^\top - 2 z^\top = i_v
\end{align*}
8: \textbf{end procedure} \\
9: \text{Upon receiving } r_i = (r_1, r_2, \ldots, r_n) \\
10: **procedure** \textsc{Majority Logic Decoding} \\
11: \[ u \leftarrow 0 \] \\
12: \textbf{repeat} \hspace{1cm} \triangleright \text{Determine } m_{u}^{(i)} \\
13: \hspace{1cm} u \leftarrow u + 1 \\
14: \hspace{1cm} h \leftarrow 0 \\
15: \hspace{1cm} \textbf{repeat} \hspace{1cm} \triangleright \text{Modifying received bits} \\
16: \hspace{2cm} h \leftarrow h + 1 \\
17: \hspace{2cm} \hat{r}_h = \sum_{j \in J_h^u} r_j \\
18: \hspace{2cm} \textbf{until } h = s_i \\
19: \hspace{2cm} \text{if } \sum_{h=1}^{s_i} \hat{r}_h \leq \left\lfloor \frac{s_i}{2} \right\rfloor \text{ then} \hspace{1cm} \triangleright \text{Majority logic} \\
20: \hspace{2cm} \hat{m}_{u}^{(i)} \leftarrow 0 \\
21: \hspace{2cm} \text{else} \\
22: \hspace{2cm} \hat{m}_{u}^{(i)} \leftarrow 1 \\
23: \hspace{2cm} \text{end if} \\
24: \hspace{1cm} r_j \leftarrow r_j + \hat{m}_{u}^{(i)} \text{ for } j \in G_{l(i-1)+u} \\
25: \hspace{1cm} \textbf{until } u = l \\
26: \textbf{end procedure}
Table 3.7: Decoding example for $l = 2$ and $k = 2$

$r_1 = (1, 1, 0, 1, 0, 1, 0, 1, 1) \text{ at } R_1$

<table>
<thead>
<tr>
<th>$u$</th>
<th>$h$</th>
<th>$\mathcal{H}_h$</th>
<th>$\hat{r}_h$</th>
</tr>
</thead>
<tbody>
<tr>
<td>1</td>
<td>1</td>
<td>{7}</td>
<td>$\hat{r}_1 = r_7 = 1$</td>
</tr>
<tr>
<td>1</td>
<td>2</td>
<td>{2, 9}</td>
<td>$\hat{r}_2 = r_2 + r_9 = 0$</td>
</tr>
<tr>
<td>1</td>
<td>3</td>
<td>{1, 8}</td>
<td>$\hat{r}_3 = r_1 + r_8 = 1 \rightarrow m_1^{(1)} = 1$</td>
</tr>
</tbody>
</table>

$r_1 \leftarrow r_1 + (0, 0, 0, 0, 0, 0, 1, 1, 1)\,$

$r_1 = (1, 1, 0, 1, 0, 1, 0, 1, 0)\,$

<table>
<thead>
<tr>
<th>$u$</th>
<th>$h$</th>
<th>$\mathcal{H}_h$</th>
<th>$\hat{r}_h$</th>
</tr>
</thead>
<tbody>
<tr>
<td>2</td>
<td>1</td>
<td>{4}</td>
<td>$\hat{r}_1 = r_4 = 1$</td>
</tr>
<tr>
<td>2</td>
<td>2</td>
<td>{6, 10}</td>
<td>$\hat{r}<em>2 = r_6 + r</em>{10} = 1$</td>
</tr>
<tr>
<td>2</td>
<td>3</td>
<td>{1, 5}</td>
<td>$\hat{r}_3 = r_1 + r_5 = 1 \rightarrow m_2^{(1)} = 1$</td>
</tr>
</tbody>
</table>

$r_2 = (1, 1, 0, 1, 0, 1, 1, 1, 1) \text{ at } R_2$

<table>
<thead>
<tr>
<th>$u$</th>
<th>$h$</th>
<th>$\mathcal{H}_h$</th>
<th>$\hat{r}_h$</th>
</tr>
</thead>
<tbody>
<tr>
<td>1</td>
<td>1</td>
<td>{2}</td>
<td>$\hat{r}_1 = r_2 = 1$</td>
</tr>
<tr>
<td>1</td>
<td>2</td>
<td>{7, 9}</td>
<td>$\hat{r}_2 = r_7 + r_9 = 0$</td>
</tr>
<tr>
<td>1</td>
<td>3</td>
<td>{1, 3}</td>
<td>$\hat{r}_3 = r_1 + r_3 = 1$</td>
</tr>
<tr>
<td>1</td>
<td>4</td>
<td>{8, 10}</td>
<td>$\hat{r}<em>4 = r_8 + r</em>{10} = 0$</td>
</tr>
<tr>
<td>1</td>
<td>5</td>
<td>{5, 6}</td>
<td>$\hat{r}_5 = r_5 + r_6 = 1 \rightarrow m_1^{(2)} = 1$</td>
</tr>
</tbody>
</table>

$r_2 \leftarrow r_2 + (0, 1, 1, 0, 0, 1, 0, 0, 1)\,$

$r_2 = (1, 0, 1, 1, 0, 0, 1, 1, 0, 0)\,$

<table>
<thead>
<tr>
<th>$u$</th>
<th>$h$</th>
<th>$\mathcal{H}_h$</th>
<th>$\hat{r}_h$</th>
</tr>
</thead>
<tbody>
<tr>
<td>1</td>
<td>1</td>
<td>{1}</td>
<td>$\hat{r}_1 = r_1 = 1$</td>
</tr>
<tr>
<td>1</td>
<td>2</td>
<td>{3}</td>
<td>$\hat{r}_2 = r_3 = 1$</td>
</tr>
<tr>
<td>1</td>
<td>3</td>
<td>{9, 10}</td>
<td>$\hat{r}<em>3 = r_9 + r</em>{10} = 0$</td>
</tr>
<tr>
<td>1</td>
<td>4</td>
<td>{7, 8}</td>
<td>$\hat{r}_4 = r_7 + r_8 = 0$</td>
</tr>
<tr>
<td>1</td>
<td>5</td>
<td>{4, 6}</td>
<td>$\hat{r}_5 = r_4 + r_6 = 1 \rightarrow m_2^{(2)} = 1$</td>
</tr>
</tbody>
</table>

### 3.3 Discussions

#### 3.3.1 On the complexity of UEP code construction

In Section 3.1.1 (also, in Section 3.2.1), we introduce an integer programming approach to construct optimal UEP codes for $k$ users in broadcast communications. Essentially,
when a separation vector \( s = (s_1, s_2, \ldots, s_k) \) is given, an integer programming problem is formulated based on a basis matrix, \( A_b \) where \( A_b \) is \( k \times (2^k - 1) \) matrix consisting of all nonzero binary \( k \)-tuples as columns in increasing order. Then the UEP code construction becomes to minimize the sum \( x_1 + x_2 + \cdots + x_{2^k-1} \) subject to satisfying certain linear constraints.

However, we observe that the number of variables for the objective function, \( x_1 + x_2 + \)
\( \cdots + x_{2^k - 1} \) exponentially increases as the number of users, \( k \) is increased. Furthermore, since integer programming is NP-hard problem, it may not provide an optimal solution in reasonable time for a large number of variables as results indicate in Section 3.1.2. These observations make the integer programming approach less practical when \( k \) is a large number; hence, we wish to direct further researches on the complexity of the integer programming approach. In the following, we present an idea to reduce the complexity of the approach.

**UEP code construction based on shortened BCH codes** In the proposed integer programming approach, we use a \( k \times (2^k - 1) \) basis matrix, but we can reduce the complexity of integer programming significantly by using a generator matrix of a binary BCH code as the basis matrix. Suppose that a non-decreasing separation vector is given as \( s = (s_1, s_2, \ldots, s_k) \), then the UEP code construction based on shortened BCH codes can be described by the following procedures.

1. Choose a binary BCH code whose dimension is at least \( k \) and whose error correction capability is at least \( t = \lfloor \frac{n_B}{2} \rfloor = k \), and let the parameters of the BCH code be \((n_B, k_B, t)\).

2. Obtain a shortened the BCH code with parameters \((n_{SB}, k, t)\) where \( n_{SB} = n_B - (k_B - k) \).

   - example for \( k = 5 \): \((31, 11, 5)\) BCH code → \((25, 5, 5)\) shortened BCH code.

3. Set the generator matrix of the shortened BCH code as the basis matrix \( A_b \).
- example for \( k = 5 \):

\[
\begin{bmatrix}
1010101101100100011010000 \\
01010101110100110001101000 \\
001010101101100110001101000 \\
000101011011100110001101000 \\
000010110111100110001101000
\end{bmatrix}
\]

4. Formulate integer programming as described in section 3.1.1.

5. Find the optimal solution to the formulated problem.

- example for \( k = 5 \): optimal value \( n = 21 \) where

\[
\begin{array}{cccccccccc}
x_4 & x_7 & x_{10} & x_{11} & x_{13} & x_{15} & x_{16} & x_{17} & x_{23} & x_{25} \\
2 & 1 & 1 & 1 & 2 & 2 & 1 & 3 & 1 & 2 & 5
\end{array}
\]

hence,

\[
\begin{bmatrix}
00011110000000000000000 \\
11001001100001000000000 \\
00110110010000110000000 \\
11011110001110000000000 \\
00101001100001111111111
\end{bmatrix}
\]

As it is shown in the example of \( k = 5 \), the complexity of integer programming is reduced since the number of variables are reduced from 31 (see Section 3.1.1) to 25. However, since the dimension of basis matrix \( A_b \) is decreased to reduce the complexity, the optimal solution from integer programming no longer guarantees to satisfy the bound derived in Section 3.1.2. Therefore, there is a trade-off between the complexity of UEP code construction and the
efficiency of the codes as we compared in Table 3.8. From the observation, reducing the complexity of the integer programming approach would be an interesting subject to research.

### 3.3.2 On the decodability of the UEP decoding algorithm

From Section 3.1.1, we find an integer programming solution denoted by \( x = (x_1, x_2, \ldots, x_{2^k-1}) \) whose nonzero components construct a generator matrix of a UEP code. Let \( \mathcal{I} \) be an index set for the nonzero components of \( x \), i.e.,

\[
\mathcal{I} = \left\{ j \mid x_j \neq 0, \ 1 \leq j \leq 2^k - 1 \right\}, \quad (3.87)
\]

and let \( \mathcal{I}_h \) be a subset of \( \mathcal{I} \) for \( 1 \leq h \leq s_i \). Then, for a given \( i \), the sets \( \mathcal{I}_h \) for \( 1 \leq h \leq s_i \) satisfy (3.47) if

\[
\sum_{j \in \mathcal{I}_h} q_j = i_i \quad \text{for} \quad 1 \leq h \leq s_i \quad (3.88)
\]
under modulo-2 additions where \( q_j \) is the \( j \)-th column of \( A_b \) from (3.8), i.e.,
\[
A_b = \begin{pmatrix}
a_{1,1} & a_{1,2} & \ldots & a_{1,2^k-1} \\
a_{2,1} & a_{2,2} & \ldots & a_{2,2^k-1} \\
\vdots & \vdots & \ddots & \vdots \\
a_{k,1} & a_{k,2} & \ldots & a_{k,2^k-1}
\end{pmatrix}
\]
\[
= (q_1, q_2, \ldots, q_{2^k-1}) \tag{3.89}
\]
and \( i \) is \( i \)-th column of \( k \times k \) identity matrix.

Let \( x_h = (x_1^{(h)}, x_2^{(h)}, \ldots, x_{2^k-1}^{(h)}) \) be defined as
\[
x_j^{(h)} \triangleq \begin{cases} 
1 & \text{if } j \in I_h \\
0 & \text{otherwise}
\end{cases} \text{ for } 1 \leq j \leq 2^k - 1. \tag{3.90}
\]

If
\[
\sum_{h=1}^{s_i} x_j^{(h)} \leq x_j \, \forall j, \tag{3.91}
\]
then the \( s_i \) numbers of disjoint subsets in Theorem 3.3 exist. Therefore, if the integer programming solution \( x \) satisfies (3.88) and (3.91) for \( 1 \leq i \leq k \), the corresponding UEP code is majority-logic-decodable by the proposed decoding algorithm. For example, the optimal UEP codes shown in Table 3.2 have the \( s_i \) numbers of the disjoint subsets, hence they are majority-logic-decodable.
Modified integer programming approach of UEP code construction

Let $A_i$ be an index set for $i$-th row of $A_b$ that has non-zero component, i.e.,

$$
A_i = \{ j | a_{i,j} = 1, 1 \leq j \leq 2^k - 1 \}.
$$

Then, consider the variable $x_j$ for a given $i$ that satisfies the following constraints:

\begin{align*}
    x_j &\geq 1, \quad j \neq \xi, j \in A_i \quad (3.92a) \\
    x_{j'} - x_j &\geq 0, \quad j' = j - \xi \quad (3.92b)
\end{align*}

where $\xi = 2^{k-i}$. Recall that if $x_j \geq 1$, then $q_j$ appears $x_j$ times in columns of $G$. Consequently, the constraints (3.92) guarantee that if $q_j$ appears $x_j$ times in columns of $G$, then $q_{j'}$ appears at least $x_j$ times in columns of $G$. Furthermore, since

$$
q_j + q_{j'} = i_i
$$

where $i_i$ is $i$-th column of $k \times k$ identity matrix, the constraints (3.92) also guarantee that there exist $x_j$ numbers of subsets that satisfy (3.47) if $x_j \geq 1$ for $j \neq \xi$ and $j \in A_i$.

Let a binary indicator variable $w_{ij}$ be defined as

$$
w_{ij} \triangleq \begin{cases} 
    1 & \text{if } x_j \geq 1 \text{ and } x_{j'} - x_j \geq 0 \\
    0 & \text{otherwise}
\end{cases} \quad (3.93)
$$

for $j \in A_i$, $j \neq \xi$, and $1 \leq i \leq k$. Then, there exist $s_i$ numbers of disjoint subsets that satisfy (3.47) if

$$
\sum_{\substack{j \neq \xi \\\n    j \in A_i}} w_{ij} x_j + x_\xi \geq s_i \quad \text{for } 1 \leq i \leq k. \quad (3.94)
$$
Therefore, (3.94) can be additional constraints for integer programming so that the corresponding UEP codes are majority-logic-decodable.

The logical constraints in (3.93) can be rewritten as integer programming constraints. First, let binary indicator variables $u_{ij}$ and $v_{ij}$ be

$$u_{ij} = 1 \text{ if } x_j \geq 1,$$

$$v_{ij} = 1 \text{ if } x_j' - x_j \geq 0.$$  \hspace{1cm} (3.95a)

Then, since $w_{ij} = u_{ij}v_{ij}$, the indicator variable $w_{ij}$ can be expressed with the following inequalities:

$$u_{ij} + v_{ij} - 1 \leq 2w_{ij} \leq u_{ij} + v_{ij}.$$  \hspace{1cm} (3.96)

Similarly, the quadratic terms (i.e., $w_{ij}x_j$) in (3.94) can be rewritten as linear constraints by introducing artificial variables $z_{ij}$ such that $z_{ij} = w_{ij}x_j$. Suppose the variables $x_j$ are bounded by $0 \leq x_j \leq M$ for $1 \leq j \leq 2^k - 1$ where $M$ is a sufficiently large constant. Then, $z_{ij}$ can be expressed with the following pairs of inequalities:

$$0 \leq z_{ij} \leq Mw_{ij},$$  \hspace{1cm} (3.97a)

$$x_j - M(1 - w_{ij}) \leq z_{ij} \leq x_j.$$  \hspace{1cm} (3.97b)

Therefore, from the integer programming problem formulated in Section 3.1.1 and the additional constraints (3.94), we can construct UEP codes that are majority-logic-decodable.
Modified UEP code construction

Minimize

\[ n = x_1 + x_2 + \cdots + x_{2^k-1} \]

subject to

\[ \mathbf{A} \mathbf{x}^\top \geq \mathbf{b}^\top, \]

\[ \sum_{j \neq 2^{k-i}, j \in A_i} z_{ij} + x_{2^k-i} \geq s_i, \quad \text{for} \quad 1 \leq i \leq k, \]

where

\[ 0 \leq z_{ij} \leq Mw_{ij}, \]

\[ x_j - M(1 - w_{ij}) \leq z_{ij} \leq x_j. \]

3.3.3 On the non-binary UEP code construction

The integer programming approach to construct binary UEP codes can be extended to construct non-binary UEP codes. Let the \( l \)-bit message \( \mathbf{m}_i = (m_{1}^{(i)}, m_{2}^{(i)}, \ldots, m_{l}^{(i)}) \) for \( 1 \leq i \leq k \) be represented with symbols in \( \mathbb{GF}(q) \) where \( q = 2^l \), then, using the integer programming approach introduced in Section 3.1.1, we construct non-binary UEP codes over \( \mathbb{GF}(q) \) with a given separation vector \( \mathbf{s} = (s_1, s_2, \ldots, s_k) \) where \( s_i = 2t_i + 1 \) for \( 1 \leq i \leq k \), which satisfies

\[ w_H(\mathbf{m}\mathbf{G}) \geq s_i, \quad m_i \neq 0 \quad \text{for} \quad 1 \leq i \leq k. \quad (3.98) \]

where \( \mathbf{m} = (m_1, m_2, \ldots, m_k) \) and \( m_1, m_2, \ldots, m_k \in \mathbb{GF}(q) \).

Let the basis matrix \( \mathbf{A}_b \) be a \( k \times (q^k - 1) \) matrix consisting of all nonzero \( k \)-tuples over
as columns in increasing order; for $\mathbb{GF}(q) = \{0, 1, \alpha, \alpha^2, \ldots, \alpha^{q-2}\}$,

$$
A_b = \begin{pmatrix}
00 0 \cdots \alpha^{q-2} \\
00 0 \cdots \alpha^{q-2} \\
\vdots & \vdots & \ddots & \vdots \\
1\alpha \alpha^2 \cdots \alpha^{q-2} \\
\end{pmatrix}
= \begin{pmatrix}
a_1 \\
a_2 \\
\vdots \\
a_k \\
\end{pmatrix},
$$

(3.99)

and, for any vector $v = (v_1, v_2, \ldots, v_w)$ over $\mathbb{GF}(q)$, let us define $[v] = (\hat{v}_1, \hat{v}_2, \ldots, \hat{v}_w)$ as

$$
\hat{v}_j = \begin{cases}
0 & \text{if } v_j = 0 \\
1 & \text{if } v_j \neq 0
\end{cases}
\quad \text{for } 1 \leq j \leq w.
$$

(3.100)

Then, similar to the formulation in Section 3.1.1, we can have the following inequalities for integer programming,

$$
A_i x^\top \geq b_i^\top \quad \text{for } 1 \leq i \leq k
$$

(3.101)

where $A_i$ is a $q^i - 1 \times (q^k - 1)$ matrix whose rows are

$$
[a_1] \quad \text{if } i = 1,
$$

(3.102a)

$$
[a_i + \sum_{u=1}^{i-1} \omega_u a_i] \quad \text{if } 2 \leq i \leq k
$$

(3.102b)

where $w_u \in \mathbb{GF}(q)$ for all $u$,

$$
x = (x_1, x_2, \ldots, x_{q^k-1}),
$$

(3.103)

and

$$
b_i = (s_{i,1}, s_{i,2}, \ldots, s_{i,q^{k-1}}) \quad \text{for } 1 \leq i \leq k.
$$

(3.104)
Based on (3.101), we can formulate integer programming problem for non-binary UEP code construction when a non-decreasing separation vector $s = (s_1, s_2, \ldots, s_k)$ is given:

**UEP code construction over $\mathbb{GF}(q)$**

Minimize

$$n = x_1 + x_2 + \cdots + x_{q^k-1}$$

subject to

$$Ax^\top \geq b^\top$$

where

$$A = \begin{pmatrix} A_1 \\ A_2 \\ \vdots \\ A_k \end{pmatrix}, \quad b^\top = \begin{pmatrix} b_1^\top \\ b_2^\top \\ \vdots \\ b_k^\top \end{pmatrix}$$

**Example 3.5** ($k = 2 \& l = 2$). Let $GF(2^2) = \{0, 1, \alpha, \alpha^2 = \alpha + 1\}$ and $s = (3, 5)$, then, from (3.99),

$$A_b = \begin{pmatrix} 0 & 0 & 1 & 1 & 1 & \alpha & \alpha & \alpha & \alpha^2 & \alpha^2 & \alpha^2 \\ 1 & \alpha & \alpha^2 & 0 & 1 & \alpha & \alpha^2 & 0 & 1 & \alpha & \alpha^2 \end{pmatrix} = \begin{pmatrix} a_1 \\ a_2 \end{pmatrix}.$$
and, from (3.102a),

\[ \mathbf{A}_1 = \begin{pmatrix} 000111111111111 \end{pmatrix} = \mathbf{a}_1, \]

\[ \mathbf{A}_2 = \begin{pmatrix} 111011101101111 \\ 111101111011110 \\ 111110111101011 \\ 111111010111101 \\ 111111010111111 \end{pmatrix} = \begin{pmatrix} \mathbf{a}_2 \\ \mathbf{a}_2 + \mathbf{a}_1 \\ \mathbf{a}_2 + \alpha \mathbf{a}_1 \\ \mathbf{a}_2 + \alpha^2 \mathbf{a}_1 \end{pmatrix}. \]

Therefore, the UEP code construction is to find \( \mathbf{x} \) that minimizes the sum \( x_1 + x_2 + \cdots + x_{15} \) satisfying

\[ x_4 + x_5 + x_6 + x_7 + x_8 + x_9 + x_{10} + x_{11} + x_{12} + x_{13} + x_{14} + x_{15} \geq 3 \]

\[ x_1 + x_2 + x_3 + x_5 + x_6 + x_7 + x_9 + x_{10} + x_{11} + x_{13} + x_{14} + x_{15} \geq 5 \]

\[ x_1 + x_2 + x_3 + x_4 + x_6 + x_7 + x_8 + x_9 + x_{11} + x_{12} + x_{13} + x_{14} \geq 5 \]

\[ x_1 + x_2 + x_3 + x_4 + x_5 + x_7 + x_8 + x_9 + x_{10} + x_{12} + x_{14} + x_{15} \geq 5 \]

\[ x_1 + x_2 + x_3 + x_4 + x_5 + x_6 + x_8 + x_{10} + x_{11} + x_{12} + x_{13} + x_{15} \geq 5. \]

The optimal solution obtained from integer programming is

\[ n = \sum_{j=1}^{15} x_j = 6 \]
Table 3.9: Length comparisons between optimal UEP codes and punctured RS codes over $\mathbb{GF}(q)$ where $q = 2^k$

<table>
<thead>
<tr>
<th>$k$</th>
<th>$q$</th>
<th>UEP codes</th>
<th>punctured RS codes</th>
</tr>
</thead>
<tbody>
<tr>
<td>4</td>
<td>16</td>
<td>12</td>
<td>12</td>
</tr>
<tr>
<td>5</td>
<td>32</td>
<td>15</td>
<td>15</td>
</tr>
<tr>
<td>6</td>
<td>64</td>
<td>18</td>
<td>18</td>
</tr>
<tr>
<td>7</td>
<td>128</td>
<td>21</td>
<td>21</td>
</tr>
<tr>
<td>8</td>
<td>256</td>
<td>24</td>
<td>24</td>
</tr>
</tbody>
</table>

where

\[
\begin{align*}
&x_2 \ x_6 \ x_7 \ x_{10} \ x_{12} \\
&2 \ 1 \ 1 \ 1 \ 1
\end{align*}
\]

Consequently, the corresponding generator matrix is

\[
G = \begin{pmatrix}
0 & 0 & 1 & 1 & \alpha & \alpha^2 \\
\alpha & \alpha & \alpha & \alpha^2 & \alpha & 0
\end{pmatrix}.
\]

Similar to Theorem 3.1, an integer programming bound on a length of the non-binary UEP code can be given by

\[
n \geq \sum_{i=1}^{k} \left\lceil \frac{s_i}{q^{k-1}} \right\rceil.
\]  

(3.105)

In Table 3.9, lengths of the optimal binary UEP codes over $\mathbb{GF}(q)$ that satisfy the bound (3.105)\(^3\) are provided for a given separation vector $s = (3, 5, \ldots, 2k + 1)$ with comparison to lengths of the $t$-error-correcting punctured RS codes where $t = \left\lfloor \frac{s_k}{2} \right\rfloor = k$. We observe that there is no difference between the lengths of UEP codes over $\mathbb{GF}(q)$ and the lengths the punctured RS codes.

\(^3\)Derivation of (3.105) given in Appendix B
Chapter 4: Deterministic network coding for reliable packet transmissions on single-hop broadcast network

Network coding concept has been adopted to many applications in order to give benefits over traditional store-and-forward networks by allowing a network node to combine packets before transmitting. Consider a single-hop, single-source, and, multiple-receiver broadcast network depicted in Figure 1.1, traditional network protocol provides reliable packet transmissions over the broadcast network by either a forward error correction (FEC) or a retransmission (ARQ). In this chapter we provide a unified solution for reliable packet transmissions on the broadcast network by applying a deterministic approach of linear network coding into both forward error correction scheme and retransmission scheme.

4.1 Deterministic network coding

Practical approach of applying linear network coding to a packet retransmission scheme is to choose coding coefficients uniformly at random from a large enough finite field and inject coding coefficients in the packet header so that receivers can decode [71]. To eliminate the overhead caused by injecting encoding information in the packet header, we apply a deterministic approach to choose coding coefficients to encode packets; in other words, the coding coefficients are known to both a sender and receivers.

4.1.1 Reed-Solomon codes

Reed-Solomon (RS) code is a widely applied error correcting code in many applications. Conventional $t$-error-correcting $(n, k, d)$ RS code is described by the parameters the length of the code $n$, the dimension $k$, and the minimum distance $d$ where $d = n - k + 1$ and $n - k = 2t$. 


Code construction

We define a generator matrix of \((n, k, n-k+1)\) Reed-Solomon code by following the original formulation of Reed and Solomon in [75]. Let \(G_{RS}\) be the \(k \times n\) generator matrix for the \((n, k, n-k+1)\) RS code, then

\[
G_{RS} \triangleq \begin{pmatrix}
1 & 1 & 1 & \cdots & 1 \\
1 & \alpha & \alpha^2 & \cdots & \alpha^{n-1} \\
\vdots & \vdots & \vdots & \ddots & \vdots \\
1 & \alpha^{k-1} & (\alpha^2)^{k-1} & \cdots & (\alpha^{n-1})^{k-1}
\end{pmatrix}
\]

(4.1)

where \(\alpha\) is a primitive element in \(\mathbb{GF}(2^m)\) whose order is \(n = 2^m - 1\) and \(k < n\). Let \(p = (p_0, p_1, \ldots, p_{k-1})\) consist of \(k\) symbols in \(\mathbb{GF}(2^m)\) with its polynomial representation,

\[
P(x) = \sum_{i=0}^{k-1} p_i x^i = p_0 + p_1 x + p_2 x^2 + \cdots + p_{k-1} x^{k-1},
\]

then a codeword, \(\mathbf{c} = (c_0, c_1, \ldots, c_{n-1})\) can be written as\(^1\)

\[
\mathbf{c} = p \cdot G_{RS} = (P(1) \ P(\alpha) \ P(\alpha^2) \ \cdots \ P(\alpha^{n-1})).
\]

Let \(C(x) = c_0 + c_1 x + c_2 x^2 + \cdots + c_{n-1} x^{n-1}\) be a polynomial representation of codeword

\(^1\)The original formulation of code in [75] encoded with all elements of \(\mathbb{GF}(2^m)\), i.e., \(\mathbf{c} = (P(0) \ P(\alpha) \ P(\alpha^2) \ \cdots \ P(\alpha^{n-1}) \ P(1))\). We note that the \((n, k, n-k+1)\) RS code is encoded with only non-zero elements for this dissertation, i.e., \(\mathbf{c} = (P(1) \ P(\alpha) \ P(\alpha^2) \ \cdots \ P(\alpha^{n-1}))\).
c, then

\[
C(\alpha^h) = \sum_{j=0}^{n-1} c_j (\alpha^h)^j
\]

\[
= \sum_{j=0}^{n-1} \left( \sum_{i=0}^{k-1} p_i (\alpha^i)^j \right) (\alpha^h)^j
\]

\[
= \sum_{i=0}^{k-1} p_i \sum_{j=0}^{n-1} \alpha^{(i+h)j}
\]

\[
= \sum_{i=0}^{k-1} p_i \frac{\alpha^{(i+h)n} + 1}{\alpha^{(i+h)} + 1}.
\]

Since

\[
\frac{\alpha^{(i+h)n} + 1}{\alpha^{(i+h)} + 1} = 0 \quad \text{for} \quad i + h \neq n \quad \text{and} \quad 0 \leq i \leq k - 1,
\]

(4.2)

\(C(x)\) have \(\alpha, \alpha^2, \ldots \alpha^{n-k}\) as its roots; therefore, the code generated by \(G_{RS}\) is Reed-Solomon code with the minimum distance of \(n - k + 1\) and its corresponding parity check matrix can be defined as

\[
H_{RS} \triangleq \begin{pmatrix}
1 & \alpha & \alpha^2 & \ldots & \alpha^{n-1} \\
1 & \alpha^2 & (\alpha^2)^2 & \ldots & (\alpha^2)^{n-1} \\
1 & \alpha^3 & (\alpha^3)^2 & \ldots & (\alpha^3)^{n-1} \\
\vdots & \vdots & \vdots & \ddots & \vdots \\
1 & \alpha^{n-k} & (\alpha^{n-k})^2 & \ldots & (\alpha^{n-k})^{n-1}
\end{pmatrix}.
\]

(4.3)

Punctured RS codes

Reed-Solomon code is a maximum distance separable (MDS) code which satisfies the Singleton bound with equality. One property of MDS codes is that a punctured MDS code
is also maximum distance separable. Generally, a punctured MDS code can be obtained by deleting columns of its generator matrix. Let $G^{(u)}_{RS}$ denote a generator matrix of the punctured RS code by deleting the last $u$ columns of $k \times n$ generator matrix defined in (4.1),

\[
G^{(u)}_{RS} \triangleq \begin{pmatrix}
1 & 1 & 1 & \cdots & 1 \\
1 & \alpha & \alpha^2 & \cdots & \alpha^{n-u-1} \\
1 & \alpha^2 & (\alpha^2)^2 & \cdots & (\alpha^{n-u-1})^2 \\
\vdots & \vdots & \vdots & \ddots & \vdots \\
1 & \alpha^{k-1} & (\alpha^2)^{k-1} & \cdots & (\alpha^{n-u-1})^{k-1}
\end{pmatrix}.
\]

(4.4)

Since deleting the last $u$ columns of $G_{RS}$ can reduce minimum distance by at most $u$, the minimum distance of punctured code is greater than or equal to $n-k+1-u$. Furthermore, since the Singleton bound implies that the minimum distance of $(n-u, k, d-u)$ punctured RS code is less than or equal to $n-u-k+1$, the code generated by $G^{(u)}_{RS}$ has the minimum distance of $n-u-k+1$.

4.1.2 Deterministic linear network codes

Using the generator matrix of the Reed-Solomon code in (4.1), we can construct a deterministic linear network code for a single-hop broadcast network (Figure 1.1). Suppose a single source in the broadcast network has $k$ packets to broadcast. Each packet is represented as $s$ symbols in a finite field, $GF(2^m)$. A linear network coding allows the broadcasting source to transmit $l$ linearly encoded packets instead of transmitting $k$ uncoded packets. Let $p_i = (p_{0,i}, p_{1,i}, \ldots, p_{(s-1),i})^T$ be a column vector of $i$-th uncoded packet and $c_j = (c_{0,j}, c_{1,j}, \ldots, c_{(s-1),j})^T$ be a column vector of $j$-th encoded packet, then an encoded packet with a deterministic linear network code can be described by

\[
c_j = \sum_{i=0}^{k-1} p_i \alpha^{ij} \quad \text{for} \quad 0 \leq j \leq l-1
\]

(4.5)
where \( \alpha \) is a primitive element in \( \mathbb{F}(2^m) \) whose order is \( n = 2^m - 1 \) and \( k, l < n \). We represent our deterministic linear network coding model as the following:

\[
C_{s \times l} = P_{s \times k} G_{k \times l}
\]

where \( C_{s \times l} \) is a \( s \times l \) matrix whose columns are linearly encoded packets, \( P_{s \times k} \) is a \( s \times k \) matrix whose columns are uncoded packets, and \( G_{k \times l} \) is a \( k \times l \) generator matrix of deterministic linear network code defined as

\[
G_{k \times l} \triangleq \begin{pmatrix}
1 & 1 & 1 & \cdots & 1 \\
1 & \alpha & \alpha^2 & \cdots & \alpha^{l-1} \\
1 & \alpha^2 & (\alpha^2)^2 & \cdots & (\alpha^{l-1})^2 \\
\vdots & \vdots & \vdots & \ddots & \vdots \\
1 & \alpha^{k-1} & (\alpha^2)^{k-1} & \cdots & (\alpha^{l-1})^{k-1}
\end{pmatrix}.
\]

We note that the generator matrix of the deterministic linear network code, \( G_{k \times l} \), is obtained from puncturing last \( n - l \) columns of generator matrix of \((n, k, n - k + 1)\) RS code (i.e., \( G_{k \times l} = G_{RS}^{(n-l)} \)). As a result, a code generated by \( G_{k \times l} \) has a minimum distance of \( l - k + 1 \).

### 4.2 Deterministic network coding for reliable packet transmission

#### 4.2.1 Packet retransmissions using deterministic network coding

In a single-hop broadcast network, traditional packet retransmission scheme (ARQ) retransmits unsuccessfully delivered packets based on packet loss information collected from receivers within broadcasting range (See Figure 4.1). It has been shown that allowing a
broadcasting source to combine retransmission packet reduces the number of retransmission packets over the broadcast network [70,71]. Specifically, the number of retransmissions depends on the maximum number of packet losses among all receivers when linear network coding is applied for packet retransmissions. For example, suppose that there are \( r \) number of receivers in a single-hop broadcast network, and let \( R_j \) denote \( j \)-th receiver where \( 1 \leq j \leq r \). If a receiver \( R_j \) has been experienced \( e_j \) packet losses, then the number of retransmission packets for a broadcasting source to retransmit is \( \max_{\forall j} \{e_j\} \) for \( 1 \leq j \leq r \).

**Encoding**

With a deterministic linear network coding, every retransmission packet is linearly encoded by pre-determined coding coefficients. Using the deterministic linear network code defined in Section 4.1.2, an encoded \( j \)-th retransmission packet can be written as

\[
c_j = \sum_{i=0}^{k-1} p_i \alpha^{ij} \quad \text{for} \quad 0 \leq j \leq t - 1.
\]

(4.8)

where \( \alpha \) is a primitive element in \( GF(2^m) \) whose order is \( n = 2^m - 1 \) and \( t \) is the number of packets needed to retransmit (See Figure 4.2). The packet retransmission scheme with the deterministic network coding can be represented in matrix form as

\[
C_{s \times t} = P_{s \times k} G_{k \times t}
\]

(4.9)

where \( C_{s \times t} \) is \( s \times t \) matrix whose columns are linearly combined packets for retransmission, \( P_{s \times k} \) is \( s \times k \) matrix whose columns are uncoded packets, and \( G_{k \times t} \) is \( k \times t \) generator matrix of deterministic linear network code for retransmission scheme. Note that the generator matrix, \( G_{k \times t} \) is obtained by puncturing the last \( n - t \) columns of the generator matrix of
\( S \) = broadcasting source
\( R_j \) = \( j \)-th receiver, \( 1 \leq j \leq r \)
\( p_i \) = \( i \)-th packet \( 0 \leq i \leq k - 1 \)

(a) transmission of \( k \) packets

(b) collect feedbacks

(c) retransmission of \( t \) packets \( (t \leq k) \)

Figure 4.1: ARQ scheme
\((n, k, n - k + 1)\) RS code defined in (4.1),

\[
G_{k \times t} = \begin{pmatrix}
1 & 1 & 1 & \cdots & 1 \\
1 & \alpha & \alpha^2 & \cdots & \alpha^{t-1} \\
1 & \alpha^2 & (\alpha^2)^2 & \cdots & (\alpha^{t-1})^2 \\
\vdots & \vdots & \vdots & \ddots & \vdots \\
1 & \alpha^{k-1} & (\alpha^2)^{k-1} & \cdots & (\alpha^{t-1})^{k-1}
\end{pmatrix}.
\]

(4.10)

Decoding

Upon receiving encoded retransmission packets, since each receiver has knowledge of coding coefficients, retransmitted packets, and previously successfully received packets, lost packets can be recovered at each receiver by solving linear equations. Because every receiver has experienced a different number of lost packets and a different set of lost packets, each receiver has different demands on retransmission packets. Thus, the coding coefficients of linear transform have to be carefully chosen to ensure that packet retransmissions cover all demands of receivers.

Suppose that a receiver lost \(t\) packets and received \(t\) retransmission packets from a broadcasting source. Let \(f_1, f_2, \ldots, f_t\) denote the indexes for \(t\) lost packets and \(s_1, s_2, \ldots, s_{k-t}\) denote the indexes for the \(k - t\) successfully received packets where \(0 \leq f_1 < f_2 < \ldots < f_t \leq k - 1\) and \(0 \leq s_1 < s_2 < \ldots < s_{k-t} \leq k - 1\), then the \(t\) retransmitted packets can be
\( S = \) broadcasting source
\( R_h = h\)-th receiver, \( 1 \leq h \leq r \)
\( p_i = i\)-th packet \( 0 \leq i \leq k - 1 \)

(a) transmission of \( k \) packets

\( e_h = \text{no. of lost packets at } h\)-th receiver

(b) collect feedbacks

\( t = \max \{e_h\} \text{ for } 1 \leq h \leq r \)
\( c_j = \sum_{i=0}^{k-1} p_i \alpha^{ij} \text{ for } 0 \leq j \leq t - 1 \)

(c) packet retransmission using deterministic network code

Figure 4.2: Packet retransmission scheme with deterministic network coding
written as

\[(c_0, c_1, \ldots, c_{t-1}) = (p_0, p_1, \ldots, p_{k-1}) G_{k \times t}\]

\[= (p_0, p_1, \ldots, p_{k-1}) \begin{pmatrix} g_{0,0} & g_{0,1} & \cdots & g_{0,t-1} \\ g_{1,0} & g_{1,1} & \cdots & g_{1,t-1} \\ \vdots & \vdots & \ddots & \vdots \\ g_{k-1,0} & g_{k-1,1} & \cdots & g_{k-1,t-1} \end{pmatrix}, \text{ where } g_{i,j} = \alpha^{ij}\]

\[= (p_{s_1}, p_{s_2}, \ldots, p_{s_{k-t}}) \begin{pmatrix} g_{s_1,0} & g_{s_1,1} & \cdots & g_{s_1,t-1} \\ g_{s_2,0} & g_{s_2,1} & \cdots & g_{s_2,t-1} \\ \vdots & \vdots & \ddots & \vdots \\ g_{s_{k-t},0} & g_{s_{k-t},1} & \cdots & g_{s_{k-t},t-1} \end{pmatrix}\]

\[+ (p_{f_1}, p_{f_2}, \ldots, p_{f_t}) \begin{pmatrix} g_{f_1,0} & g_{f_1,1} & \cdots & g_{f_1,t-1} \\ g_{f_2,0} & g_{f_2,1} & \cdots & g_{f_2,t-1} \\ \vdots & \vdots & \ddots & \vdots \\ g_{f_t,0} & g_{f_t,1} & \cdots & g_{f_t,t-1} \end{pmatrix} \] (4.11)

Let the two separated coefficient matrices in (4.11) be $W_s$ and $W_f$ respectively, then

\[(c_0, c_1, \ldots, c_{t-1}) = (p_{s_1}, p_{s_2}, \ldots, p_{s_{k-t}}) W_s + (p_{f_1}, p_{f_2}, \ldots, p_{f_t}) W_f. \] (4.12)

Because the receiver knows all coding coefficients (i.e., $W_s$ and $W_f$), $t$ retransmitted packets \(\{c_0, c_1, \ldots, c_{t-1}\}\), and \(k - t\) successfully delivered packets \(\{p_{s_1}, p_{s_2}, \ldots, p_{s_{k-t}}\}\), the $t$ lost packets \(\{p_{f_1}, p_{f_2}, \ldots, p_{f_t}\}\) can be recovered by solving linear equations if the square matrix, $W_f$ is invertible.

Let $V_t(a_0, a_1, \ldots, a_{t-1})$ denote a $t \times t$ Vandermonde matrix with elements of $a_0, a_1, \ldots, a_{t-1}$,
then

\[ W_f^\top = V_t(\alpha^{f_1}, \alpha^{f_2}, \ldots, \alpha^{f_t}) \]

\[
= \begin{pmatrix}
1 & 1 & \cdots & 1 \\
\alpha^{f_1} & \alpha^{f_2} & \cdots & \alpha^{f_t} \\
\alpha^{f_1^2} & \alpha^{f_2^2} & \cdots & \alpha^{f_t^2} \\
\vdots & \vdots & \ddots & \vdots \\
\alpha^{f_1^{t-1}} & \alpha^{f_2^{t-1}} & \cdots & \alpha^{f_t^{t-1}}
\end{pmatrix}.
\]

(4.13)

Since \( \det(A^\top) = \det(A) \) where \( A \) is a square matrix,

\[
\det(W_f) = \det(W_f^\top)
\]

(4.14)

\[
= \det(V_t(\alpha^{f_1}, \alpha^{f_2}, \ldots, \alpha^{f_t}))
\]

\[
= \prod_{f_1 \leq i < j \leq f_t} (\alpha^j - \alpha^i).
\]

(4.15)

Since the elements, \( \alpha^{f_1}, \alpha^{f_2}, \ldots, \alpha^{f_t} \) are non-zero and distinct over \( \mathbb{GF}(2^m) \), the determinant of \( W_f \) is non-zero. Therefore, the matrix \( W_f \) is non-singular as required.

Now consider a case that a receiver requested \( e \) retransmission packets where \( e \) is less than \( t \) and the receiver successfully received \( e \) consecutively encoded retransmission packets.
\{c_h, c_{h+1}, \ldots, c_{h+e-1}\} \text{ where } 0 \leq h \leq t - e. \text{ For simplicity, we assume } h = 0, \text{ then }

(c_0, c_1, \ldots, c_{e-1}) = (p_{s_1}, p_{s_2}, \ldots, p_{s_{k-e}}) \begin{pmatrix} g_{s_1,0} & g_{s_1,1} & \cdots & g_{s_1,e-1} \\ g_{s_2,0} & g_{s_2,1} & \cdots & g_{s_2,e-1} \\ \vdots & \vdots & \ddots & \vdots \\ g_{s_{k-e},0} & g_{s_{k-e},1} & \cdots & g_{s_{k-e},t-1} \end{pmatrix} + (p_{f_1}, p_{f_2}, \ldots, p_{f_e}) \begin{pmatrix} g_{f_1,0} & g_{f_1,1} & \cdots & g_{f_1,e-1} \\ g_{f_2,0} & g_{f_2,1} & \cdots & g_{f_2,e-1} \\ \vdots & \vdots & \ddots & \vdots \\ g_{f_e,0} & g_{f_e,1} & \cdots & g_{f_e,e-1} \end{pmatrix}. \quad (4.16)

Similar to (4.12), \(e\) retransmitted packets can be written as

(c_0, c_1, \ldots, c_{e-1}) = (p_{s_1}, p_{s_2}, \ldots, p_{s_{k-e}}) W^s + (p_{f_1}, p_{f_2}, \ldots, p_{f_e}) W^f \quad (4.17)

where \(W^s\) and \(W^f\) are corresponding coefficient matrices. Because the determinant of \(W^f\) is equal to the determinant of \(V\(e\alpha_{f_1}, \alpha_{f_2}, \ldots, \alpha_{f_e}\), as long as \(e\) consecutively encoded packet are successfully delivered at the receiver, \(W^f\) is invertible. Therefore, the encoding based on Vandermonde matrix does guarantee to decode packets if a receiver (who requested \(e\) packet retransmissions) successfully receives \(e\) consecutively encoded retransmission packets where \(e\) is less than or equal to \(t\).
Example

Let $k = 4$, $s = 4$. Suppose

$$
P_{4 \times 4} = \begin{pmatrix}
1 & \alpha & 1 & 1 \\
1 & 1 & \alpha & \alpha^2 \\
\alpha^4 & \alpha & \alpha & \alpha^3 \\
\alpha^5 & 1 & \alpha^6 & \alpha^4 \\
\end{pmatrix}
$$

where $\alpha$ is a primitive element in $\mathbb{GF}(2^3)$ and is a root of the primitive polynomial $x^3 + x + 1$.

Assume that a broadcasting source collects feedbacks from receivers and there are at most 2 unsuccessfully delivered packets among all receivers within broadcasting range. Then the source needs to retransmit 2 linearly combined packets using (4.9):

$$
C_{4 \times 2} = P_{4 \times 4}G_{4 \times 2}
$$

$$
= \begin{pmatrix}
1 & \alpha & 1 & 1 \\
1 & 1 & \alpha & \alpha^2 \\
\alpha^4 & \alpha & \alpha & \alpha^3 \\
\alpha^5 & 1 & \alpha^6 & \alpha^4 \\
\end{pmatrix} \begin{pmatrix}
1 & 1 \\
1 & \alpha \\
\alpha^4 & \alpha^5 \\
\alpha^6 & \alpha^4 \\
\end{pmatrix} = \begin{pmatrix}
\alpha^3 & \alpha \\
\alpha^4 & \alpha^6 \\
\alpha^6 & \alpha^2 \\
\alpha^6 & \alpha^4 \\
\end{pmatrix}
$$

At the receiving end, each receiver wants to recover its lost packets from the linearly combined packets. For example, a receiver $R$ has $p_0 = (1, 1, \alpha^4, \alpha^5)^\top$ and $p_2 = (1, \alpha, \alpha, \alpha^6)^\top$
and wants to recover $p_1$ and $p_3$ from retransmitted packets. The linearly encoded retransmission packets can be represented by

$$(c_0, c_1) = (p_0, p_1, p_2, p_3) G_{4 \times 2}$$

$$= (p_0, p_2) \begin{pmatrix} g_{0,0} & g_{0,1} \\ g_{2,0} & g_{2,1} \end{pmatrix} + (p_1, p_3) \begin{pmatrix} g_{1,0} & g_{1,1} \\ g_{3,0} & g_{3,1} \end{pmatrix}$$

$$= \begin{pmatrix} 1 & 1 \\ 1 & \alpha \\ \alpha^4 & \alpha \\ \alpha^5 & \alpha^6 \end{pmatrix} \begin{pmatrix} 1 & 1 \\ 1 & \alpha^2 \end{pmatrix} + (p_1, p_3) \begin{pmatrix} 1 & \alpha \\ 1 & \alpha^3 \end{pmatrix}.$$ 

Since the receiver $R$ knows $p_0$, $p_2$, and $G_{4 \times 2}$,

$$(p_1, p_3) = \left\{ (c_0, c_1) + (p_0, p_2) \begin{pmatrix} 1 & 1 \\ 1 & \alpha^2 \end{pmatrix} \right\} \begin{pmatrix} 1 & \alpha \\ 1 & \alpha^3 \end{pmatrix}^{-1}$$

$$= \left\{ \begin{pmatrix} \alpha^3 & \alpha \\ \alpha^4 \alpha^5 \\ \alpha^6 \alpha^2 \\ \alpha^6 \alpha^4 \end{pmatrix} + \begin{pmatrix} 1 & 1 \\ 1 & \alpha \\ \alpha^4 & \alpha \\ \alpha^5 & \alpha^6 \end{pmatrix} \begin{pmatrix} 1 & 1 \\ 1 & \alpha^2 \end{pmatrix} \right\} \begin{pmatrix} 1 & \alpha \\ 1 & \alpha^3 \end{pmatrix}^{-1}$$

$$= \begin{pmatrix} \alpha & 1 \\ 1 & \alpha^2 \\ \alpha \alpha^3 \\ 1 & \alpha^4 \end{pmatrix}.$$ 

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4.2.2 Forward error corrections using deterministic network coding

Because a deterministic linear network code constructed by puncturing the generator matrix of RS code (4.7), the deterministic linear network coding for packet transmission can easily provide forward error corrections.

Encoding

In a single-hop broadcast network, a source broadcasts \( k + 2t \) linearly encoded packets to provide \( t \) packet-error-correction. Using the deterministic linear network code defined in Section 4.1.2, the packet encoding for forward error correction can be described by

\[
c_j = \sum_{i=0}^{k-1} p_i \alpha^{ij} \quad \text{for} \quad 0 \leq j \leq n' - 1,
\]

where \( \alpha \) is a primitive element in \( \mathbb{GF}(2^m) \) and \( n' = k + 2t \) (See Figure 4.3). A deterministic linear network coding model for forward error correction can also be expressed in matrix form,

\[
C_{s \times n'} = P_{s \times k} G_{k \times n'}
\]

where \( P_{s \times k} \) is a \( s \times k \) matrix whose columns are uncoded packets, \( C_{s \times n'} \) is a \( s \times n' \) matrix whose columns are encoded packets, and \( G_{k \times n'} \) is a \( k \times n' \) generator matrix for deterministic linear network code. Similar to the packet retransmission scheme, the generator matrix, \( G_{k \times n'} \) for forward error correction scheme is obtained from puncturing the last \( n - (k + 2t) \)
columns of the generator matrix in (4.1),

\[
G_{k \times n'} = \begin{pmatrix}
1 & 1 & 1 & \cdots & 1 \\
1 & \alpha & \alpha^2 & \cdots & \alpha^{n'-1} \\
1 & \alpha^2 & (\alpha^2)^2 & \cdots & (\alpha^{n'-1})^2 \\
\vdots & \vdots & \vdots & \ddots & \vdots \\
1&\alpha^{k-1}(\alpha^2)^{k-1} & \cdots & (\alpha^{n'-1})^{k-1}
\end{pmatrix}.
\]

(4.20)

**Theorem 4.1.** The deterministic linear network code generated by \(G_{k \times n'}\) guarantees to correct up to \(t\) packet errors where \(n' = k + 2t\).

**Proof.** Each encoded packet consists of \(s\) symbols over \(\mathbb{GF}(2^m)\) and any corrupted symbol in a packet would result in a packet error. Thus, \(t\)-packet-error affects \(t\) columns of \(C_{s \times n'}\) and it corrupts at most \(t\) symbols in each row of \(C_{s \times n'}\) (See Figure 4.3). Since rows of \(C_{s \times n'}\) are encoded with \((k + 2t, k, 2t + 1)\) punctured RS code, they can be corrected up to \(t\) symbols of errors. Therefore the deterministic linear network code generated by \(G_{k \times n'}\) guarantees to correct up to \(t\) packet errors where \(n' = k + 2t\). \(\Box\)

**Decoding**

Let \(R_{s \times n'}\) denote a \(s \times n'\) matrix whose columns are received packets, \(C_{s \times n'}\) denote a \(s \times n'\) matrix whose columns are transmitted packets and \(E_{s \times n'}\) denote a \(s \times n'\) matrix of errors introduced by broadcast channel. Then,

\[
R_{s \times n'} = C_{s \times n'} + E_{s \times n'}
\]

and

\[
r^*_h = c^*_h + e^*_h \quad \text{for} \quad 0 \leq h \leq s - 1
\]
\[
\begin{align*}
\begin{pmatrix}
\mathbf{c}_0, & \mathbf{c}_1, & \ldots, & \mathbf{c}_{n'-1}
\end{pmatrix}
\end{align*}
\]

(a) Packet transmission with \( t \)-error-correction capability

\[
\begin{align*}
\mathbf{n}' &= k + 2t \\
\mathbf{c}_j &= \sum_{i=0}^{k-1} \mathbf{p}_i \alpha^{ij} \quad \text{for} \quad 0 \leq j \leq n' - 1
\end{align*}
\]

(b) A block of encoded packets

Figure 4.3: Forward error correction scheme with deterministic network coding
where \( r^*_h = (r_{h,0}, r_{h,1}, \ldots, r_{h,(n'-1)}) \) and \( e^*_h = (e_{h,0}, e_{h,1}, \ldots, e_{h,(n'-1)}) \) denote a row vector of the received words and error vectors respectively.

Upon receiving \( \mathbf{R}_{s \times n'} \), row-by-row decoding is performed to correct packet errors. We can use standard error and erasure decoder for a \((n, k, n-k+1)\) RS code to decode punctured \((n', k, n'-k+1)\) RS code by treating the deleted columns as erasure positions.

Let the received polynomial be \( R_h(x) = r_{h,0} + r_{h,1}x + \ldots + r_{h,(n'-1)}x^{n'-1} \), then the standard error and erasure decoding procedures for the punctured RS code consist of the following:

1. Compute erasure location polynomial, \( \Gamma_h(x) \) for \( 0 \leq h \leq s-1 \),

\[
\Gamma_h(x) = \Gamma(x) = \prod_{i=n'}^{n-1} (1 - \alpha^i x).
\] (4.21)

2. Compute syndrome polynomial, \( S_h(x) \),

\[
S_h(x) = \sum_{j=1}^{n-k} s_{h,j} x^{(j-1)}
\] (4.22)

where \( s_{h,j} = r_h(\alpha^j) = \sum_{i=0}^{n'-1} r_{h,i}(\alpha^j)^i \) and \( 0 \leq h \leq s - 1 \).

3. Compute modified syndrome polynomial, \( \Theta_h(x) \),

\[
\Theta_h(x) = \Gamma_h(x) S_h(x) \mod x^{n-k}.
\] (4.23)

4. Key equation:

\[
\Lambda_h(x) \Theta_h(x) \equiv \Omega_h(x) \mod x^{n-k}
\] (4.24)

where \( \Lambda_h(x) \) is error location polynomial and \( \Omega_h(x) \) is error value polynomial.
5. Apply Euclid’s algorithm to solve the key equation and determine $\Lambda_h(x)$ and $\Omega_h(x)$.

6. Apply Forney’s algorithm to find error location and value

$$e_{hj} = \begin{cases} 
\frac{\Omega_h(\alpha^{-j})}{\Lambda_h(\alpha^{-j})} & : \text{if } \Lambda_h(\alpha^{-j}) = 0 \\
0 & : \text{otherwise}
\end{cases}$$

for $0 \leq j \leq n' - 1$ \hspace{1cm} (4.25)

7. Find the transmitted codeword, $c_h^*$. Suppose that the broadcast channel introduced less than $t$ packet errors. Through row-by-row decoding of the punctured RS code, each receiver can recover the encoded packets, $C_{s \times n'}$. Now consider a $s \times k$ sub-matrix of $C_{s \times n'}$ by deleting the last $n' - k$ columns and define as $C'_{s \times k}$, then

$$C'_{s \times k} = P_{s \times k} V_k(\alpha^0, \alpha^1, \ldots, \alpha^{k-1})$$

where $V_k(\alpha^0, \alpha^1, \ldots, \alpha^{k-1})$ is the $k \times k$ Vandermonde matrix. Since the elements of $V_k(\alpha^0, \alpha^1, \ldots, \alpha^{k-1})$ are non-zero and distinct over $\mathbb{GF}(2^m)$, $V_k(\alpha^0, \alpha^1, \ldots, \alpha^{k-1})$ has non-zero determinant. Therefore each receiver can recover the original packet information by solving linear equations: $P_{s \times k} = C'_{s \times k} V_k(\alpha^0, \alpha^1, \ldots, \alpha^{k-1})^{-1}$.

Example

Let $k = 3$ and $s = 4$. Suppose

$$P_{4 \times 3} = \begin{pmatrix}
1 & 1 & 1 \\
1 & \alpha & \alpha^2 \\
\alpha^4 & \alpha & \alpha^3 \\
\alpha^5 & \alpha^6 & \alpha^4
\end{pmatrix}$$

where $\alpha$ is a primitive element in $\mathbb{GF}(2^3)$ and is a root of the primitive polynomial $x^3 + x + 1$. 

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From (4.1), a (7, 3, 5) RS code can be generated by
\[
G_{RS} = G_{3 \times 7} = \begin{pmatrix}
1 & 1 & 1 & 1 & 1 & 1 \\
1 & \alpha & \alpha^2 & \alpha^3 & \alpha^4 & \alpha^5 & \alpha^6 \\
1 & \alpha^2 & \alpha^3 & \alpha^4 & \alpha^5 & \alpha^6 \\
\end{pmatrix}.
\]

Now assume that the broadcast channel needs single error correction capability. A (5, 3, 3) punctured single-error-correcting RS code can be generated by puncturing the last two columns of \(G_{3 \times 7}\),
\[
G_{3 \times 5} = \begin{pmatrix}
1 & 1 & 1 & 1 & 1 \\
1 & \alpha & \alpha^2 & \alpha^3 & \alpha^4 \\
1 & \alpha^2 & \alpha^4 & \alpha^6 & \alpha \\
\end{pmatrix}.
\]

Then, a broadcasting source obtains encoded packets:
\[
C_{4 \times 5} = P_{4 \times 3} G_{3 \times 5} = \begin{pmatrix}
1 & \alpha^5 & \alpha^3 & \alpha^5 & \alpha^6 \\
\alpha^5 & \alpha^3 & \alpha^5 & \alpha^6 & \alpha^6 \\
\alpha^5 & \alpha^6 & \alpha^2 & \alpha^2 & \alpha^5 \\
\alpha^2 & \alpha^3 & \alpha^5 & 0 & \alpha^3 \\
\end{pmatrix}.
\]

For a receiver in a broadcasting range, suppose that received encoded packets are
\[
R_{4 \times 5} = \begin{pmatrix}
1 & \alpha^5 & \alpha^3 & 1 & \alpha^6 \\
\alpha^5 & \alpha^3 & \alpha^5 & \alpha & \alpha^6 \\
\alpha^5 & \alpha^6 & \alpha^2 & \alpha & \alpha^5 \\
\alpha^2 & \alpha^3 & \alpha^5 & 1 & \alpha^3 \\
\end{pmatrix},
\]

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and each row of received words are

\[ r_0(x) = 1 + \alpha^5 x + \alpha^3 x^2 + x^3 + \alpha^6 x^4, \]

\[ r_1(x) = \alpha^5 + \alpha^3 x + \alpha^5 x^2 + \alpha x^3 + \alpha^6 x^4, \]

\[ r_2(x) = \alpha^5 + \alpha^6 x + \alpha^2 x^2 + \alpha x^3 + \alpha^5 x^4, \]

\[ r_3(x) = \alpha^2 + \alpha^3 x + \alpha^5 x^2 + x^3 + \alpha^3 x^4. \]

From (4.21), the erasure location polynomial is

\[ \Gamma_h(x) = (1 + \alpha^5 x)(1 + \alpha^6 x), \]

\[ = 1 + \alpha x + \alpha^4 x^2 \quad \text{for} \quad h = 0, 1, 2, 3. \]

Then a receiver can compute the syndrome polynomials using (4.22),

\[ S_0(x) = \alpha^3 + \alpha^6 x + \alpha^6 x^2 + \alpha^4 x^3, \]

\[ S_1(x) = \alpha^6 + \alpha^2 x + x^2 + \alpha^2 x^3, \]

\[ S_2(x) = \alpha + \alpha^2 x + x^2 + \alpha^3 x^3, \]

\[ S_3(x) = 1 + \alpha^2 x + x^2; \]
and the modified syndrome polynomials using (4.23),

\[ \Theta_0(x) = \alpha^3 + \alpha^3 x + \alpha^6 x^2 + \alpha^2 x^3, \]
\[ \Theta_1(x) = \alpha^6 + \alpha^6 x + x^2 + \alpha^3 x^3, \]
\[ \Theta_2(x) = \alpha + \alpha^6 x^2 + \alpha^2 x^3, \]
\[ \Theta_3(x) = 1 + \alpha^4 x + \alpha^2 x^2 + \alpha^5 x^3. \]

Using the Euclid’s algorithm, the error location polynomials and the error value polynomial can be obtained as

\[ \Lambda_0(x) = \alpha^2(1 + \alpha^3 x), \]
\[ \Lambda_1(x) = \alpha(1 + \alpha^3 x), \]
\[ \Lambda_2(x) = \alpha^2(1 + \alpha^3 x), \]
\[ \Lambda_3(x) = \alpha^6(1 + \alpha^3 x), \]

and

\[ \Omega_0(x) = \alpha^5 + \alpha^6 x, \]
\[ \Omega_1(x) = 1 + \alpha x + x^2, \]
\[ \Omega_2(x) = \alpha^3 + \alpha^6 x + \alpha x^2, \]
\[ \Omega_3(x) = \alpha^6 + \alpha^5 x + \alpha^5 x^2. \]
Then using (4.25) one can locate error position and its value, hence the error vectors are

\[
E_{4 \times 5} = \begin{pmatrix}
0 & 0 & 0 & \alpha^4 & 0 \\
0 & 0 & 0 & \alpha^5 & 0 \\
0 & 0 & 0 & \alpha^4 & 0 \\
0 & 0 & 0 & 1 & 0 \\
\end{pmatrix}.
\]

Finally, a receiver recovers the encoded packets,

\[
C_{4 \times 5} = R_{4 \times 5} + E_{4 \times 5}
\]

\[
= \begin{pmatrix}
1 & \alpha^5 & \alpha^3 & \alpha^5 & \alpha^6 \\
\alpha^5 & \alpha^3 & \alpha^5 & \alpha^6 & \alpha^6 \\
\alpha^6 & \alpha^4 & \alpha^2 & \alpha^2 & \alpha^5 \\
\alpha^2 & \alpha^4 & \alpha^5 & 0 & \alpha^3
\end{pmatrix}.
\]

Since a receiver recovers the encoded packets, one can now obtain the original packets by
multiplying inverse of the Vandermonde matrix;

\[
P_{4 \times 3} = C_{4 \times 3} \cdot V_{3 \times 3}^{-1}
\]

\[
\begin{pmatrix}
1 & \alpha^5 & \alpha^3 \\
\alpha^5 & \alpha^3 & \alpha^5 \\
\alpha^5 & \alpha^6 & \alpha^2 \\
\alpha^2 & \alpha^3 & \alpha^5
\end{pmatrix}
\begin{pmatrix}
\alpha & \alpha^2 & \alpha^4 \\
\alpha^2 & \alpha^6 & 1 \\
\alpha^5 & 1 & \alpha^4
\end{pmatrix}
\]

\[
\begin{pmatrix}
1 & 1 & 1 \\
1 & \alpha & \alpha^2 \\
\alpha^4 & \alpha & \alpha^3 \\
\alpha^5 & \alpha^6 & \alpha^4
\end{pmatrix}
\]

4.3 Numerical analysis and simulations

4.3.1 Analysis

Packet Losses

We assume that packet loss characteristics over a broadcast channel are independent and identical with a packet loss probability of \(p\) at each receiver, hence a transmitted packet is successfully received at a receiver with probability of \(1 - p\). Let \(\{X_i\}\) be a set of random variables which takes a value of 1 if \(i\)-th packet is not received successfully, or a value of 0 if \(i\)-th packet is received successfully for \(1 \leq i \leq k\),

\[
\Pr(X_i = 1) = p \quad \text{and} \quad \Pr(X_i = 0) = 1 - p. \quad (4.26)
\]

Let \(\{Y_j\}\) be a set of random variables denotes the number of lost packets for \(j\)-th receiver \(R_j\) where \(1 \leq j \leq r\), then \(Y_j\) is the sum of a set of \(\{X_i\}\) which follows a binomial distribution

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with parameters of \( k \) and \( p \),

\[
Y_j = \sum_{i=1}^{k} X_i
\]

(4.27)

and

\[
\Pr(Y_j = y) = \binom{k}{y} p^y (1-p)^{k-y}.
\]

(4.28)

We define a random variable \( Z \) to denote that the maximum number of unsuccessfully delivered packets among all receivers,

\[
Z = \max \{Y_1, Y_2, \ldots, Y_r\},
\]

(4.29)

then we have

\[
\Pr(Z \leq z) = \Pr(\max\{Y_1, Y_2, \ldots, Y_r\} \leq z)
\]

(4.30)

\[
= \prod_{i=1}^{r} \Pr(Y_i \leq z)
\]

(4.31)

\[
= \{\Pr(Y_i \leq z)\}^r.
\]

(4.32)

Therefore,

\[
\Pr(Z = z) = \Pr(Z \leq z) - \Pr(Z \leq z - 1)
\]

(4.33)

\[
= \prod_{i=1}^{r} \Pr(Y_i \leq z) - \prod_{i=1}^{r} \Pr(Y_i \leq z - 1)
\]

(4.34)

\[
= \{\Pr(Y_i \leq z)\}^r - \{\Pr(Y_i \leq z - 1)\}^r
\]

(4.35)
and

\[ E[Z] = \sum_{i=0}^{k} i \Pr(Z = i) \] \hspace{1cm} (4.36)

\[ = \Pr(Z = 1) + 2 \Pr(Z = 2) + \cdots + k \Pr(Z = k). \] \hspace{1cm} (4.37)

From (4.33) and (4.36), on average, there are at most \( E[Z] \) numbers of unsuccessfully delivered packets out of \( k \) transmitted packets among all receivers where

\[ E[Z] = k - \sum_{i=0}^{k-1} \Pr(Y \leq i)^r. \] \hspace{1cm} (4.38)

We numerically experiment with the packet losses. The results are depicted in Figure 4.4, Figure 4.5, Figure 4.6 and Figure 4.7. To evaluate the packet loss analysis, we simulate actual packet losses among receivers in a single-hop broadcast network and compare the simulation results with the analysis. The comparisons are shown in Figure 4.8.
Figure 4.5: $E[Z]$ versus number of receivers, $r$.

Figure 4.6: $E[Z]$ versus number of transmitted packets, $k$. 
Figure 4.7: Contours of $E[Z]$.

Figure 4.8: Comparison results: theory versus simulation.
Traditional ARQ scheme

For comparison, we review the average number of transmissions required for traditional ARQ scheme. Let $N_{ARQ}$ denote the average number of transmissions required for ARQ scheme, $r$ be the number of receivers, $p$ be the probability of packet loss at each receiver, and $P_{success}$ be the probability that a retransmission packet is successfully delivered at all receivers. Then,

$$N_{ARQ} = P_{success} + (1 + N_{ARQ}) \times (1 - P_{success}).$$

(4.39)

By solving the above recursive equation, we have

$$N_{ARQ} = \frac{1}{P_{success}}.$$

(4.40)

Under the assumption that the packet loss is independent and identical among all receivers,

$$P_{success} = (1 - p)^r.$$

(4.41)

Therefore,

$$N_{ARQ} = \frac{1}{(1 - p)^r}.$$

(4.42)

Retransmissions Scheme

For an analysis of retransmission scheme, we assume that each receiver sends ACK/NAKs to its source based on current success or failure of packet receptions regardless of success/failure of previous retransmission attempts (i.e., memoryless receiver). Let $N_{RET}$ denote the average number of transmissions required to successfully deliver a packet with retransmission scheme, $r$ be the number of receivers, and $p$ be the packet loss rate.

Proposition 4.1. If $t$ packets are unsuccessfully delivered out of $k$ packet transmissions, the average number of transmissions required to deliver a packet with network coded packet
Retransmission is

\[ N_{RET} = 1 + \frac{t}{k(1 - p)^{tr}} \quad (4.43) \]

where \(0 < t \leq k\).

**Proof.** Let \(T_{RET}\) denote the total number of retransmissions for \(t\) unsuccessfully delivered packets, \(P_{success}\) be the probability that the retransmission packets are successfully delivered to all receiver. Then,

\[ T_{RET} = t \times P_{success} + (t + T_{RET}) \times (1 - P_{success}). \quad (4.44) \]

By solving the above recursive equation, we have

\[ T_{RET} = \frac{t}{P_{success}}. \quad (4.45) \]

Under the assumption that the packet loss is independent and identical among all receivers,

\[ P_{success} = (1 - p)^{tr}. \quad (4.46) \]

From (4.45) and (4.46),

\[ T_{RET} = \frac{t}{(1 - p)^{tr}}. \quad (4.47) \]

Therefore,

\[ N_{RET} = \frac{k + T_{RET}}{k} = 1 + \frac{t}{k(1 - p)^{tr}}. \]

\[ \square \]
Forward Error Correction scheme

Let $N_{FEC}$ denote the average number of transmissions required to successfully deliver a packet when forward error correction scheme is used with deterministic linear network coding.

**Proposition 4.2.** Assume that there are $t$ unsuccessfully delivered packets out of $k$ broadcasting packets. The average number of transmissions required to deliver a packet for forward error correction scheme with deterministic linear network coding is

$$N_{FEC} = 1 + 2 \frac{t}{k}$$  

(4.48)

where $0 < t \leq k$.

*Proof.* For the forward error correction scheme using deterministic network coding, a broadcast source transmit $n'$ encoded packets using $(n', k, n' - k + 1)$ punctured RS code to correct $t$ packet errors, where $n' = k + 2t$. Since $n'$ is the number of transmission required to transmit $k$ packets while providing $t$-error correction capability, the average number of transmissions for successfully delivering a packet can be given by $N_{FEC} = \frac{n'}{k} = 1 + 2 \frac{t}{k}$. □

### 4.3.2 Numerical results

We experiment numerically to evaluate the theoretical analysis of the expected number of transmissions to successfully deliver a packet in a single-hop wireless broadcast network. Both forward error correction scheme and retransmission scheme apply deterministic network coding for packet transmissions.

Figures 4.9 and 4.10 show the expected number of transmissions for delivering a packet with varying packet error probability, $p$, varying the number of packets for a broadcasting source to transmit, $k$, and varying the number of receivers within broadcasting range, $r$. Given $k$, $r$, and $p$, the maximum number of unsuccessfully delivered packets over the single-hop broadcast network among $r$ receivers are calculated as $t = E[Z]$ (4.38).
Figure 4.9: Expected no. of transmission vs. packet error probability
Figure 4.10: Expected no. of transmission vs. no. of receivers
We observe that the expected number of transmissions for retransmission scheme increases rapidly as $p$, $k$, or $r$ increases. On the other hand, the expected number of transmissions for forward error correction scheme remains small even if the packet error probability, the number of packets to transmit, or the number of receivers are large.

We also simulate the expected number of transmissions in a single-source, single-hop broadcast network to compare with the results of numerical analysis. Figure 4.11 shows the comparisons between analysis and simulation results for traditional ARQ scheme, retransmission scheme, and forward error correction scheme.

### 4.4 Discussions: unequal error protection using network coding

Theoretical analysis presented in this chapter assumes that error characteristics at all receivers in the broadcast network are identical. In the following, we provide an example of unequal error protection on a clustered broadcast network by using the proposed deterministic network coding in a hybrid way.

#### Unequal error protection with hybrid-ARQ scheme using network coding

Consider a clustered broadcast network in Figure 4.12, a single source has $k$ packets to broadcast to receiver $R_1$ to $R_{x+y}$. Assume that the broadcast channel degrades signals physically, packet losses at receivers in the inner cluster is smaller than packet losses at receivers in the outer cluster (i.e., $p_1 < p_2$). To deal with the unequal error characteristics at receivers, we use the deterministic network coding for hybrid-ARQ (i.e., first apply forward error correction scheme with the proposed network code to recover lost packets at the receivers in the inner cluster, then apply network coded retransmissions in the outer cluster). The network coded packet transmissions for unequal error protection on the clustered broadcast network are described with the following steps:
Figure 4.11: Comparison result: numerical analysis vs. simulation
1. Send network coded packets with forward error correction capability

The idea of unequal protection scheme is to recover packet losses at the receivers in the inner cluster with forward error correction and reduce the retransmission requests from the receivers in the outer cluster. The forward error correction scheme with deterministic network coding assumes that there is no help of error detection from lower layer. However, since we provide scheme that forward error correction and retransmission work together in a hybrid way, it seems that involvement of packet error detection from the lower layer is useful to the unequal error protection scheme. If CRC detects which packet comes with error, then the error location in the received packets are known to the receiver. In Theorem 4.1, we prove that network coded $k+2t$ packets correct up to $t$ packet errors, but, with given error locations on packets, only $k + t$ encoded packets are needed to correct $t$ packet erasures [52].

With the clustered broadcast network, a source transmits $k + t_1$ encoded packets to recover $t_1$ packet erasures where $t_1$ denotes the number of packet losses at the inner cluster’s receivers. From (4.18), a packet encoding for forward error correction using the proposed deterministic network code can be described by

$$c_j = \sum_{i=0}^{k-1} p_i \alpha^{ij} \quad \text{for} \quad 0 \leq j \leq k + t_1 - 1, \quad (4.49)$$
where $\alpha$ is a primitive element in $\mathbb{GF}(2^m)$.

2. Collect feedbacks from receivers

Suppose packet losses at the receivers in the inner cluster is at most $t_1$ and at the receivers in the outer cluster is at most $t_2$. Since $k + t_1$ encoded packets can recover all packet erasures at the receivers in the inner cluster, packet retransmission depends only on the feedbacks from receivers in the outer cluster.

3. Send network coded packet for retransmission

Based on the collected feedbacks from receivers, the broadcasting source knows that receivers in the inner cluster successfully received $k$ packets. The source also knows that there are at most $t_2$ packet losses among receivers in the outer cluster. However, since the source initially broadcast $k + t_1$ packets, the receivers in the outer cluster successfully received at least $k - (t_2 - t_1)$ packets. Therefore the broadcasting source needs to retransmit $k - (k - (t_2 - t_1)) = t_2 - t_1$ packets for receivers in the outer cluster in order to deliver $k$ packets.

Let $f_1, f_2, \ldots, f_{t_2}$ be indexes for the $t_2$ unsuccessfully delivered packets to receivers in the outer cluster where $f_1 < f_2 < \ldots < f_{t_2}$, then a packet encoding for retransmission with the proposed deterministic network code using (4.8) can be described by

$$c_j = \sum_{i=0}^{k-1} p_i \alpha^{ij} \text{ for } f_1 \leq j \leq f_{t_2 - t_1}. \quad (4.50)$$

As we have shown in the above example, both forward error correction scheme and retransmission scheme can adaptively work together to provide unequal error protection. Since we have limited our focus on a special case of the clustered broadcast network, an application of the hybrid ARQ scheme in general broadcast networks would be an interesting subject to research.
Chapter 5: Summary and future works

Error controls are important techniques for reliable communications over noisy channels. When information is corrupted by channel errors, the error control techniques are employed either to retransmit the corrupted information based on feedback (ARQ), or to correct the channel errors using error correcting codes (FEC). In this dissertation, we have investigated methodologies of both a retransmission scheme and a forward error correction scheme.

Unequal error protection (UEP) codes have been considered as an efficient error correction method when information has levels of significance. For multiuser communications over a broadcast channel, we have proposed a UEP coding scheme for a multiuser broadcast channel. First, we have introduced an integer programming approach to construct a binary UEP code. For a given unequal error protection requirement from each user, we have formulated an integer programming problem to be optimized for constructing an optimal UEP code. Numerical results and integer programming bounds have shown the efficiency of the code constructions. Also, we have investigated asymptotically achievable code rates for the multiuser communications and we have analyzed performance of the UEP coding schemes for the multiuser communications on degraded broadcast channels. Then, we have presented decoding methods that use integer programming and majority logic. When users receive information that is encoded by the UEP code, each user uses iterative integer programming to find sufficient numbers of index subsets so that each receiver can decode the information by majority logic. We have found that the UEP coding and decoding based on integer programming effectively provide unequal error protection to each user in broadcast communications.

For reliable packet transmissions over a single-hop broadcast network, we have applied a linear network coding into both a retransmission scheme and a forward error correction scheme. We have first constructed a deterministic network code from a Reed-Solomon error
correcting code whose generator matrix is in the form of Vandermonde matrix. Then, we have provided an adaptive way to apply the deterministic network code for both a packet retransmission scheme and a packet-level forward error correction scheme by puncturing the generator matrix. For forward error correction scheme, we have constructed a generator matrix by puncturing the last \( n - (k + 2t) \) columns of the generator matrix of a \((n, k, n-k+1)\) RS code to correct \( t \) packet errors. On the other hand, retransmission packets are generated by puncturing the last \( n-t \) columns of the generator matrix of a \((n, k, n-k+1)\) RS code for \( t \) packet retransmissions. Therefore, we have found a unified solution to use the deterministic linear network code for reliable packet transmissions on a single-hop wireless broadcast network. We have provided the numerical analysis and simulation results to prove the efficiency of applying the deterministic network code for packet transmissions, and we have also shown that the unified solution can be applied in a hybrid fashion to provide efficient error controls.

### 5.1 Future works

In Section 3.3.2, we have discussed decodability of the proposed iterative decoding method that uses multiple integer programming and majority logic, and we have shown that not every optimal UEP code constructed by the proposed integer programming approach is decodable by the decoding method. We have also provided an idea of the modified integer programming approach to construct UEP codes that are majority-logic-decodable (i.e., received information can be decomposed into sufficient number of subsets that are decodable by majority logic). However, the modified integer programming approach in Section 3.3.2 does not guarantee to construct optimal UEP codes because of the additional constraints.

Based on what we have found, we would like to extend our research to find a UEP code construction method such that the codes are majority-logic-decodable and has optimal length. Currently, we focus on the following research directions:

1. Solution filtering: As it has been noted in Section 3.1.2, there are many optimal
solutions from integer programming for a UEP code construction that satisfies a given unequal error protection requirement. Suppose there are certain linear constraints that validate the decodability of each optimal solution. Then, every optimal solutions can be filtered by the additional constraints to obtain majority-logic-decodable UEP codes. Therefore, research objective would be finding the constraints for filtering solutions.

2. Modifying integer programming problem: The solution filtering approach ensures that the filtered solution constructs an optimal UEP code. However, since finding every or large numbers of optimal solutions from integer programming has to precede the filtering, the amount of computation time will be increased. Therefore, modifying an integer programming problem by adding linear constraints is preferred especially when $k$ is large. Since, as pointed out, the additional constraints may change the optimal value of the solution, research objective would be finding the additional constraints for integer programming that validate decodability and optimality of the UEP code constructions.
Appendix A: Generator matrices of optimal UEP codes

Single-bit message  Let $G$ be a generator matrix of the optimal UEP codes constructed from Table 3.2, and $\hat{s} = (\hat{s}_1, \hat{s}_2, \ldots, \hat{s}_k)$ be the corresponding separation vector obtained from the generator matrix.

1. $k = 2$

Integer programming solution

\[
\begin{array}{ccc}
  x_1 & x_2 & x_3 \\
  4 & 2 & 1 \\
\end{array}
\]

Generator matrix

\[
G = \begin{pmatrix}
  0 & 0 & 0 & 1 & 1 & 1 & 1 \\
  1 & 1 & 1 & 0 & 0 & 1 & 0 \\
\end{pmatrix}
\]

Separation vector

$\hat{s} = (3, 5)$

Disjoint subsets

$\mathcal{J}(1) = \{\{5\}, \{6\}, \{4, 7\}\}$

$\mathcal{J}(2) = \{\{1\}, \{2\}, \{3\}, \{4\}, \{6, 7\}\}$

where $\mathcal{J}(i) \triangleq \{\mathcal{J}_1, \mathcal{J}_2, \ldots, \mathcal{J}_{s_i}\}$ for $1 \leq i \leq k$. 
2. $k = 3$

Integer programming solution

\[
\begin{array}{ccccccc}
  x_1 & x_2 & x_3 & x_4 & x_5 & x_6 & x_7 \\
  3 & 2 & 2 & 1 & 1 & 1 & 1 \\
\end{array}
\]

Generator matrix

\[
G = \begin{pmatrix}
  0 & 0 & 0 & 0 & 0 & 0 & 0 & 1 & 1 & 1 \\
  0 & 0 & 1 & 1 & 1 & 1 & 0 & 0 & 1 & 1 \\
  1 & 1 & 1 & 0 & 0 & 1 & 1 & 0 & 1 & 0 \\
  1 & 1 & 0 & 0 & 1 & 1 & 0 & 1 & 0 & 1 \\
\end{pmatrix}
\]

Separation vector

\[
\hat{s} = (4, 6, 7)
\]

Disjoint subsets

\[
J(1) = \{\{8\}, \{5,10\}, \{7,11\}\}
\]

\[
J(2) = \{\{4\}, \{5\}, \{8,10\}, \{1,6\}, \{9,11\}\}
\]

\[
J(3) = \{\{1\}, \{2\}, \{3\}, \{8,9\}, \{4,6\}, \{10,11\}, \{5,7\}\}
\]
3. \( k = 4 \)

Integer programming solution

\[
\begin{array}{cccccccccccccccc}
& x_1 & x_2 & x_3 & x_4 & x_5 & x_6 & x_7 & x_8 & x_9 & x_{10} & x_{11} & x_{12} & x_{13} & x_{14} & x_{15} \\
\hline
2 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1
\end{array}
\]

Generator matrix

\[
G = \begin{pmatrix}
0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 \\
0 & 0 & 0 & 1 & 1 & 1 & 1 & 0 & 0 & 0 & 1 & 1 & 1 & 1 & 1 & 1 \\
0 & 1 & 1 & 0 & 0 & 1 & 1 & 0 & 0 & 1 & 1 & 0 & 0 & 1 & 1 & 1 \\
1 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 \\
\end{pmatrix}
\]

Separation vector

\[
\hat{s} = (8, 8, 8, 9)
\]

Disjoint subsets

\[
\mathcal{J}(1) = \{9\}, \{3, 11\}, \{4, 12\}
\]

\[
\mathcal{J}(2) = \{5\}, \{11, 15\}, \{10, 14\}, \{4, 8\}, \{1, 6\}
\]

\[
\mathcal{J}(3) = \{3\}, \{13, 15\}, \{10, 12\}, \{6, 8\}, \{14, 16\}, \{2, 4\}, \{5, 7\}
\]

\[
\mathcal{J}(4) = \{1\}, \{2\}, \{13, 14\}, \{11, 12\}, \{7, 8\}, \{15, 16\}, \{3, 4\}, \{5, 6\}, \{9, 10\}
\]
4. \( k = 5 \)

Integer programming solution

\[
\begin{array}{cccccccccccccccc}
 x_1 & x_2 & x_3 & x_4 & x_5 & x_6 & x_7 & x_8 & x_9 & x_{10} & x_{11} & x_{12} & x_{13} & x_{14} & x_{15} & x_{16} & x_{17} & x_{18} & x_{19} \\
 2 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1
\end{array}
\]

Generator matrix

\[
G = \begin{pmatrix}
000000000000000111 \\
000000011111111000 \\
000111100001111000 \\
0110011001100110011 \\
1101010101010101010
\end{pmatrix}
\]

Separation vector

\[
\hat{s} = (4, 8, 8, 10, 11)
\]

Disjoint subsets

\[
\mathcal{J}(1) = \{\{17\}, \{4, 20\}, \{1, 18\}\}
\]

\[
\mathcal{J}(2) = \{\{9\}, \{7, 15\}, \{6, 14\}, \{4, 12\}, \{1, 10\}\}
\]

\[
\mathcal{J}(3) = \{\{5\}, \{11, 15\}, \{10, 14\}, \{4, 8\}, \{1, 6\}, \{3, 7\}, \{9, 13\}\}
\]

\[
\mathcal{J}(4) = \{\{3\}, \{17, 19\}, \{13, 15\}, \{10, 12\}, \{6, 8\}, \{14, 16\}, \{2, 4\}, \{5, 7\}, \{9, 11\}\}
\]

\[
\mathcal{J}(5) = \{\{1\}, \{2\}, \{17, 18\}, \{7, 8\}, \{13, 14\}, \{11, 12\}, \{15, 16\}, \{3, 4\},
\{5, 6\}, \{9, 10\}, \{19, 20\}\}
\]

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5. $k = 6$

Integer programming solution

\[
\begin{array}{ccccccccccccccccccc}
\hspace{2cm} & x_1 & x_2 & x_3 & x_4 & x_5 & x_6 & x_7 & x_8 & x_9 & x_{10} & x_{11} & x_{12} & x_{13} & x_{14} & x_{15} & x_{16} & x_{17} & x_{18} & x_{19} & x_{20} \\
\hline
1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 \\
\end{array}
\]

\[
\begin{array}{ccccccccccccccccccc}
\hspace{2cm} & x_{21} & x_{32} & x_{33} & x_{34} & x_{35} \\
\hline
1 & 1 & 1 & 1 & 1 \\
\end{array}
\]

Generator matrix

\[
G = \begin{pmatrix}
0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 1 & 1 & 1 & 1 \\
0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 1 & 1 & 1 & 1 & 1 & 1 & 1 \\
0 & 0 & 0 & 0 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 \\
0 & 0 & 1 & 1 & 1 & 1 & 0 & 0 & 0 & 0 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 \\
0 & 1 & 1 & 0 & 0 & 0 & 1 & 1 & 0 & 0 & 1 & 1 & 0 & 0 & 1 & 1 & 0 & 0 & 1 & 1 & 0 & 0 & 1 & 1 \\
1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 & 1 & 0 \\
\end{pmatrix}
\]

Separation vector

\[
\hat{s} = (4, 6, 8, 10, 12, 13)
\]
Disjoint subsets

\[ \mathcal{J}(1) = \{\{22\}, \{1, 23\}, \{2, 24\}\} \]

\[ \mathcal{J}(2) = \{\{16\}, \{5, 21\}, \{1, 17\}, \{3, 19\}, \{2, 18\}\} \]

\[ \mathcal{J}(3) = \{\{8\}, \{4, 12\}, \{3, 11\}, \{7, 15\}, \{1, 9\}, \{2, 10\}, \{5, 13\}\} \]

\[ \mathcal{J}(4) = \{\{4\}, \{3, 7\}, \{1, 5\}, \{2, 6\}, \{8, 12\}, \{10, 14\}, \{9, 13\}, \{11, 15\}, \{16, 20\}\} \]

\[ \mathcal{J}(5) = \{\{2\}, \{16, 18\}, \{1, 3\}, \{5, 7\}, \{4, 6\}, \{8, 10\}, \{12, 14\}, \{9, 11\}, \{13, 15\}, \{17, 19\}, \{22, 24\}\} \]

\[ \mathcal{J}(6) = \{\{1\}, \{6, 7\}, \{2, 3\}, \{4, 5\}, \{8, 9\}, \{10, 11\}, \{12, 13\}, \{14, 15\}, \{16, 17\}, \{18, 19\}, \{20, 21\}, \{22, 23\}, \{24, 25\}\} \]
6. \( k = 7 \)

Integer programming solution

\[
\begin{array}{cccccccccccccccccccc}
   x_1 & x_2 & x_3 & x_4 & x_5 & x_6 & x_7 & x_8 & x_9 & x_{10} & x_{11} & x_{12} & x_{13} & x_{14} & x_{15} & x_{16} & x_{17} & x_{18} & x_{19} & x_{20} \\
   1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 \\
   x_{21} & x_{22} & x_{23} & x_{32} & x_{33} & x_{34} & x_{35} & x_{64} & x_{65} & x_{104} \\
   1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 \\
\end{array}
\]

Generator matrix

\[
G = \begin{pmatrix}
000000000000000000000000111 \\
00000000000000000000000111101 \\
0000000000000000001111111000000 \\
00000001111111110000000000001 \\
001111100001111000111110000000 \\
01100110011001100110011001100100 \\
10101010101010101010101010101010
\end{pmatrix}
\]

Separation vector

\[
\hat{s} = (3, 5, 8, 9, 12, 14, 15)
\]
Disjoint subsets

\[ J(1) = \{\{28\}, \{1, 29\}, \{8, 24, 30\}\} \]

\[ J(2) = \{\{24\}, \{1, 25\}, \{2, 26\}, \{3, 27\}, \{8, 28, 30\}\} \]

\[ J(3) = \{\{16\}, \{3, 19\}, \{7, 23\}, \{2, 18\}, \{1, 17\}, \{4, 20\}, \{5, 21\}\} \]

\[ J(4) = \{\{8\}, \{1, 9\}, \{5, 13\}, \{4, 12\}, \{2, 10\}, \{3, 11\}, \{6, 14\}, \{7, 15\}, \{24, 28, 30\}\} \]

\[ J(5) = \{\{4\}, \{17, 21\}, \{11, 15\}, \{8, 12\}, \{18, 22\}, \{1, 5\}, \{3, 7\}, \{2, 6\}, \{10, 14\}, \{9, 13\}, \{16, 20\}\} \]

\[ J(6) = \{\{2\}, \{4, 6\}, \{12, 14\}, \{1, 3\}, \{5, 7\}, \{8, 10\}, \{9, 11\}, \{16, 18\}, \{17, 19\}, \{20, 22\}, \{13, 15\}, \{21, 23\}, \{24, 26\}\} \]

\[ J(7) = \{\{1\}, \{14, 15\}, \{22, 23\}, \{8, 9\}, \{12, 13\}, \{6, 7\}, \{18, 19\}, \{20, 21\}, \{4, 5\}, \{16, 17\}, \{26, 27\}, \{2, 3\}, \{10, 11\}, \{24, 25\}, \{28, 29\}\} \]
7. \( k = 8 \)

Integer programming solution

| \( x_1 \) | \( x_2 \) | \( x_3 \) | \( x_4 \) | \( x_5 \) | \( x_6 \) | \( x_7 \) | \( x_8 \) | \( x_9 \) | \( x_{10} \) | \( x_{11} \) | \( x_{12} \) | \( x_{13} \) | \( x_{14} \) | \( x_{15} \) | \( x_{16} \) | \( x_{17} \) | \( x_{18} \) | \( x_{19} \) | \( x_{20} \) |
| 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 | 1 |

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<th>( x_{23} )</th>
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</tr>
</tbody>
</table>

Generator matrix

\[
G = \begin{pmatrix}
0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 0 & 1 & 1 & 1
\end{pmatrix}
\]

Separation vector

\[
\hat{s} = (3, 5, 7, 11, 11, 13, 15, 17)
\]
Disjoint subsets

\[ \mathcal{J}(1) = \{\{33\}, \{1, 34\}, \{8, 16, 24, 35\}\} \]

\[ \mathcal{J}(2) = \{\{28\}, \{1, 29\}, \{2, 30\}, \{6, 31, 33, 35\}, \{12, 16, 27, 32\}\} \]

\[ \mathcal{J}(3) = \{\{24\}, \{2, 26\}, \{1, 25\}, \{3, 27\}\} \]

\[ \{14, 16, 28, 31\}, \{10, 20, 29, 32\}, \{7, 13, 18, 33, 35\}, \} \]

\[ \mathcal{J}(4) = \{\{16\}, \{7, 23\}, \{1, 17\}, \{6, 22\}, \{2, 18\}, \}

\[ \{3, 19\}, \{4, 20\}, \{5, 21\}, \{12, 24, 30, 31\}\} \]

\[ \mathcal{J}(5) = \{\{8\}, \{7, 15\}, \{1, 9\}, \{6, 14\}, \{2, 10\}, \{4, 12\}, \{3, 11\}, \}

\[ \{5, 13\}, \{20, 24, 30, 31\}, \{21, 26, 28, 32\}, \{16, 18, 19, 25, 33, 35\}\} \]

\[ \mathcal{J}(6) = \{\{4\}, \{9, 13\}, \{11, 15\}, \{2, 6\}, \{10, 14\}, \}

\[ \{3, 7\}, \{1, 5\}, \{8, 12\}, \{16, 20\}, \{18, 22\}, \}

\[ \{17, 21\}, \{19, 23\}, \{30, 31, 33, 35\}\} \]

\[ \mathcal{J}(7) = \{\{2\}, \{1, 3\}, \{25, 27\}, \{9, 11\}, \{24, 26\}, \}

\[ \{5, 7\}, \{4, 6\}, \{8, 10\}, \{12, 14\}, \{13, 15\}, \]

\[ \{16, 18\}, \{17, 19\}, \{20, 22\}, \{21, 23\}, \{28, 30\}\} \]

\[ \mathcal{J}(8) = \{\{1\}, \{6, 7\}, \{8, 9\}, \{33, 34\}, \{14, 15\}, \{10, 11\}, \}

\[ \{4, 5\}, \{12, 13\}, \{28, 29\}, \{24, 25\}, \{20, 21\}, \{18, 19\}, \]

\[ \{2, 3\}, \{16, 17\}, \{22, 23\}, \{26, 27\}, \{31, 32\}\} \]
Multi-bit message  Let $G$ be a generator matrix of the optimal UEP codes constructed from Table 3.5, and $\hat{s} = (\hat{s}_1, \hat{s}_2, \ldots, \hat{s}_k)$ be the corresponding separation vector with respect to the $G$.

1. $k = 2$ and $l = 2$

   Integer programming solution

   $x_1 \ x_2 \ x_3 \ x_4 \ x_5 \ x_7 \ x_8 \ x_9 \ x_{10} \ x_{11}$
   \[1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \]

   Generator matrix

   $G = \begin{pmatrix} 0 & 0 & 0 & 0 & 1 & 1 & 1 & 1 & 1 & 1 \\ 0 & 0 & 1 & 1 & 1 & 0 & 0 & 0 & 0 & 0 \\ 0 & 1 & 1 & 0 & 0 & 1 & 0 & 0 & 1 & 1 \\ 1 & 0 & 1 & 0 & 1 & 1 & 0 & 1 & 0 & 1 \\ 0 & 1 & 0 & 1 & 1 & 0 & 1 & 0 & 0 & 0 \\ 1 & 0 & 1 & 1 & 0 & 1 & 0 & 1 & 0 & 1 \end{pmatrix}$

   Separation vector

   $\hat{s} = (3, 5)$

2. $k = 3$ and $l = 2$

   Integer programming solution

   $x_1 \ x_2 \ x_4 \ x_5 \ x_6 \ x_8 \ x_9 \ x_{10} \ x_{11} \ x_{16} \ x_{17} \ x_{19} \ x_{32} \ x_{35} \ x_{47} \ x_{61}$
   \[1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \ 1 \]

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Generator matrix

\[
G = \begin{pmatrix}
0000000000001111 \\
0000000001111001 \\
0000000000010011 \\
000000111000001 \\
001110000000001 \\
0100100110010110 \\
1001001010101011
\end{pmatrix}
\]

Separation vector

\[\hat{s} = (4, 5, 7)\]

3. \(k = 2\) and \(l = 3\)

Integer programming solution

\[
\begin{array}{cccccccccc}
 x_1 & x_2 & x_3 & x_4 & x_5 & x_6 & x_7 & x_8 & x_{16} & x_{34} & x_{54} & x_{61} \\
1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1
\end{array}
\]

Generator matrix

\[
G = \begin{pmatrix}
0000000001111 \\
0000000010011 \\
0000000100101 \\
0000001001111 \\
0011100000010 \\
0110011000010 \\
1010101000001
\end{pmatrix}
\]

Separation vector

\[\hat{s} = (3, 5)\]
4. \( k = 2 \) and \( l = 4 \)

Integer programming solution

\[
\begin{array}{cccccccccccccccc}
  x_1 & x_2 & x_4 & x_7 & x_8 & x_{11} & x_{13} & x_{14} & x_{16} & x_{32} & x_{64} & x_{127} & x_{128} & x_{179} & x_{213} \\
  1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 & 1 \\
\end{array}
\]

Generator matrix

\[
\begin{pmatrix}
0000000000011111 \\
00000000011001 \\
00000000101010 \\
00000001001011 \\
00001111000100 \\
00110011000100 \\
01010101000101 \\
100101100001011
\end{pmatrix}
\]

Separation vector

\[
\hat{s} = (3, 5)
\]
Appendix B: Derivation of (3.105)

From the integer programming formulation, we have \( \frac{q^{k-1}}{q-1} \) inequalities in the form of

\[
Ax^\top \geq b^\top.
\]

Since each column of \( A \) has \( q^{k-1} \) ones, the sum of \( \frac{q^{k-1}}{q-1} \) inequalities can be given by

\[
q^{k-1}(x_1 + \cdots + x_{q^{k-1}}) \geq s_1 + qs_2 + \cdots + q^{(k-1)}s_k,
\]

hence,

\[
q^{k-1} n \geq \sum_{i=1}^{k} q^{i-1} s_i. \tag{B.1}
\]

By applying ceiling functions for integer property,

\[
n \geq \sum_{i=1}^{k} \left\lceil \frac{q^{i-1}}{q^{k-1}} s_i \right\rceil. \tag{B.2}
\]

Therefore,

\[
n \geq \sum_{i=1}^{k} \left\lceil \frac{s_i}{q^{k-i}} \right\rceil.
\]
Bibliography


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Curriculum Vitae

Wook Jung received his Bachelor of Science in Information and Computer Engineering in 2000 from Ajou University, Republic of Korea. He then pursued graduate studies at George Mason University, Fairfax, VA, where he received his Master of Science in Computer Engineering in 2003. His main research interests lie in efficient error control coding for improving network performance. More generally, his interests lie in both theoretical and practical aspects of communication networks.